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## THESIS

AUTOMATED POLE PLACEMENT ALGORITHM  
FOR MULTIVARIABLE OPTIMAL CONTROL SYNTHESIS

by

Chow, Wah Keh  
September 1985

Thesis Advisor:

D. J. Collins

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Automated Pole Placement Algorithm  
for Multivariable Optimal Control Synthesis

by

Chow, Wah Keh  
B.A.(Hons), University of Oxford, 1978

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# ABSTRACT

This work addresses the application of numerical optimization technique to the pole-placement problem in multivariable optimal control. An algorithm is developed to select a set of weighting matrix element such that the conventional transient response criteria are satisfied.

General properties of the optimal system in terms of stability, robustness and relative weights between state and control variables were explored by applying the method to the design of two multivariable systems. Results indicated that this method provides good insight to the problem for the designer and is therefore a useful tool in multivariable control synthesis.



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## I. INTRODUCTION

### A. BACKGROUND

For more than two decades, the need to solve control problems in aerospace application has been the primary driving force behind the modern control theory development. Problems in manoeuvring, guidance and tracking of aircrafts and space vehicles have motivated the development of various control design and synthesis methods. One of the methods, the so-called Linear Quadratic Control or LQ-control [Refs. 1,2] has been widely used and is treated extensively in the control literatures. Unlike most classical methods where the design are based on conventional time response criteria, the LQ theory treats the problem of designing controllers as that of minimizing a quadratic cost function of states and control inputs. The design problems become that of selecting suitable weighting matrices in the performance index. Two questions naturally arise from this method. First, how does one select the weighting matrices and second, once a set weighting matrices is selected, how does one know that it is a good design. There are generally two approaches to the first problem; the obvious one is to rely on physical arguments and a certain amount of trial and error [Refs. 3,4] Unfortunately, such formulation can be obtained in only a few cases. Reference 4 provides a few guidelines that can be employed. The second approach is to avoid the physical aspect of the performance index but instead try to relate the weighting matrices with some other performance specification. For example, Tyler and Tuteur [Ref. 5] expressed the characteristic polynomial as an explicit function of the weighting matrices for single input

single output (SISO) system with diagonal weighting elements. Root-Locus type of procedure were used to show how the variation in weighting elements affect the eigenvalues of the closed-loop system. Similar relations were explored in [Refs. 6,7] in which more general expressions were obtained. Their uses were restricted to single input case due to difficulty in handling polynomial matrices. Solheim [Ref. 8] later developed a sequential design procedure based on diagonalized (decoupled) system. More recent results of eigenvalue placement in optimal control problem are presented in [Refs. 9,10,11,12].

The second issue of LQ design, i.e., whether a good design has been obtained once the performance index has been fixed, is related to the multivariable nature of system. Unlike the single input case where the closed-loop eigenvalues uniquely define the feedback gain and hence the weighting matrices, the MIMO structure provides additional dimension which allows further tradeoff for properties other than the closed-loop eigenvalue location. An example is the gain and phase margin, or in MIMO case, the so-called robustness criteria. Robust-control has been the subject of extensive researches in recent years and results relating to optimal control can be found in [Refs. 13,14,15].

It becomes evident from the above discussion that LQ control design and synthesis are not just a matter of specifying performance index. Optimal in the sense of satisfying performance index and perhaps pole location does not necessary means that a good design has been obtained. Other criteria like disturbance rejection, robustness and sensitivity need to be considered and incorporated in the design procedure. This is the motivation behind our present research which in turn leads to the development of the synthesis package. An overview of the thesis is described in the next section.



## B. OVERVIEW

In this section an overview of the thesis is given. A background of multivariable optimal control theory in terms of its structure, frequency domain characteristic and asymptotic properties is first discussed together with derivation of some useful relationships in Chapter 2. General robustness concepts and its application in Linear Quadratic (LQ) Control is presented in Chapter 3. In Chapter 4, a computer aided design package for pole-placement synthesis based on numerical optimization technique is presented. This package provides a useful computational tool to support the material in the remaining chapter. A step-by-step pole-placement synthesis procedure is also presented to illustrate how the package can be used to design optimal control system that meet time response criteria and other properties. The use of the pole-placement synthesis package in two actual design problems is demonstrated in Chapter 5. Results in terms of frequency and time response properties, robustness (singular value decomposition) are compared to those obtained by other design methods. Program listings and an example of a design session are included in the Appendix.

## II. MULTIVARIABLE LINEAR QUADRATIC CONTROL

In this Chapter a brief review of Multivariable Linear Quadratic Control theory is presented. Structure of LQ system is first given, general stability properties are then discussed. In section two the general pole assignment problem is formulated for the MIMO state feedback system. Interpretation of the state and control input weighting matrices and their effect on the closed-loop time response behaviors and the asymptotic properties are presented.

### A. LINEAR QUADRATIC SYSTEM

Consider the following linear time-invariant state-space system given by the equations:

$$\dot{x}(t) = Ax(t) + Bu(t) \quad (\text{eqn 2.1})$$

$$y(t) = Cx(t) \quad (\text{eqn 2.2})$$

where  $x(t)$  is the  $n$ -dimensional state vector,  $u(t)$  is the  $m$ -dimensional control vector and  $y(t)$  is the  $p$ -dimensional output vector.  $A$ ,  $B$  and  $C$  are real constant matrices of dimension  $n \times n$ ,  $n \times m$  and  $p \times n$  respectively. Assuming that they form a controllable pair  $(A,B)$  and an observable pair  $(A,C)$ , the optimal feedback control law is obtained by minimizing the following quadratic performance index.

$$J = \int_0^{\infty} (x^T Q x + \rho u^T R u) dt \quad (\text{eqn 2.3})$$

where  $R$  is positive definite ( $R > 0$ ) for bounded input and  $\rho$  is a scalar.  $Q$  is a semi-positive definite matrix ( $Q \geq 0$ ).

When both  $Q$  and  $R$  are diagonal matrices,  $\rho$  defines the relative weight between the state and control weighting matrices in the performance index. The quadratic form  $x^T Q x$  and  $u^T R u$  provide a weighted measure of the magnitude of the states and control vector respectively. The steady state control law that minimizes  $J$  is given by,

$$u(t) = -F x(t) \quad (\text{eqn 2.4})$$

where  $F$  is the feedback gain matrix which is given by

$$F = -R^{-1} B^T P \quad (\text{eqn 2.5})$$

The positive definite matrix  $P$  is given by the solution to the steady state Riccati equation.

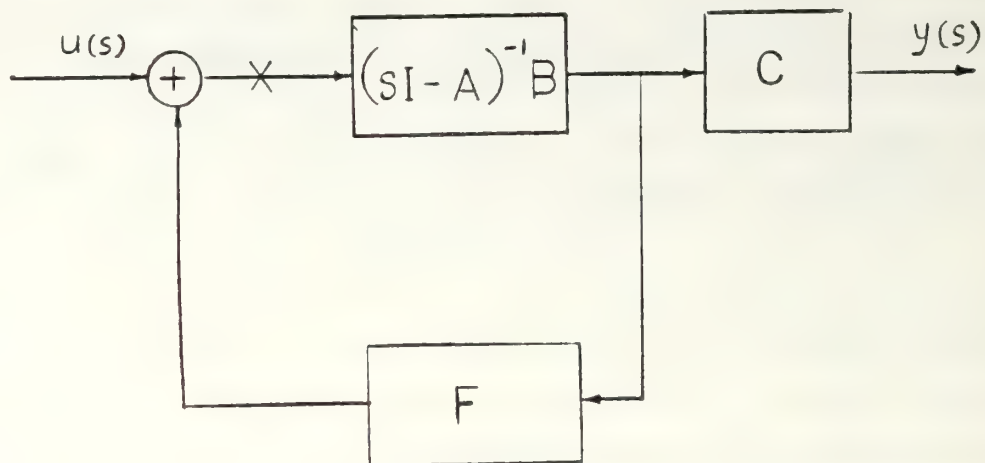
$$P A + A^T P + Q - P B R^{-1} B^T P = 0 \quad (\text{eqn 2.6})$$

Equation 2.5 and 2.6 are well-known results in optimal control theory that yield the optimal closed-loop system

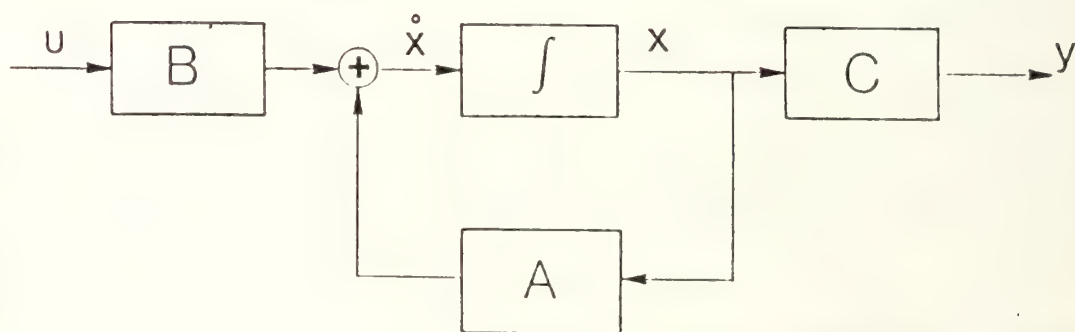
$$\dot{x}(t) = [A + B F] x(t) \quad (\text{eqn 2.7})$$

whose closed-loop poles are given by the eigenvalues of the matrix  $[A + B F]$ . The LQ system given by equations 2.1 through 2.6 is closed-loop stable and can be represented by the feedback configuration in both the time and frequency domain as shown in Figure 2.1 .





Frequency Domain



Time Domain

Figure 2.1 State Feedback System-Time and Frequency Domain.

In Figure 2.1, if the loop is broken at the input (X) as shown, the loop transfer function is given by

$$G(s) = F(sI - A)^{-1}B \quad (\text{eqn 2.8})$$

The matrix  $[I + G(s)]$  is called the Return Difference Matrix and will be shown to have some important feedback properties in the following section.

## B. POLE ASSIGNMENT PROBLEM

In the most general form, the state feedback pole assignment problem in control system design can be formulated precisely as follows:

"Given real matrices (A,B) of order (nxn, nxm) respectively and a set of n complex numbers  $(\lambda_1, \lambda_2, \dots, \lambda_n)$  closed under complex conjugation. Find a real mxn matrix F such that the eigenvalues of  $[A+BF]$  are  $\lambda_i$ ,  $i = 1, 2, 3 \dots n$ ."

In general, the closed-loop eigenvalues of (A+BF) can be arbitrary located in the complex plane, with the only restriction that complex characteristic eigenvalues must occur in complex conjugate pair. In other words, if the matrices (A,B) are a completely controllable pair, the stability of the system can always be improved by state feedback. If the (A,B) pair is not completely controllable, then the system is required to be 'stabilizeable' meaning that in its controllability canonical form given by equation 2.9 below, the matrix  $A_{22}$  is asymptotically stable or any unstable subspace of equation 2.9 is also in the controllable subspace.

$$\begin{bmatrix} \dot{x}_1(t) \\ \dot{x}_2(t) \end{bmatrix} = \begin{bmatrix} A_{11} & A_{12} \\ 0 & A_{22} \end{bmatrix} \begin{bmatrix} x_1(t) \\ x_2(t) \end{bmatrix} + \begin{bmatrix} B \\ 0 \end{bmatrix} \begin{bmatrix} u_1(t) \\ u_2(t) \end{bmatrix}$$

(eqn 2.9)

The solution to the pole assignment problem in the single input ( $m=1$ ) case, when it exists, can be shown to be unique. In the multiple input case ( $1 < m < n$ ), the solution of the so-called inverse eigenvalue problem is, in general, undetermined with many degrees of freedom. Additional conditions must be supplied in order to eliminate the extra degrees of freedom. This has been an area of active research in recent years and a number of approaches have been developed to relate the extra degrees of freedom with properties such as system eigenvectors, transmission zeros and robustness [Refs. 16,17]. In this work, it is shown that Linear Quadratic formulation incorporating equation 2.3 will partly remove the uncertainty that exists in the multiple inputs case. It will be shown that useful properties like robustness are guaranteed. It is also shown that the LQ type of pole placement formulation, when combined with eigenvectors assignment type of formulation, will produce some very useful design and synthesis procedures. In the present work, however, only the LQ eigenvalue placement problem is addressed; the problem of combined eigenvalue and eigenvector assignment is briefly described in Chapter 5.



### C. WEIGHTING MATRICES AND SYSTEM PERFORMANCES

This section briefly reviews the effect of weighting matrices on system performance. The physical aspects of the weighting matrix for both single and multiple input systems are presented first together with some discussion on the asymptotic behavior of the LQ system.

It was shown in the last section that under complete controllable conditions, the time-invariant linear system can be stabilized by a linear feedback control law. For the regulator-type problem where the aim is to bring the system from an arbitrary initial state to the zero state, the closed loop poles can be chosen far to the left on the complex plane. Convergence to the zero state is fast but the large input required may not be practical. This naturally leads to an optimization problem where the trade off is between speed of convergence to zero and the magnitude of the input. This is reflected in the two quadratic terms in the performance index. The quantity  $x^T Q x$  in the first term of the performance index is a measure of the extent in which the state at time  $t$  deviates from the zero state. The matrix  $Q$  determines how much weight is attached to each of the component of the state. The integral  $\int (x^T Q x) dt$  is a criteria for the cumulative deviation of  $x(t)$  from the zero state during the interval.

The problem of large control input is resolved by incorporating the second quadratic term,  $\int (u^T R u) dt$ . Larger value in the element of the control weighting matrix  $R$  will result in smaller input. It will be shown later that one can manipulate  $R$  to achieve some secondary design objectives. The remaining parameter  $\rho$ , that need to be specified, accounts for the relative weighting between the state and the control inputs. Selecting optimal value for  $\rho$  depends on the particular problem and the design requirement. As  $\rho$

decreases, the integrated square regulating error decreases but the integrated square input increases. Very often, the optimal control problem is solved for many different values of  $\rho$ . A graph similar to that shown in figure 2.2 is obtained where the integrated square regulating error is plotted versus the integrated square input. An appropriate value of  $\rho$  is then selected to give sufficiently small regulator error without excessively large input.

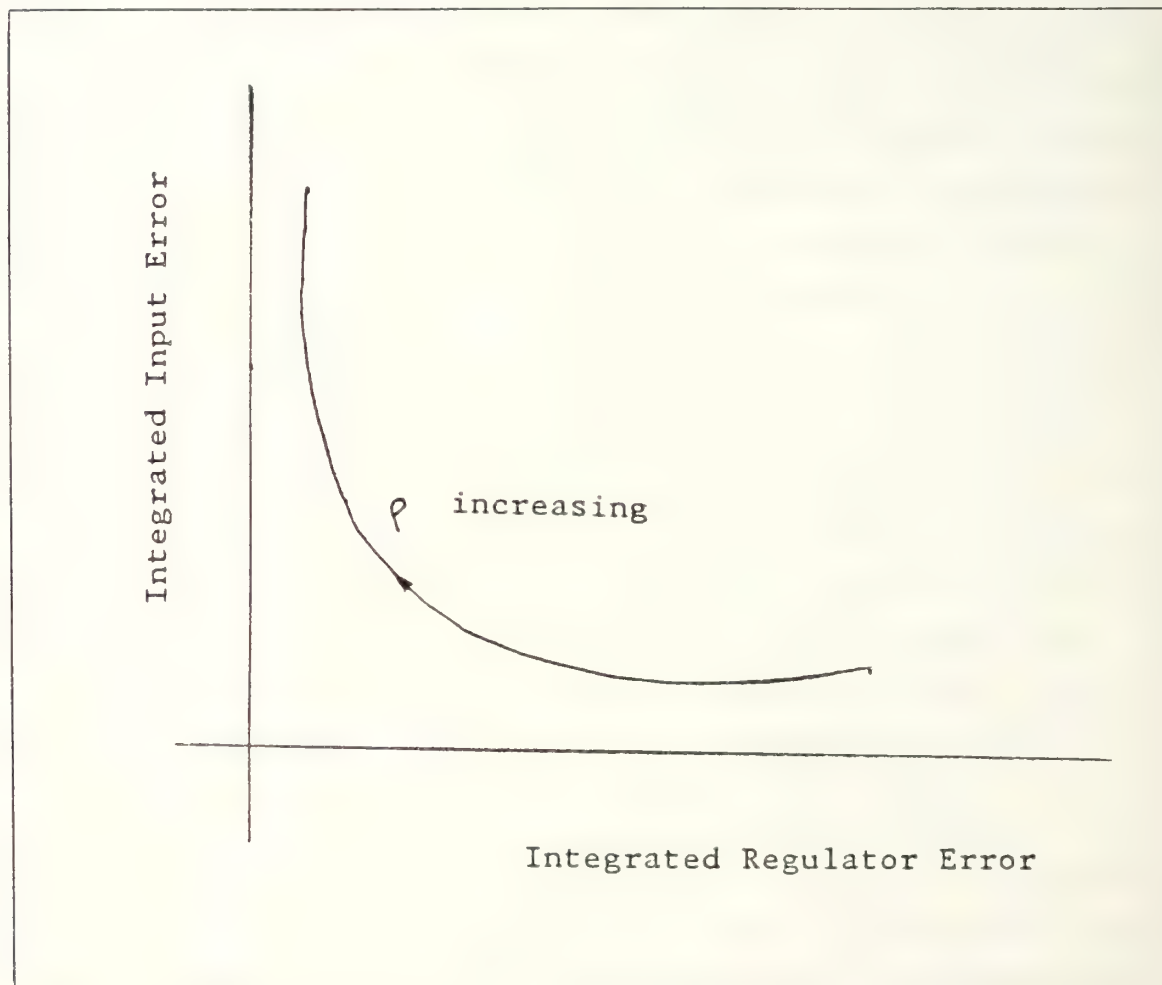


Figure 2.2 Selecting Relative Weighting Parameter  $\rho$ .

The special case where  $\rho$  approaches zero ,the so-called asymptotic properties, has been shown to provide good insight for LQ control system design. Some of the results from [Refs. 4,18] are summarized below.

As  $\rho$  decreases to zero for the system given by equations 2.1 through 2.6, some ( say  $q$  ) of the closed-loop poles go to infinity while other (  $n-q$  ) stay finite. Those remaining finite approach the left half plane zero of  $\det[B^T(-sI-A^T)^{-1}Q(sI-A)^{-1}B]$ . If  $m$  is the dimension of the input vector, then at least  $m$  closed-loop poles approaches infinity. All closed-loop poles that go to infinity do so by grouping into several Butterworth patterns of different order and radii. For  $\rho$  approaching infinity, the closed-loop poles approach the mirror image of the plant open-loop poles. To illustrate the asymptotic concept, two examples from [Ref. 4] are given below.

An example of the asymptotic properties of a single input system is shown in Figure 2.3 . The closed-loop poles of a position control system using LQ type feedback are plotted as a function of  $\rho$  . The system has two open-loop poles at -4.6 and 0.0 . As  $\rho$  decreases, the closed-loop poles go to infinity along two straight lines that make an angle of  $\pi/4$  with the negative real axis. As  $\rho$  approaches infinity, both closed-loop poles first meet on the negative real axis and then approach the open-loop poles at (-4.6, 0).

Figure 2.4 shows the asymptotic loci of the closed-loop poles for a multiple input system where  $n=4$  and  $m=2$ . There are four open-loop poles at  $(-0.006123, \pm j0.09353)$  and  $(-1.250, \pm j1.394)$  and both the state and control weighting matrices are taken to be of a diagonal form. As  $\rho$  approaches to zero, one closed-loop pole stay finite at -1.002. The remaining three go to infinity, two of which assume a second order Butterworth pattern and the last one



approaches on the negative real axis. When  $\rho$  approaches infinity, all closed-loop poles approach the open-loop poles.

Many researchers have explored this asymptotic properties. Stein [Refs. 9,10] developed a procedure to select the control weighting matrices for a desired closed-loop asymptotic eigenstructure. It will be shown in the subsequent Chapters that the asymptotic properties provide useful guideline for the design procedures to be described.

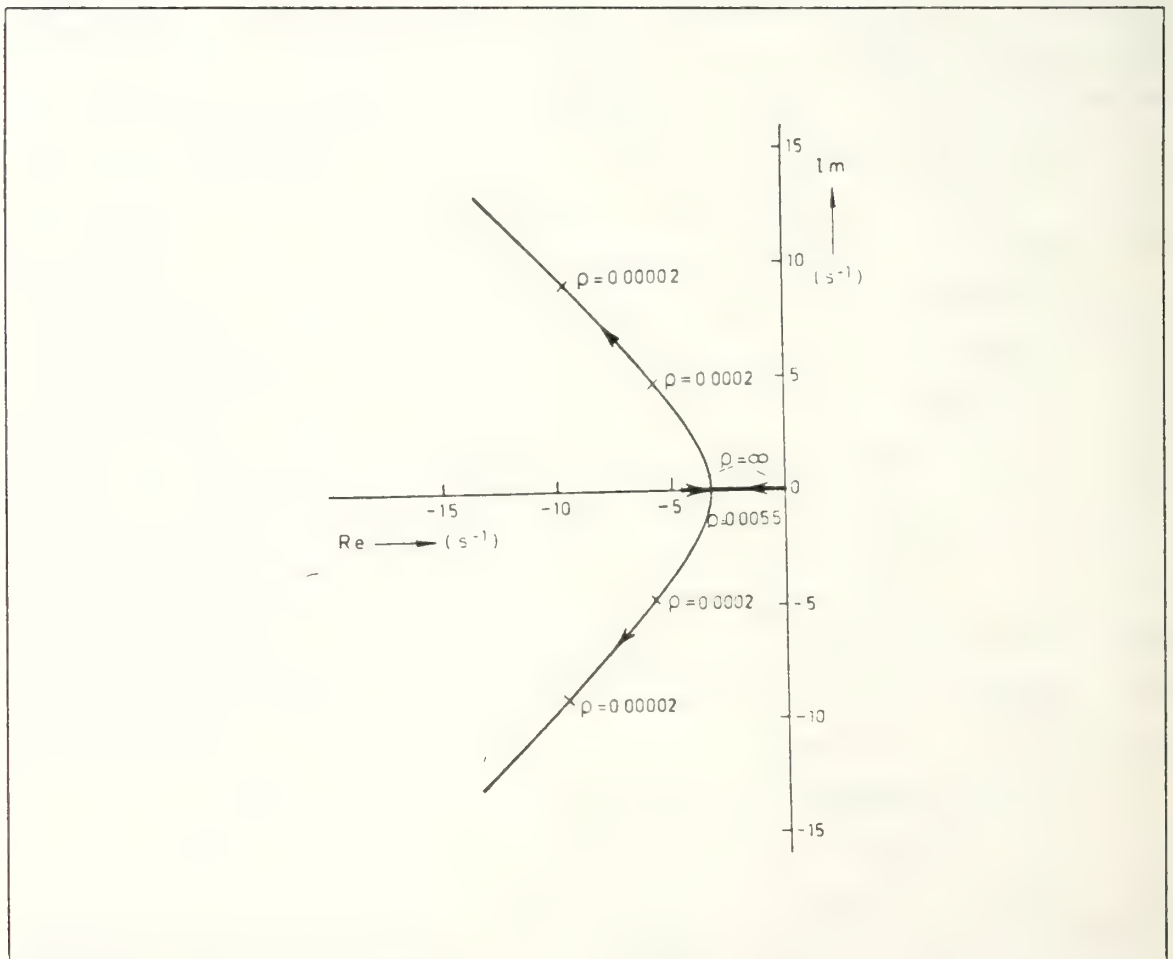
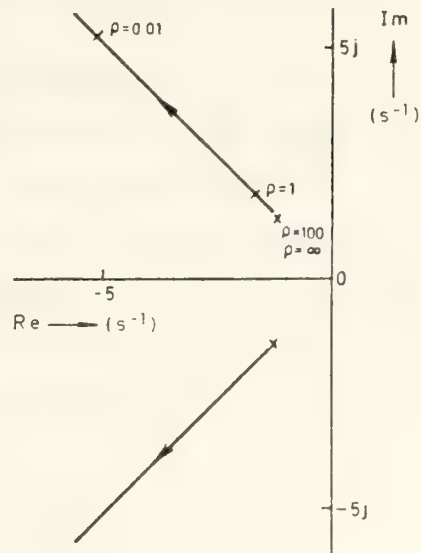
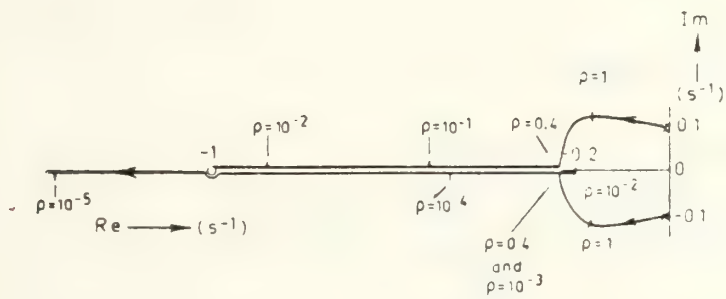


Figure 2.3 Single Input Asymptotic Root Loci.



Faraway Poles



Nearby Poles

Figure 2.4 Multiple Input Asymptotic Root Loci.

### III. ROBUSTNESS THEORY AND LINEAR QUADRATIC CONTROL

In the last Chapter, the effect of weighting matrices on the closed-loop pole of the LQ system was discussed. This Chapter addresses yet another important feedback property that control system designers are concerned with: Robustness. Robustness theory was developed when it was realized that the classical single loop Nyquist test was not adequate to guarantee stability when the multivariable open loop plant deviates from its model due to a variety of reasons [Ref. 15]. In the following section, the concept of robust design for both SISO and MIMO general feedback system is reviewed. The singular value analysis is discussed in term of multiplicative type of disturbances. Finally, robustness for linear quadratic state feedback are presented in terms of the effect of weighting matrices on the singular value curve.

#### A. ROBUSTNESS CONCEPTS

The concept of robustness for SISO system can best be described in terms of the definition of phase and gain margin. A system characterized by good gain and phase margin implies that changes in the plant model parameters and changes in the loop gain and/or phase may be accommodated without loss of stability. The gain and phase margins of a SISO system are defined with reference to the perturbed system in Figure 3.1

Assuming that the unperturbed system ( $l(j\omega)=1$ ) is stable, the positive (or negative) phase margin is the value of  $\phi$  greater (or less) than zero at which the perturbed system with  $l(j\omega) = k \cdot \exp(j\phi)$  becomes unstable. The upward



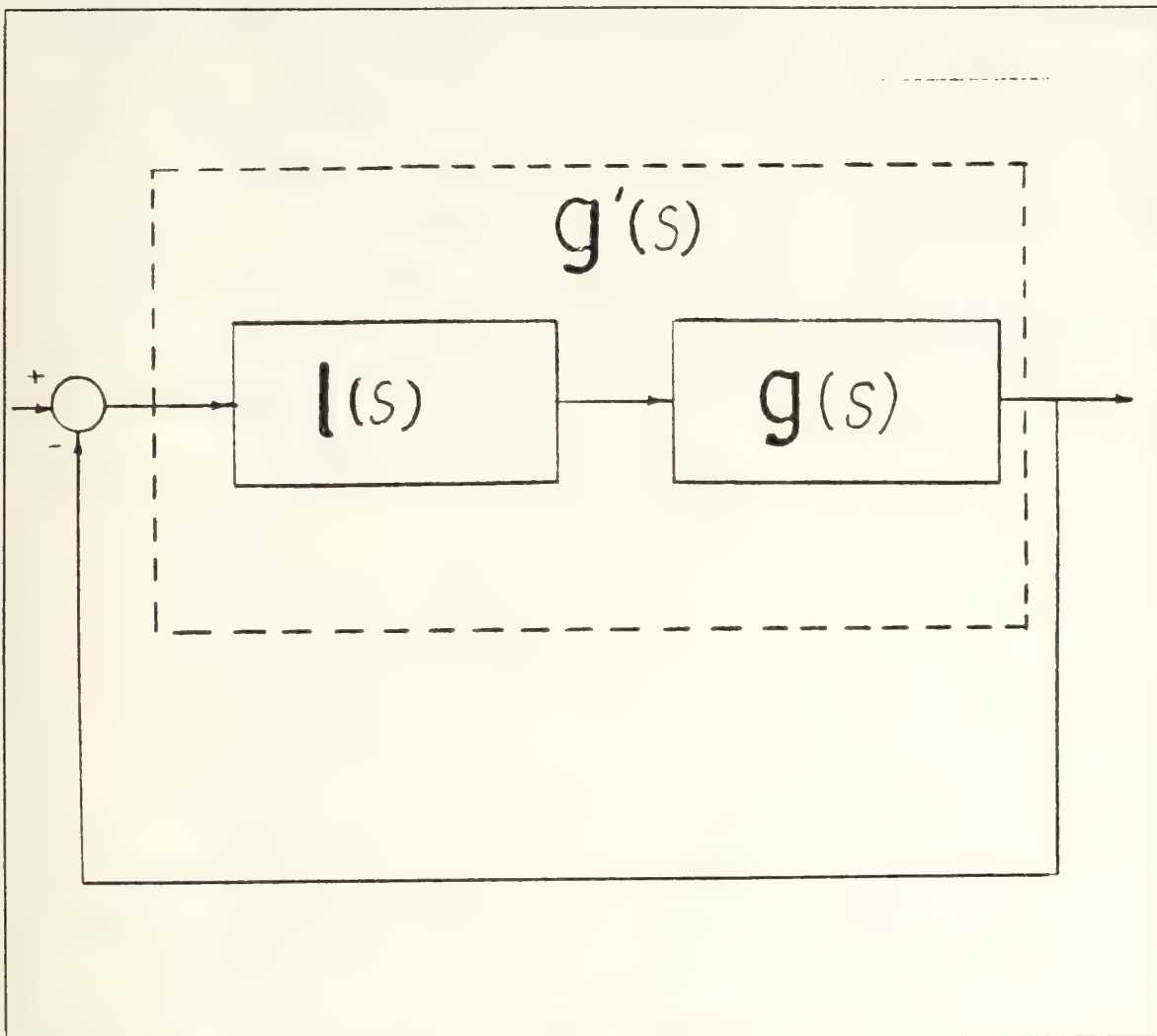


Figure 3.1 The Perturbed SISO System.

(or downward) gain margin is the smallest (or greatest) value of  $1(j\omega)=k=\text{constant}$ , for which the system become unstable. With reference to the classical Nyquist plot in Figure 3.2 , gain and phase margin are defined as,

$$\begin{aligned} \text{GM}^{\uparrow} (\text{upward}) &= 1/k_1 & \text{GM}^{\downarrow} (\text{downward}) &= 1/k_2 \\ \text{PM}^+ &= \alpha_1 & \text{PM}^- &= \alpha_2 \end{aligned}$$

A set of minimum guaranteed GM and PM may be obtained by defining  $\alpha_o = \min[1 + g(j\omega)]$  as shown in Figure 3.3 where,

$$GM = 1/(1 \pm \alpha_o)$$

and

$$PM = \pm \cos^{-1}(1 - \alpha_o^2/2)$$

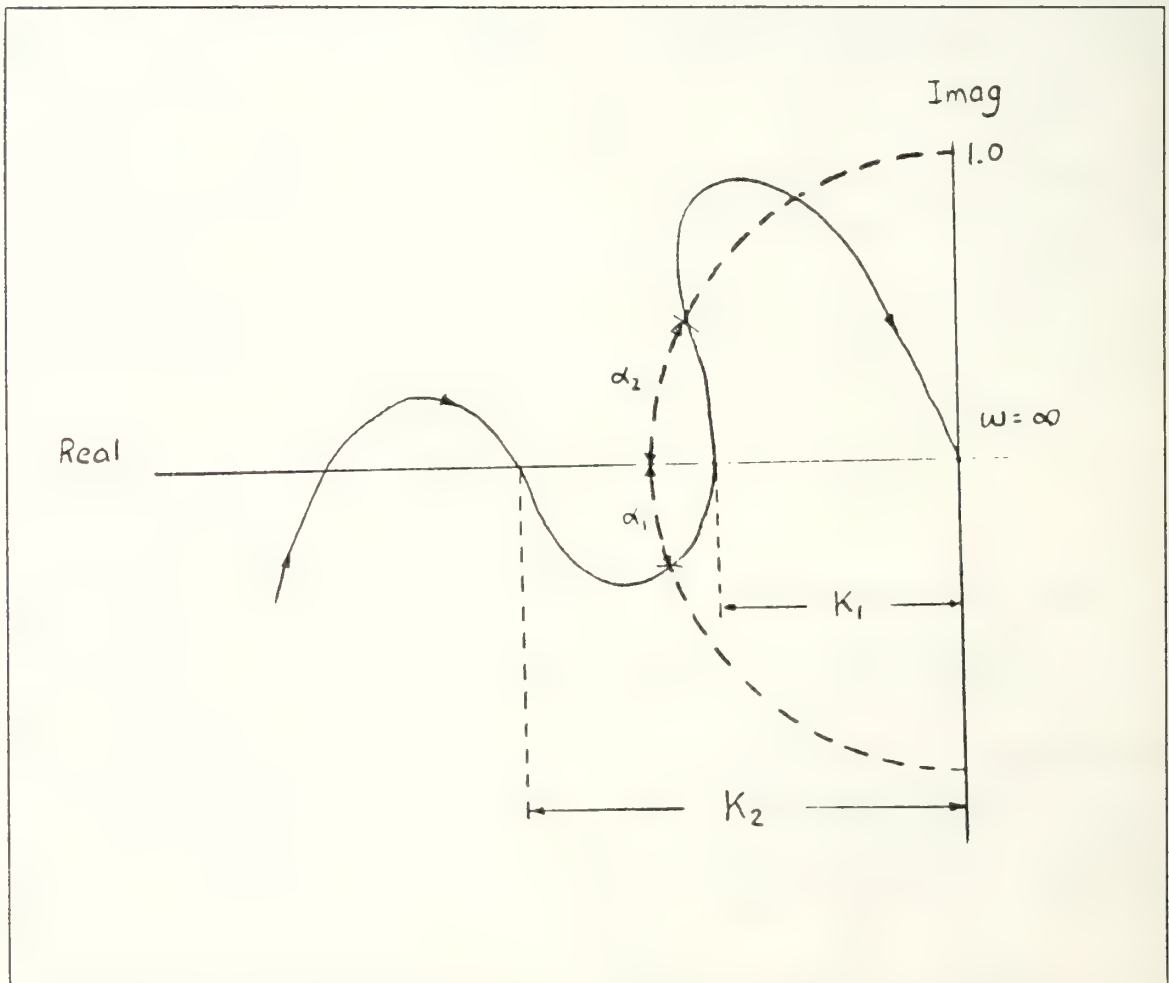


Figure 3.2 The Nyquist Plot - Gain and Phase Margin.

Note that in the above definition of GM and PM, either  $\phi_i$  'or'  $\kappa_i$  is allowed to change in the loop. The allowed changes are therefore very restrictive. A more useful definition of the gain and phase margin for MIMO system that accounts for simultaneous changes in both  $\phi_i$  and/or  $\kappa_i$  (the so-called universal gain and phase margin) has been derived in [Ref. 19]. From Figure 3.3 it can be seen that  $\alpha_0$  may provide a rather conservative estimate of the actual gain and phase margin.

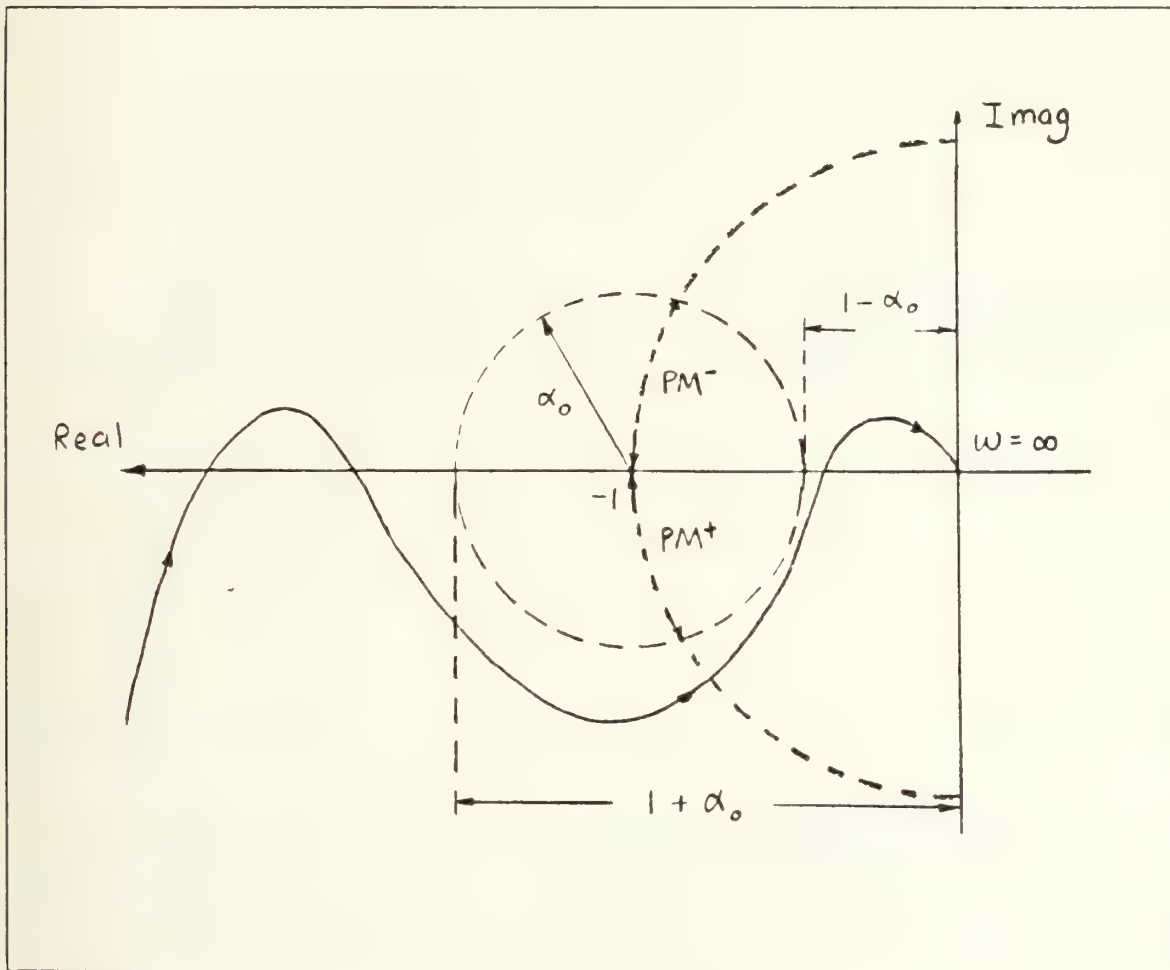


Figure 3.3 The Minimum Guaranteed GM and PM.



In MIMO system, gain and phase margin characterize the ability of the system to tolerate gain and/or phase changes within all loops simultaneously. Figure 3.4 shows a perturbed MIMO system with the assumption that  $L(j\omega) = \text{Dia}(l_1(j\omega), l_2(j\omega) \dots)$ . As in the SISO case, the system will remain stable as long as  $l_i(j\omega)$  satisfy  $GM^- < k_i < GM^+$  (assuming that  $\phi_i$ 's are zero). For the case when the magnitude of  $l(j\omega)$  are constant, the system will remain stable for all  $\phi_i$ 's that satisfy  $PM^- < \phi_i < PM^+$ .

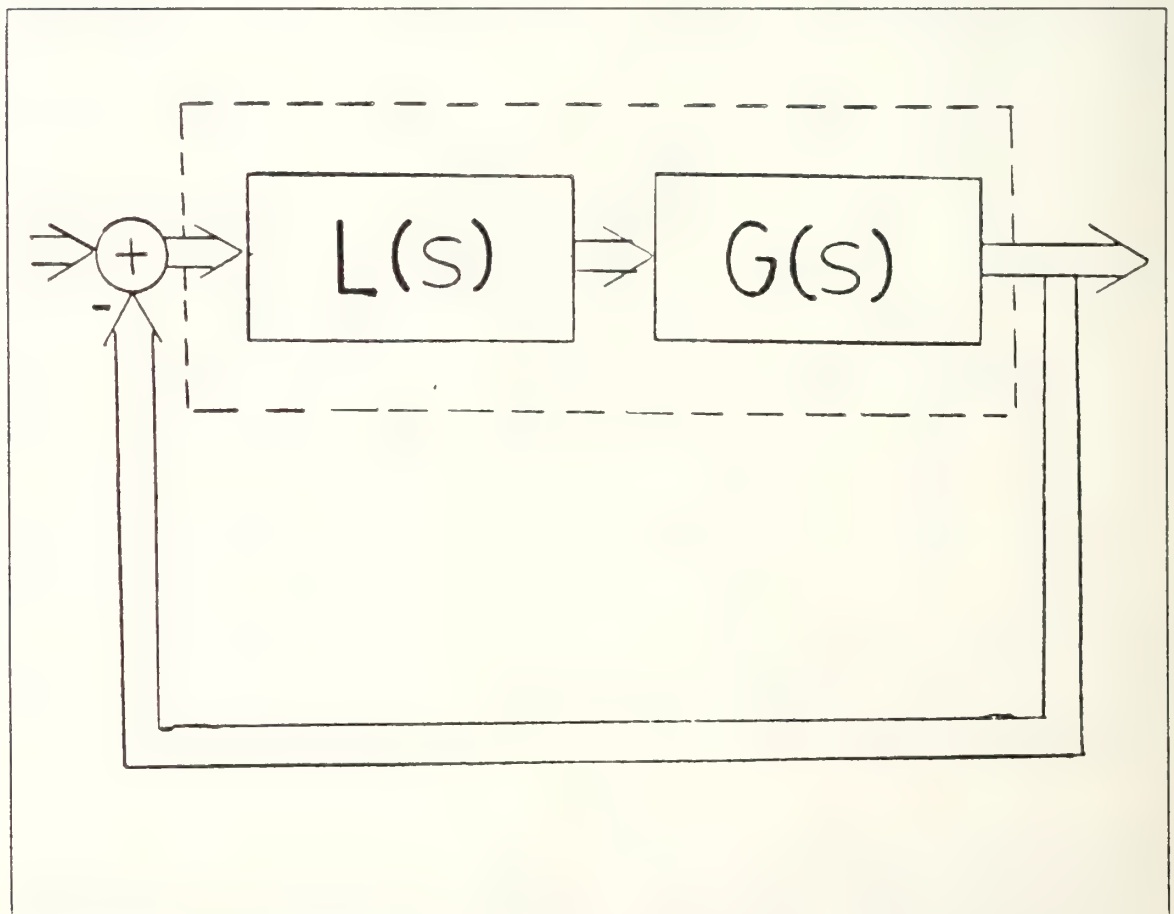


Figure 3.4 The Perturbed MIMO System.

The set of minimum guaranteed multivariable gain and phase margins are determined by the minimum singular value ( $\underline{\sigma}$ ) of the return difference matrix  $[I + G(s)]$ , where  $G(s)$  is the open loop transfer matrix and consists of the plant and its controller. Note the similarity between the SISO and MIMO cases,

$\alpha_o$  : nearness of  $(1 + g(s))$  to the origin.

$\underline{\sigma}$  : nearness of matrix  $[I + G(s)]$  to singularity.

Two important results that are related to multivariable phase and gain margin developed in [Ref. 15] are next presented as a theorem.

THEOREM: The multiplicative perturbed system (Figure 3.4) is stable if either of the following conditions hold:

$$1. \quad \underline{\sigma} [I + G(s)] > \bar{\sigma} [L^{-1}(s) - I] \quad (\text{eqn 3.1})$$

$$2. \quad \underline{\sigma} [I + G^{-1}(s)] > \bar{\sigma} [L(s) - I] \quad (\text{eqn 3.2})$$

where  $\bar{\sigma}$ ,  $\underline{\sigma}$  denote the maximum and minimum singular values of  $[I+G(s)]$  respectively.

It will be shown that condition 1 can be related to the optimality condition of LQ system and hence provides a useful relationship between the weighting matrices and robustness.

## B. ROBUSTNESS IN LQ SYSTEM

Robustness properties pertaining to LQ system are closely related to the frequency domain optimality condition. For the SISO case, Kalman [Ref. 1] showed that the return difference transfer function satisfies the inequality

$$(1 + g(j\omega)) \geq 1 \quad (\alpha_o = 1) \quad (\text{eqn 3.3})$$

Inspection of the Nyquist diagram in Figure 3.5 clearly indicates that a SISO LQ state feedback has a guaranteed infinite upward gain margin, 0.5 downward gain margin and a minimum phase margin of  $\pm 60$  deg.

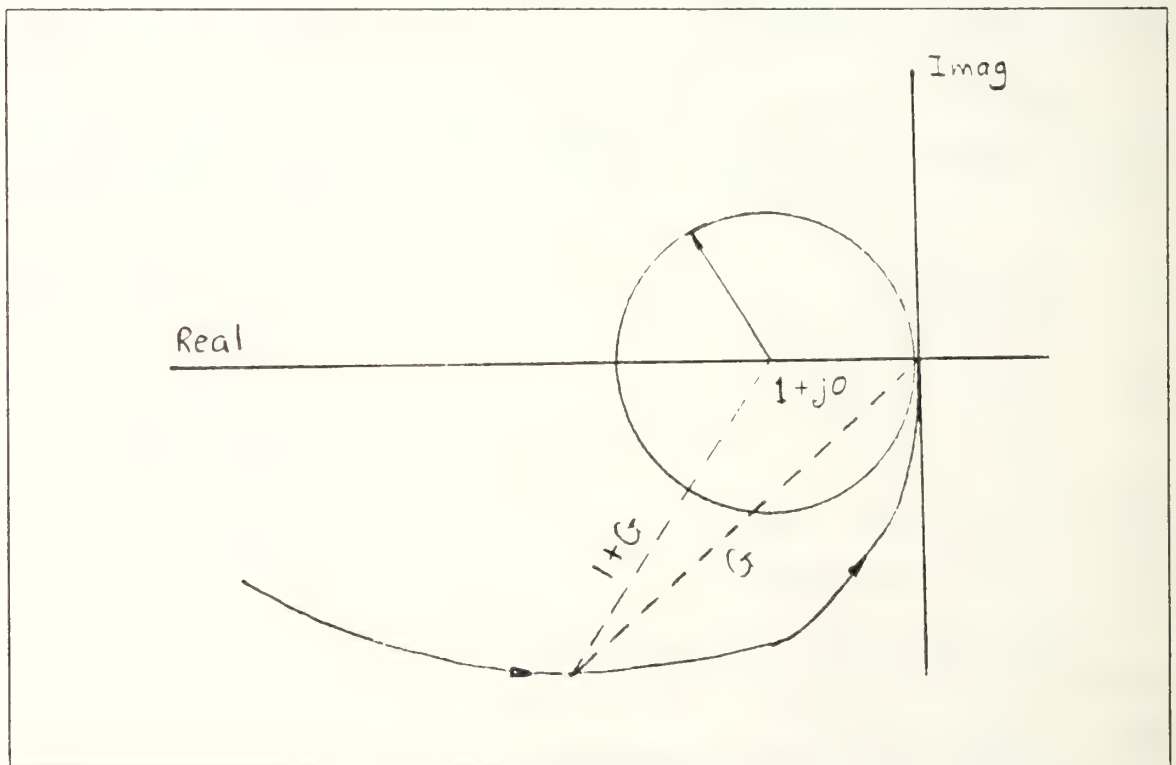


Figure 3.5 SISO LQ Nyquist.

In a similar manner, multivariable stability margin can be derived from the multivariable version of condition 1 in equation 3.1 ;

$$[I + G(s)]^H R [I + G(s)] > R \quad (\text{eqn 3.4})$$

where

$$G(s) = R^{-1} B^T P [sI - A]^{-1} B$$

and  $P \geq 0$  satisfies the steady state Riccati equation.

It can be shown that condition 1 in equation 3.1 above can be written as

$$\underline{\sigma} [I + R^{1/2} G(j\omega) R^{-1/2}] \geq 1 \quad (\text{eqn 3.5})$$

which can be reduced to

$$\underline{\sigma} [I + G(j\omega)] > 1 \quad (\text{eqn 3.6})$$

where  $R$  is diagonal ( i.e.  $R = \rho I$  for some positive scalar  $\rho$  ). Like the SISO case, the multivariable LQ regulator with loop transfer matrix  $G(s)$  that satisfies equation 3.5 and 3.6 has, in all the feedback loops, a guaranteed minimum gain and phase margin given by,

$$GM = 1/2, \text{ and } PM = \pm 60 \text{ deg}$$

The case when  $R$  is not diagonal is interesting as condition 3.6 no longer apply and additional trade-off can be obtained by including off diagonal terms in the control input weighting matrix. This is especially useful when the nature and structure of the disturbances are known. Design involving the off diagonal  $R$  matrix will be shown in Appendix A.



## IV. DESIGN PROCEDURE

### A. GENERAL

The background material described in Chapter 2 and 3 are the basis for developing a computer aided design package and the corresponding design procedure. The design philosophy presented in this Chapter is most useful when a designer is able to characterize the desired system in terms of closed-loop eigenvalues and time response. Some initial physical insight of the weighting matrices, their asymptotic properties and the nature of the perturbation will be useful in the design process. This Chapter begins with a discussion of the various approaches to the LQ pole placement problem. The selected approach and the corresponding computer aided design package is presented. The design philosophy and design procedure for both the reduced order and full order model are then given.

### B. APPROACHES

All the pole placement algorithms for LQ system that have been developed so far require an expression that relate the characteristic equation of the optimal system with the elements of the weighting matrices. Two such formulations for the stabilizeable and detectable time-invariant linear system (equation 2.1) and the quadratic criteria (equation 2.3) are given by

$$\phi_c(s)\phi_c(-s) = \phi(s)\phi(-s)\det[I + R^{-1}H^T(-s)QH(s)] \quad (\text{eqn 4.1})$$

and

$$\phi_c(s)\phi_c(-s) = \phi(s)\phi(-s)\det[I + 1/\rho R^{-\frac{1}{2}} H^T(-s)QH(s)R^{-\frac{1}{2}}] \quad (\text{eqn 4.2})$$

where  $\phi_c(s) = \det[sI - A + BF]$  and  $\phi(s) = \det[sI - A]$  are the closed-loop and open-loop characteristic polynomials respectively.  $H(s) = C(sI - A)^{-1}B$  is the open loop transfer matrix of the system.

Both formulations have been used in root-locus type of procedure to investigate how the closed-loop poles move as weighting matrices changes [Refs. 5,6]. For MIMO case, there has been little success due to problems involving polynomial matrices. In this work, a different approach is adopted. Equation 4.1 or 4.2 is formulated as a numerical optimization problem in which the objective function is made equal to the determinant part of equation 4.1 or 4.2

$$\text{Obj} = \det[I + R^{-1}H^T(s)QH(s)] \quad (\text{eqn 4.3})$$

or

$$\text{Obj} = \det[I + 1/\rho R^{-\frac{1}{2}} H^T(-s)QH(s)R^{-\frac{1}{2}}] \quad (\text{eqn 4.4})$$

For a given desired closed loop pole  $s = s_d$ , equation 4.3 or 4.4 becomes

$$\phi_c(s_d)\phi_c(-s_d) = 0 \quad (\text{eqn 4.5})$$

Providing that  $\phi(s_d)\phi(-s_d)$  is not equal to zero, the objective function must equal to zero if the particular Q, R set is to correspond to the desired closed-loop poles. Convergence to zero for a given set of Q and R is therefor automatically guaranteed.

The pole placement problem can therefore be solved as an unconstrained multivariable optimization in which the elements of Q and R are varied to make the objective

function in equation 4.3 and 4.4 approach zero. This was done during the early phase of the work. It was later discovered that more insight to the problem can be obtained by first transforming the problem to an appropriate coordinate system and then to perform pole placement one at a time. This is of advantage as a system designer is often satisfied with several open-loop poles in a large system. Reassigning poles in the the reduced-order model will reduce computer time and memory requirement.

The optimization routine selected for this work is the so-called SUMT method (Sequential Unconstrained Minimization Techniques) obtained from the ADS package in [Refs. 20,21]. In this method, the objective function (eg. equation 4.3 or 4.4 ) and any constraint equation are formulated into an augmented objective function in which the problem is solved as an unconstraint optimization task.

## C. POLE PLACEMENT ALGORITHMS

For ease of implementation and better insight, only the problem of determining the state weighting matrix  $Q$  (given  $R$ ) that gives a set of closed-loop eigenvalues is considered. It must be emphasised that the algorithm can also be formulated to determine  $R$  (for a given  $Q$ ) or to vary  $Q$  and  $R$  at the same time. In most cases, the present formulation is adequate as designers usually have some knowledge about the control weighting matrix. System matrix that has real and distinct eigenvalues is presented first, follows by cases where  $A$  has complex eigenvalues and repeated eigenvalues.

### 1. System with Real and Distinct Eigenvalues

The original system given by equation 2.1 and 2.2 is first transformed into a diagonal form using the transformation given by;

$$\mathbf{x}(t) = \mathbf{M}\mathbf{z}(t)$$

(eqn 4.6)

where  $\mathbf{M}$  is an eigenvector matrix corresponding to the system matrix  $\mathbf{A}$ . and  $\mathbf{z}(t)$  is the new state vector. The transformed system in the new coordinate is given by,

$$\dot{\mathbf{z}}(t) = \mathbf{\Lambda} \mathbf{z}(t) + \mathbf{M}^{-1}\mathbf{B}\mathbf{u}(t)$$

(eqn 4.7)

where  $\mathbf{\Lambda}$  is a diagonal matrix  $\text{dia}[\lambda_1, \lambda_2, \lambda_3, \dots]$

The performance index (equation 2.3), when expressed in terms of the new state vector  $\mathbf{z}(t)$  becomes,

$$\begin{aligned} J &= \int_0^{\infty} (\mathbf{x}^T \mathbf{Q} \mathbf{x} + \mathbf{u}^T \mathbf{R} \mathbf{u}) dt \\ &= \int_0^{\infty} (\mathbf{z}^T \mathbf{M}^T \mathbf{Q} \mathbf{M} \mathbf{z} + \mathbf{u}^T \mathbf{R} \mathbf{u}) dt \\ &= \int_0^{\infty} (\mathbf{z}^T \hat{\mathbf{Q}} \mathbf{z} + \mathbf{u}^T \mathbf{R} \mathbf{u}) dt \end{aligned}$$

(eqn 4.8)

where  $\hat{\mathbf{Q}} = \mathbf{M}^T \mathbf{Q} \mathbf{M}$ .

It can be shown that to move an open-loop pole to its new location given by  $s_i = s_d$ , only  $\hat{Q}_i$  is required and other  $\hat{Q}_s$  have no effect on the pole assignment. As an example, to move the open-loop pole at  $s = \lambda_2$  for  $\mathbf{\Lambda} = \text{dia}[\lambda_1, \lambda_2, \lambda_3, \dots]$  to its new location  $s = \bar{\lambda}_2$ , only  $\hat{\mathbf{Q}} = \text{dia}[0, \hat{q}_2, 0, \dots]$  is required.

$\hat{\mathbf{Q}}$  can then be selected according to equation 4.3 or 4.4 using the optimization routine. As currently implemented in the program, there is no constraint equation formulation. Once the value of  $\hat{\mathbf{Q}}$  that satisfies the desired pole location is obtained, the system is transformed back to the original coordinate system via,

$$\mathbf{Q} = \mathbf{M}^{-T} \hat{\mathbf{Q}} \mathbf{M}^{-1}$$

(eqn 4.9)



With  $Q$  known, and  $R$  given, the optimal feedback gain  $F$  can be obtained by solving the steady state Riccati equation as given in equation 2.5 and 2.6 . Since the pole placement is done in the decoupled coordinate system, only the eigenvalues that correspond to  $Q_i$  is reassigned; all other eigenvalues remain unchange. It can be also shown that the eigenvector corresponding to an eigenvalue is also unchange, this property will be shown to be useful in the reduced order formulation of the linear quadratic problem.

If desired, the problem here can also be formulated to move more than one eigenvalues in one run. This can be done by modifying the objective function to include more terms as follows;

$$Obj = \sum_{i=1}^n \det[I + R^{-1} H^T (-s) Q H(s) R^{-1}] \quad (eqn 4.10)$$

where  $n$  is the number of poles to be reassigned.

The augmented matrix  $A_{aug} = [A + BF]$  is then computed. If desired, the procedure may be repeated to move other open loop eigenvalue to its specified position using the new  $A_{aug}$  as the starting plant matrix. This will in turn result in another set of  $Q$  and  $F$  . The effective  $Q_e$  and  $F_e$  after  $n$  reassignments are given by

$$Q_e = Q_1 + Q_2 + \dots Q_n \quad (eqn 4.11)$$

and

$$F_e = F_1 + F_2 + \dots F_n \quad (eqn 4.12)$$

The above pole assignment procedure can also be applied to an optimal system where an initial starting  $Q$  and  $R$  are given. A good example is when the control system designer has some knowledge of the weighting matrix but would also like to meet a specific time response requirement.

## 2. System with Complex Eigenvalues

If the same similarity transformation mentioned in the last section is used, the transformation matrix will be complex. To be able to work with real matrix, an auxiliary transformation of the form given by equation 4.13 is used;

$$x(t) = Tz(t) \quad (\text{eqn 4.13})$$

$T = ML$  and  $M$  is the eigenvector matrix (equation 4.6) The matrix  $L$  is given by,

$$L = \begin{bmatrix} 0.5 & -0.5j & 0.0 & \dots & 0.0 \\ 0.5 & 0.5j & 0.0 & \dots & . \\ 0.0 & 0.0 & 1.0 & \dots & . \\ . & \dots & \dots & 1.0 & . \\ 0.0 & \dots & \dots & \dots & 1.0 \end{bmatrix} \quad (\text{eqn 4.14})$$

The transformed system is then given by,

$$\dot{z}(t) = A Z(t) + T^{-1}Bu(t) \quad (\text{eqn 4.15})$$

with performance index ,

$$J = \int (z^T T^T Q Tz + u^T R u ) dt \quad (\text{eqn 4.16})$$

where  $\hat{Q}$  is now given by  $\hat{Q} = T^T Q T$ .

It can be shown that to move a pair of complex eigenvalues given by  $s = a + bj$ , a weighting matrix of the form

$$\hat{Q} = \begin{bmatrix} 0 & 0 & 0 & \dots & 0 \\ 0 & \hat{q}_i & 0 & & . \\ 0 & 0 & \hat{q}_{i+1} & & . \\ 0 & . & . & & . \\ 0 & . & . & \dots & 0 \end{bmatrix}$$

(eqn 4.17)

with  $\hat{q}_i = \hat{q}_{i+1}$  is required.

In a similar manner,  $\hat{Q}$  can be obtained by using the optimization routine, with the condition  $\hat{q}_i = \hat{q}_{i+1}$  formulated as a constrained equation. Inverse transformation and determination of  $Q_e$  and  $F_e$  are identical to the distinct eigenvalue case with  $M$  in equation 4.9 replaced by  $T$ .

### 3. System With Repeated Eigenvalues

In this case, the system matrix cannot be diagonalized but the general procedure given above still apply. The system is first transformed into the Jordan canonical form ;

$$J = U^{-1} A U \quad (\text{eqn 4.18})$$

where  $U$  is a transformation matrix which is not the eigenvector matrix  $M$ . An example of the Jordan form is given below,

$$J = \begin{bmatrix} \lambda & 1 & 0 \\ 0 & \lambda & 1 \\ 0 & 0 & \lambda \end{bmatrix}$$

(eqn 4.19)

The only difference with the two procedures mentioned above is that the pole reassignment has to begin at the bottom of each Jordan block. For example, in the system given above (equation 4.19), the first re-assignment will result in a new system given by equation 4.20

$$J = \begin{bmatrix} \lambda & 1 & 0 \\ 0 & \lambda & 1 \\ 0 & 0 & s_d \end{bmatrix}$$

(eqn 4.20)

Determination of Q and F using the optimization and the inverse transformation routines are identical to the distinct eigenvalues case with M in equation 4.9 replaced by U.

#### D. COMPUTER PROGRAM DESCRIPTION

The computer aided design package developed in this thesis is illustrated in Figure 4.1. The program is developed using the top-down approach with special purpose subroutines called by the main control program. The driver program supports three independent modes with the data entry portion common to all modes:

1. Data Entry : The system matrices A, B, C and/or F, Q, R etc are entered through a data file. Design variables such as desired poles locations, elements of matrices to be varied etc, are also specified through the input data file.
2. Pole Placement Mode : In this mode, an arbitrary set of closed-loop eigenvalues is assigned by selecting the appropriate state weighting matrix. As shown in Figure 4.1, the transformation matrices for various



cases are computed first. The pole placement is achieved using the numerical optimization routine described in the last section;  $Q$  is obtained and then inverse-transformed to the original co-ordinate system. If desired, the results can be used as an input to the Linear Quadratic Control Program.

3. Linear Quadratic Control Mode : This part of the program is adopted from the OPTSYS program. Given a set of weighting matrices  $Q$  and  $R$  and the system matrices  $A$ ,  $B$  and  $C$ , it computes the steady state feedback gain  $F$ , closed-loop eigenvalues, etc.
4. Singular Value Analysis Mode : This portion of the program allows the designer to analyze various designs obtained from the two modes mentioned above in term of singular value vs frequency plot. The main part of this program is adopted from [Ref. 22].

The three modes of operation mentioned above may be used in any order to implement specific design objectives. A typical design process will involve runs alternating between the three modes until a compromise between primary and secondary design objectives is achieved. Record of a typical design run together with a complete listing of the main program and their non-standard subroutine are given in Appendix B and C.

## E. DESIGN PHILOSOPHY

The Linear Quadratic constant state feedback design philosophy for the linear time-invariant model is illustrated in Figure 4.2. It assumes that the location of the eigenvalues and system time response are the main design objectives. These objectives can be achieved using the pole placement procedure developed in this thesis. Single or multiple reassignment can be made in one run. A number of

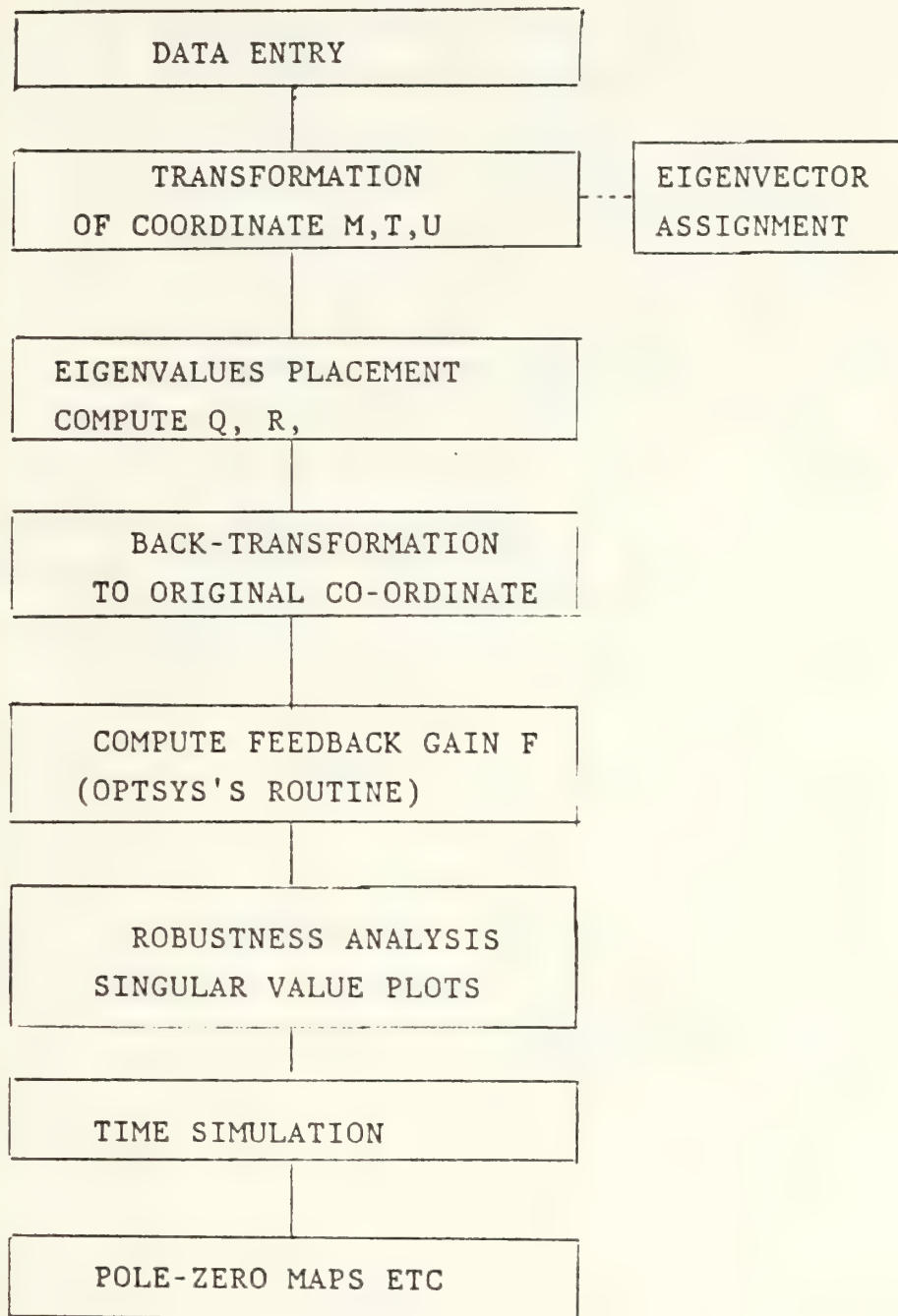


Figure 4.1 Computer Aided Design Package Organization.

designs can then be obtained using different starting control weighting matrices, different state weighting matrices and different assignment sequences. Physical constraints such as control input amplitude, control input energy as well as general system properties such as asymptotic behavior are heavily relied upon during this process. After the major objectives are satisfactorily achieved, secondary design objectives are considered. These include feedback gain reduction (by increasing the control weighting matrix), robustness (in terms of minimization of system sensitivity to modelling errors and/or parameter variations), zeros locations, eigenvectors assignments. The extra degrees of freedom available in the MIMO state feedback system can often provide a means to improve these secondary objectives while only slightly modifying the closed-loop pole assignment and thus the time response.

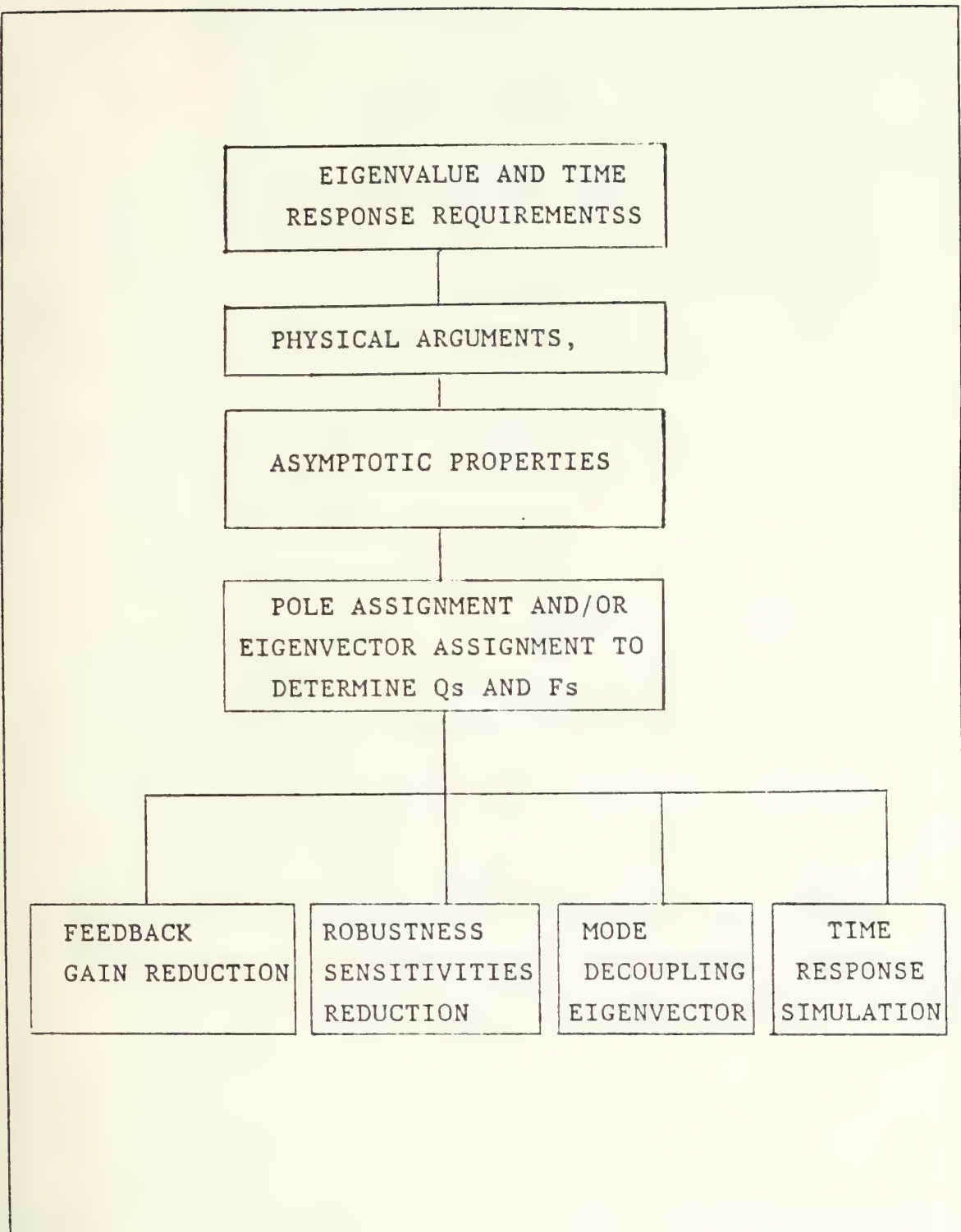


Figure 4.2 LQ Eigenvalue Assignment Philosophy.



## V. DESIGN EXAMPLES

The design procedure described in Chapter 4 is illustrated in this Chapter by two design problems. A typical LQ structure and its properties, together with the pole placement procedure is first presented with a 2x2 model. A practical design problem is then presented for the highly coupled lateral channels of a CH-47 Helicopter. The resulting LQ designs are compared with other multivariable state feedback designs [Refs. 22,23]. It is shown that the procedure developed here is a viable tool for robust constant feedback controller design.

### A. INTRODUCTORY 2X2 PROBLEM

This problem formulated in reference 23 serves to demonstrate how a highly cross-coupled multivariable control problem can be formulated and solved as a linear quadratic design problem, using the pole placement procedure. The problem provides excellent insight into the structure of the multivariable LQ system and its built-in robustness to cross-coupled perturbation.

Figure 5.1 shows a diagram of this basic 2X2 system in which the plant is given by

$$\dot{x}(t) = Ax(t) + Bu(t) \quad (\text{eqn 5.1})$$

$$y(t) = Cx(t) \quad (\text{eqn 5.2})$$

where

$$A = \begin{bmatrix} -1 & 0 \\ 0 & -1 \end{bmatrix}$$

$$B = \begin{bmatrix} 1 & 50 \\ 0 & 1 \end{bmatrix}$$

$$C = \begin{bmatrix} 1 & 0 \\ 0 & 1 \end{bmatrix}$$

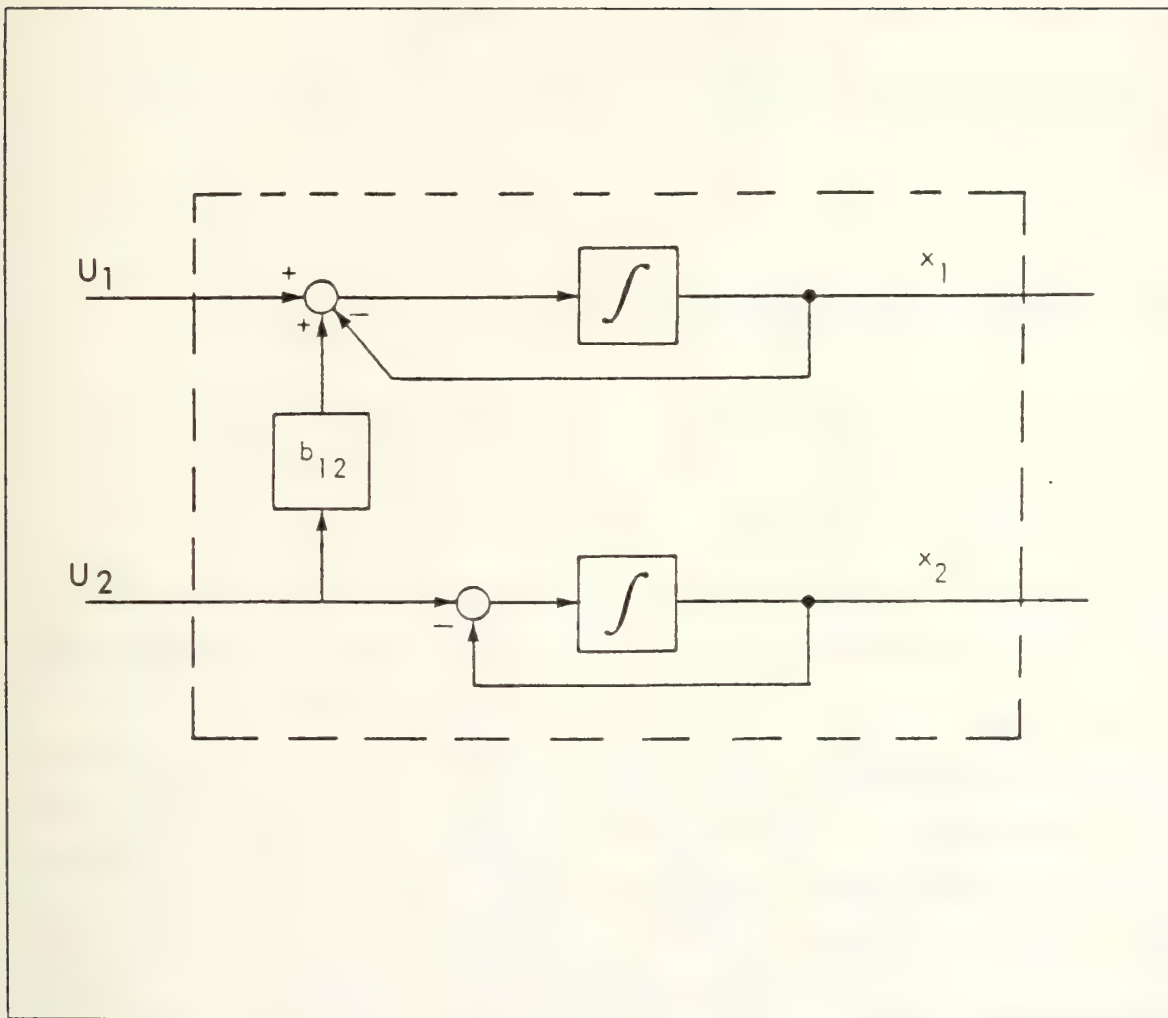


Figure 5.1 A Simple 2X2 MIMO Model.

This system has open-loop eigenvalue at -1, -1 and is therefore stable. The  $b_{12}$  term in the control matrix B is purposely made large to produce the cross-coupled effect from channel two to channel one( see Figure 5.1). The design requirement is to select a set of feedback gain F such that the closed-loop eigenvalues are at -2, -2. Assuming that this is the only requirement, it is not difficult to see that a unity feedback law of the form (Figure 5.2),

$$\begin{bmatrix} u_1 \\ u_2 \end{bmatrix} = \begin{bmatrix} -1 & 0 \\ 0 & -1 \end{bmatrix} \begin{bmatrix} x_1 \\ x_2 \end{bmatrix} + \begin{bmatrix} u_{c1} \\ u_{c2} \end{bmatrix}$$

(eqn 5.3)

will produce the desired closed-loop system given by,

$$\begin{bmatrix} \dot{x}_1 \\ \dot{x}_2 \end{bmatrix} = \begin{bmatrix} -2 & 50 \\ 0 & -2 \end{bmatrix} \begin{bmatrix} x_1 \\ x_2 \end{bmatrix} + \begin{bmatrix} 1 & 50 \\ 0 & 1 \end{bmatrix} \begin{bmatrix} u_{c1} \\ u_{c2} \end{bmatrix}$$

(eqn 5.4)

The above design seems to be acceptable as far as eigenvalues or time response is concerned. It is now shown that when robustness of the system is considered, the unity feedback gain controller performs rather poorly. On the other hand, design using LQ Pole Placement type of formulation will result in robust controllers. To demonstrate the lack of robustness of the unity feedback design, the feedback gain matrix F as given in equation 5.4 is perturbed slightly (by +5%) and the eigenvalues of the resulting closed-loop

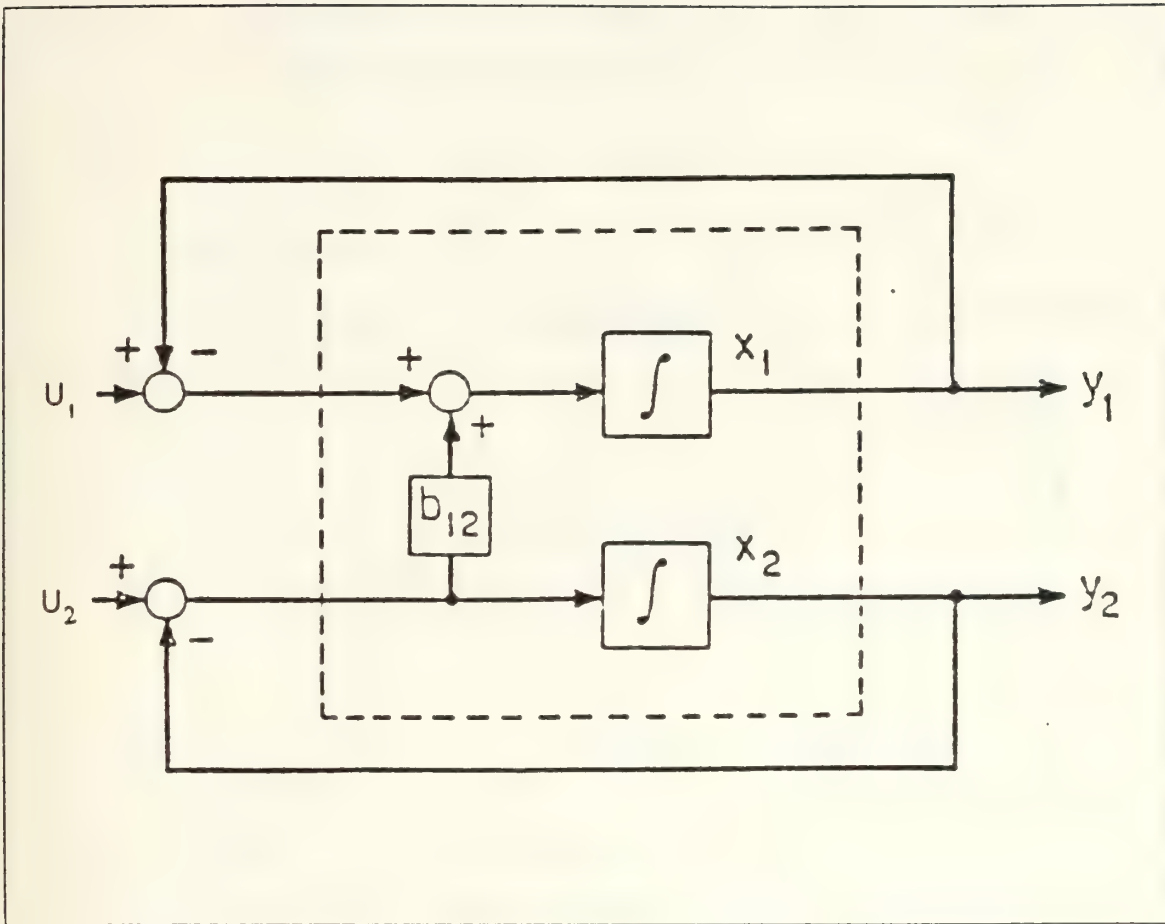


Figure 5.2 Unity Feedback for the 2X2 Model.

system matrix are calculated. The absolute and percentage errors in the eigenvalue due to the perturbation of the closed-loop system are given in Table I .

It can be seen from the above that the first cut design is very susceptible to model and feedback perturbation. A 5 % changes in the  $f_{21}$  term has resulted in a large shift ( 160% ) in the closed-loop eigenvalue. Lack of robustness in the unity feedback design can also be seen in terms of the minimum singular value plot of the return difference matrix in the frequency domain. For the unity feedback gain system shown in Figure 5.2, the return difference matrix is given by,



TABLE I  
PERTURBED EIGENVALUE FOR 2X2 MODEL

Perturbation in F (+5%)	Absolute Changes in Eigenvalues	Percent Changes in Eigenvalues
$f_{11}$ and $f_{22}$	0.05 , 0.05	2.5 , 2.5
$f_{12}$	0.0 , 0.0	0.0 , 0.0
$f_{21}$	0.67 , +3.265	33.5 , 163.0
All	1,255, 5.346	37.25 , 167.0

$$I + G(s) = \begin{bmatrix} s+2/(s+1) & 50/s+1 \\ 0 & s+2/(s+1) \end{bmatrix}$$

(eqn 5.5)

where  $G(s) = C(sI-A)^{-1}B$  is the loop transfer matrix as indicated in Figure 5.3

The multivariable Nyquist diagram ( locus of  $\det[I+G(s)]$  for the system is shown in Figure 5.4. If this diagram is interpreted as for a single input system, the  $(-1/2, \infty)$  gain margin and  $(\pm 160)$  phase margin would lead one to believe that the design is a good one. This has been shown to be not the case, a 5% perturbation in F would cause the system to become unstable. The above clearly demonstrate the inadequacy of the classical method in evaluating stability margin for MIMO system.

Robustness properties of the unity feedback controller will now be analyzed in terms of singular value as discussed

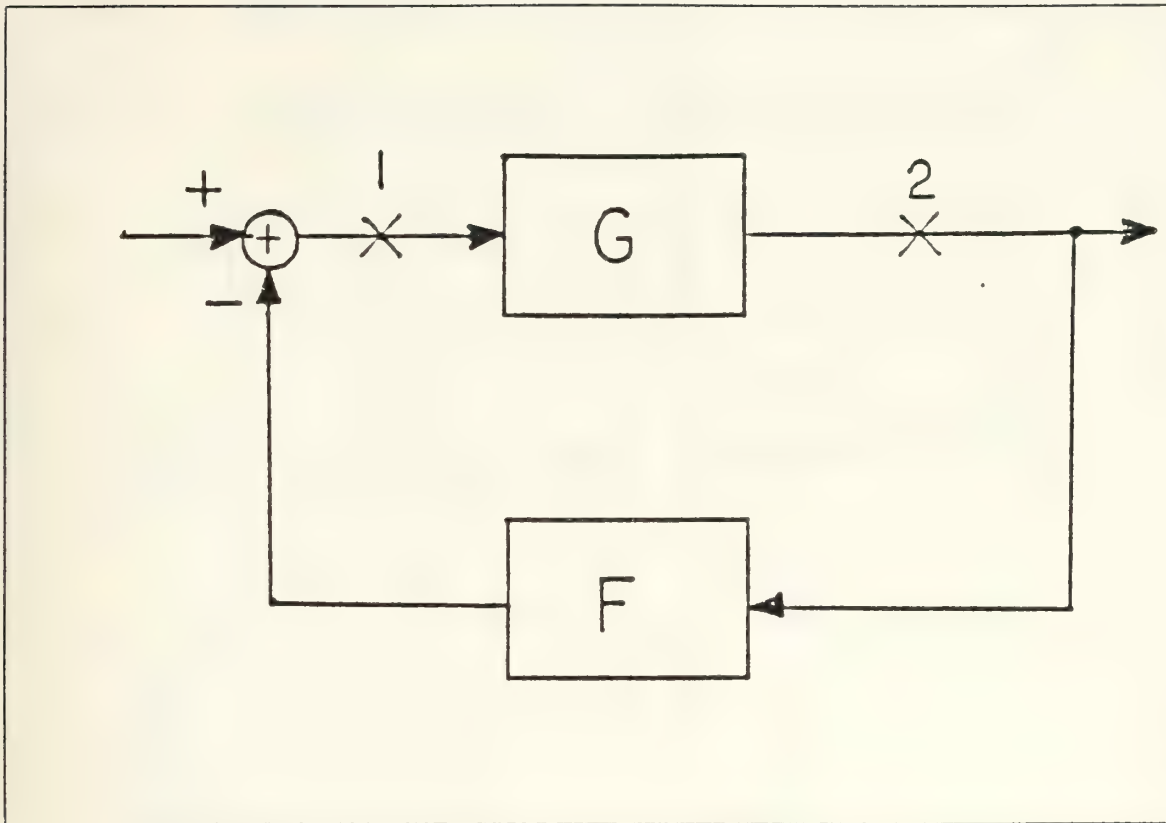


Figure 5.3 Loop Transfer Matrix -  $F = I$ .

in Chapter 3. The minimum singular value plot of  $[I+G(s)]$ , is shown in Figure 5.5 as a function of frequency. The lack of robustness is clearly indicated by the relative small singular value at frequency around 2 rad/s. Using the universal phase and gain margin chart developed in [Ref. 19], the minimum singular value at this frequency corresponds to a gain margin of (0.91, 1.0) and a phase margin of ( $\pm 4$  deg).

It is now shown that formulation using LQ approach and the pole placement procedure developed here will result in robust design that meet the time response requirement. Furthermore, better insight of the design process can be obtained from the procedure to be described here. The first step in the LQ design is to determine the asymptotic

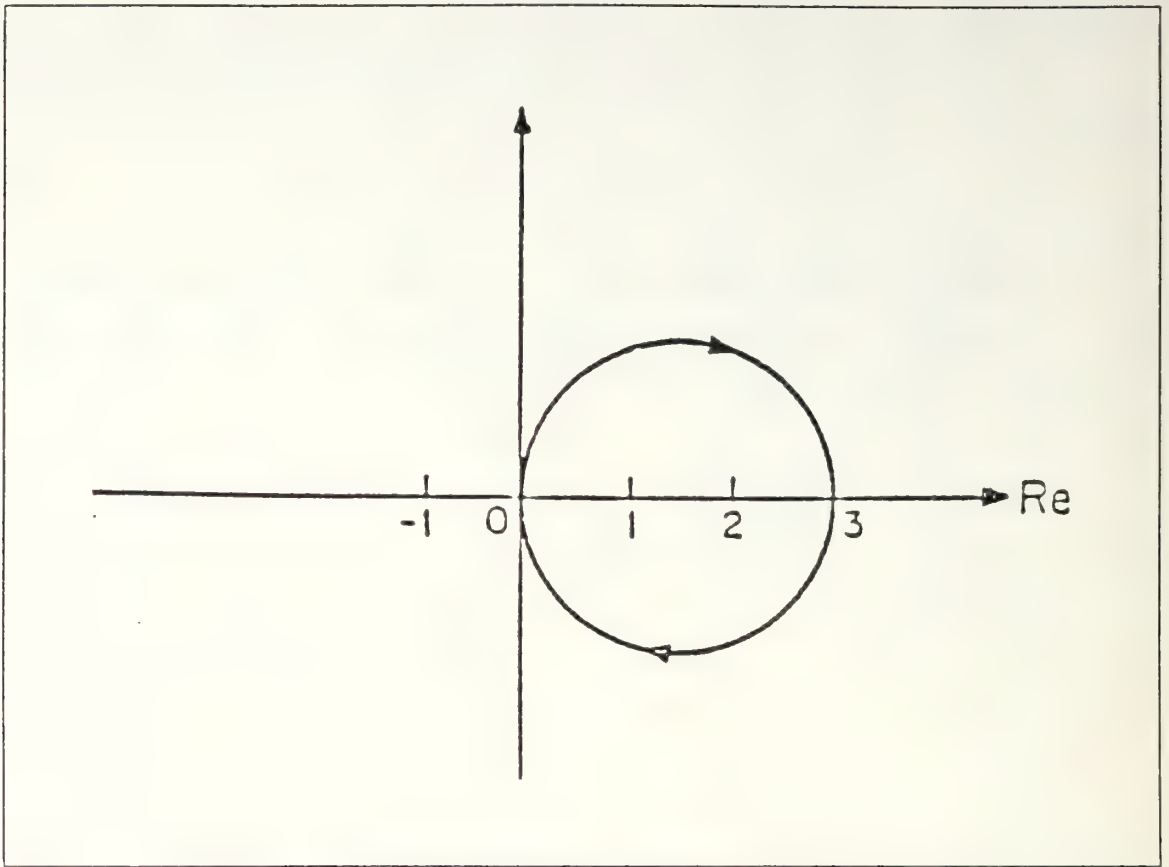


Figure 5.4 Multivariable Nyquist Plot.

properties of the system, i.e. movement of closed-loop poles as  $R \rightarrow 0$ . Using results from Chapter 2, it can be established that as  $R$  increase from 0 to  $\infty$ , both closed-loop poles move from infinity on the real axis to the open-loop poles location. None of the closed-loop poles stay finite as  $R \rightarrow 0$  since the dimension of the input control vector is equal to the dimension of the state. Assuming that  $R = I$ , the pole placement is accomplished in two steps. The first step is to move the open-loop pole at -1 to -2.0. As the system matrix  $A$  given is already in Jordan form, no transformation is required. The pole placement program puts the pole at -1.9987 with,

# SINGULAR VALUE PLOT

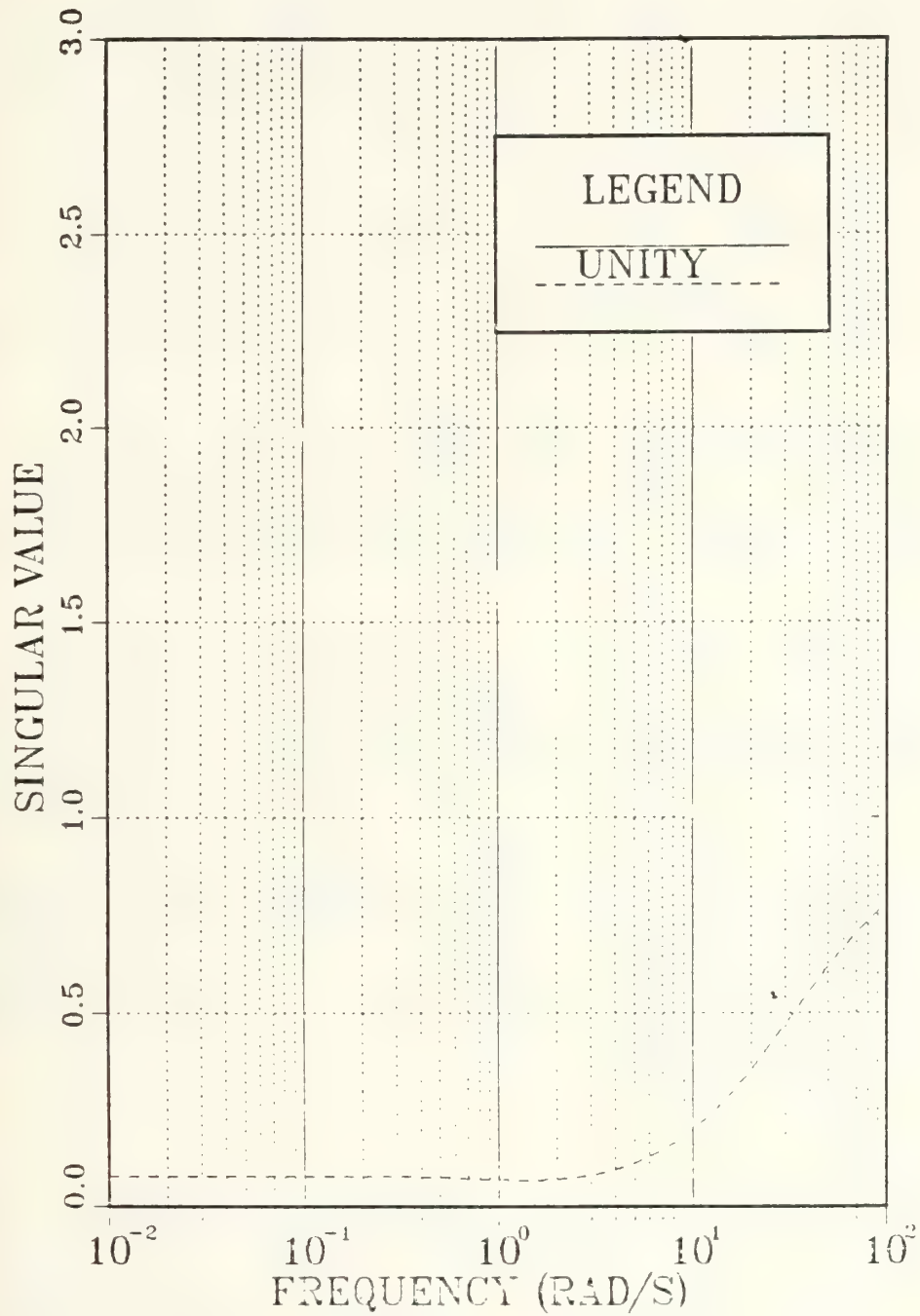


Figure 5.5 Singular Value Plots - Unity Feedback.



$$Q_1 = \begin{bmatrix} 0.00119 & 0 \\ 0 & 0 \end{bmatrix} \quad F_1 = \begin{bmatrix} 0 & 0 \\ 0.01983 & 0 \end{bmatrix}$$

and

$$A_{aug} = \begin{bmatrix} 1.9915 & 0 \\ 0.01983 & 1.0 \end{bmatrix}$$

In the second step, the other open-loop pole at -1. is moved to -2.0 , using  $A_{aug}$  as the new plant matrix. The resulting  $Q$  and  $F$  and the augmented plant matrix become,

$$Q_2 = \begin{bmatrix} -2.998 & -149.9 \\ -149.9 & 7499.3 \end{bmatrix} \quad F_2 = \begin{bmatrix} 0.9994 & -49.978 \\ -0.00841 & 0.4211 \end{bmatrix}$$

The effective  $Q_e$  and  $F_e$  required to move both open-loop poles at -1.0 to -2. are  $Q_e = Q_1 + Q_2$  and  $F_e = F_1 + F_2$  as shown in equation 5.6 below. The pole placement procedure is completed with the final eigenvalues placed at  $(-1.99255, \pm j0.05628)$ .

$$Q_e = \begin{bmatrix} 2.99919 & -149.9 \\ -149.9 & 7499.3 \end{bmatrix} \quad F_e = \begin{bmatrix} 0.9994 & -49.978 \\ 0.0114 & 0.4211 \end{bmatrix}$$

(eqn 5.6)

The singular value plots of the case where  $R = I$  together with the unity feedback gain ( non-LQ design ) are shown in Figure 5.6. The well established fact that LQ design possesses  $(1/2, \infty)$  gain margin and  $(\pm 60\text{deg})$  phase margin can also be readily observed from the same figure as the minimum singular values of  $[I+G]$ ,  $\underline{\sigma}$ , is greater than one for all frequency. Changes in closed-loop eigenvalue for a small perturbation in  $F$  is again computed as shown in Table II. It can be seen that the LQ design is robust with the largest percentage change in eigenvalues location of only 10%, when compared with the 160% change in the unity feedback design.

TABLE II  
PERTURBED EIGENVALUE FOR LQ DESIGN

Perturbation in $F$ (+5%)	Absolute Changes in Eigenvalues	Percent Changes in Eigenvalues
$f_{11}$ and $f_{22}$	0.2149 , 0.142	10.7 , 7.1
$f_{12}$	0.119 , 0.119	5.59 , 5.59
$f_{21}$	0.0592, 0.0578	2.90 , 2.89
All	0.07 , 0.070	3.52 , 3.52

The pole-zero plots of various closed-loop transfer functions of the closed-loop transfer matrix for both the unity feedback and LQ design are compared in Figure 5.7 and 5.8. For the unity feedback design, zero at minus three for the input 2 to output 1 channel corresponds to the

# SINGULAR VALUE PLOT

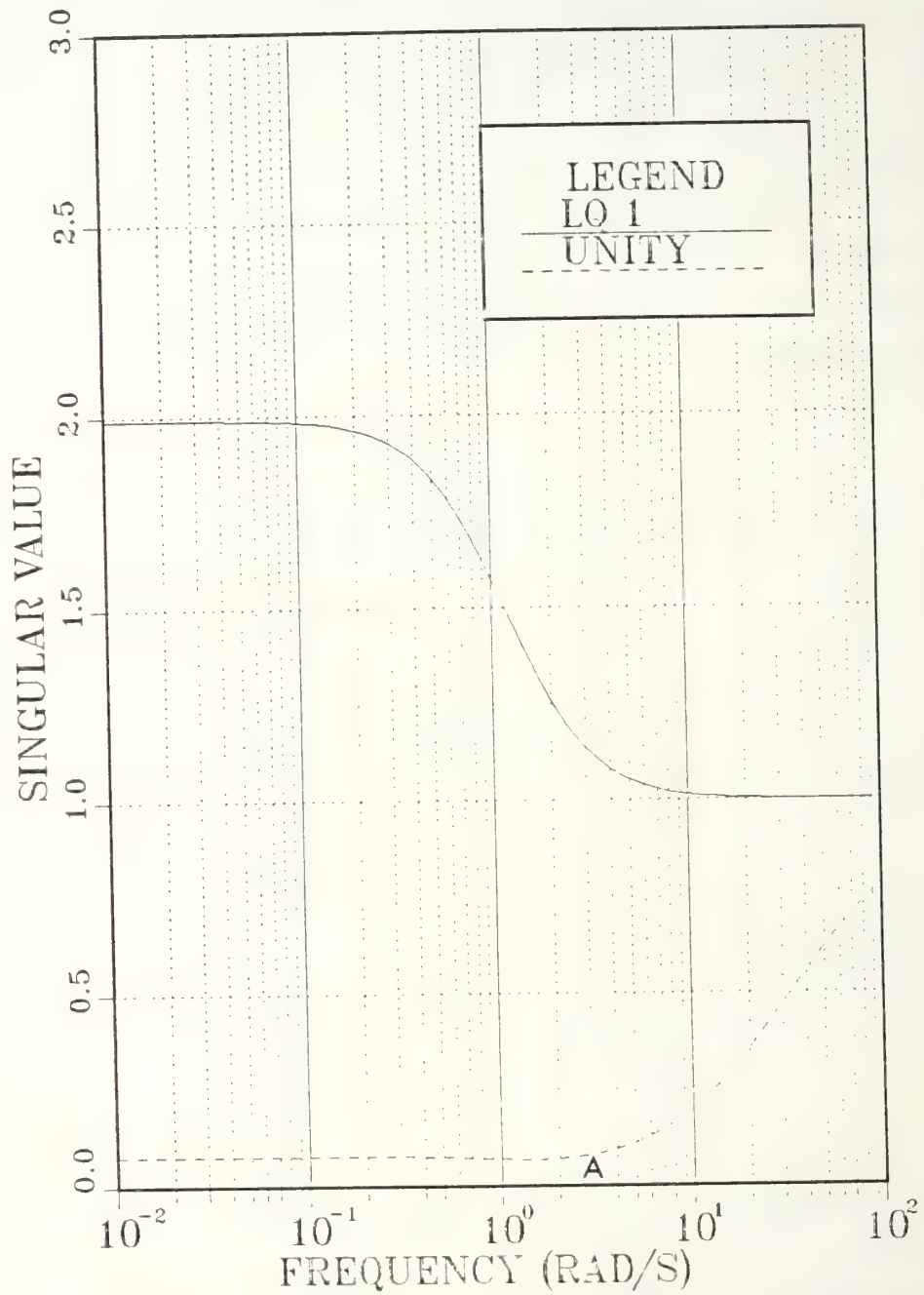
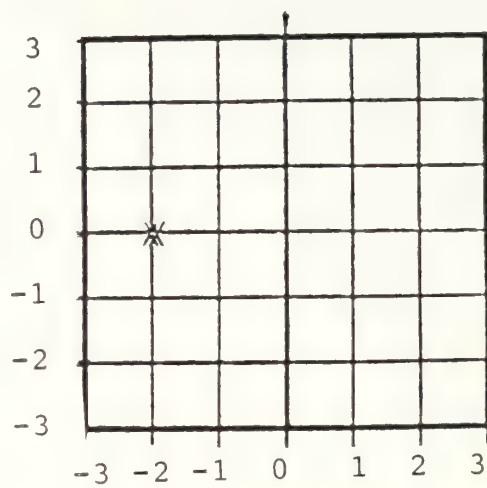


Figure 5.6 Comparison-Singular Value Plots (2x2 model).

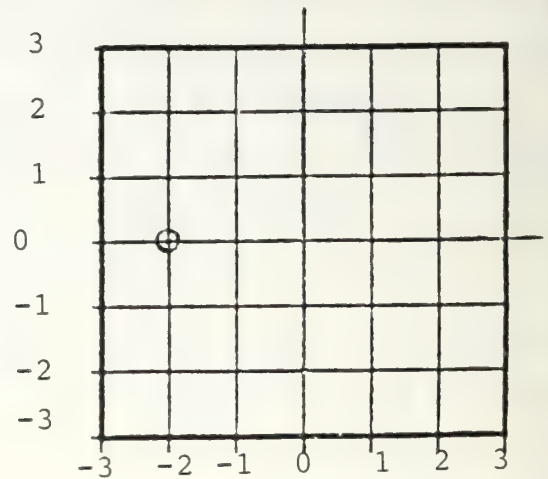
minimum singular value frequency ( point A in Figure 5.6). It is in fact this zero that causes the the system to be sensitive to perturbation. For the LQ design, the built in robustness cause the zero at minus three to move toward the pole location at -2.

Improvement in the robustness from LQ design is now analyzed in terms of Bode plots. The open-loop gain and phase vs frequency plots for a MIMO system can be obtained from the open-loop transfer function matrix,  $G(s)$ . For full state feedback,  $G(s)=F(sI-A)^{-1}B$ . (if the open-loop plots without feedback is considered,  $G(s)=C(sI-A)^{-1}B$ ) The matrix  $G$  is a matrix-valued rational function of  $s$ , it describes how the system (with or w/o feedback) appears to its environment. It is an external description of the system and is closely related to the zeros of the system. The open-loop Bode plots for the two designs are compared in Figures 5.9 to 5.11 As  $b_{21}=0$ , there is no coupling from channel 1 to channel 2. All channels have a -20 dB/decade slope at high frequency which is in agreement with earlier observation that each channels has one finite zero. It is interesting to note that the unity feedback and LQ design result in almost identical gain vs frequency plots for direct channels (i.e. channel 1-1 and 2-2). Any classical single loop type of analysis will not be able to detect any difference between the two designs. On the other hand, cross-coupling effect can be readily seen from the gain vs frequency plot in channel 2-1 (Figure 5.10). The unity feedback design is characterized by the rather large channel 2-1 gain at low frequency. A very small perturbation in channel one's parameter can change the system behavior considerably. This has been illustrated earlier by perturbing the feedback gain. It can be seen from the figure that LQ design reduces the crossfeed gain by large amount.

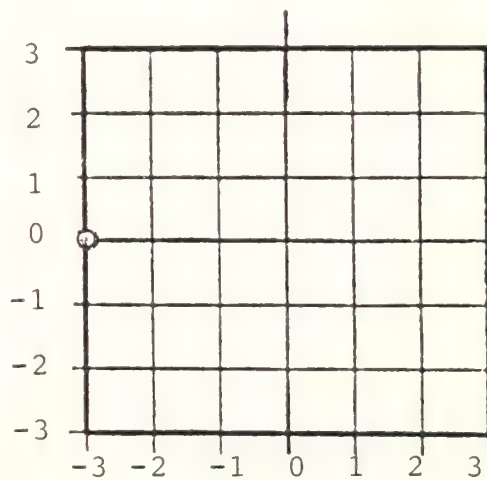




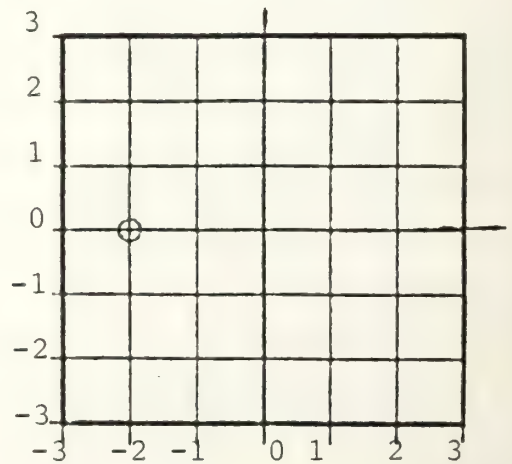
POLES (ALL)



ZERO ( 1 TO 1 )

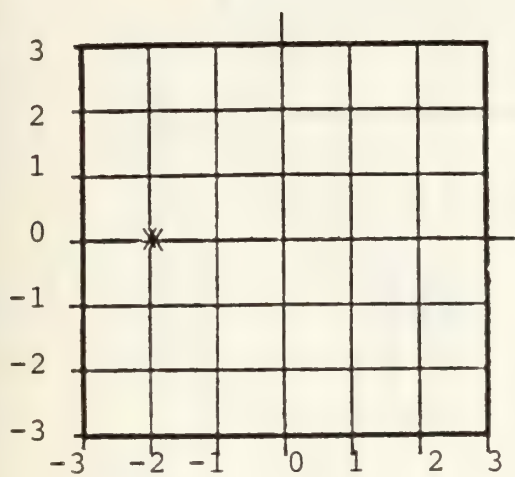


ZERO ( 2 TO 1 )

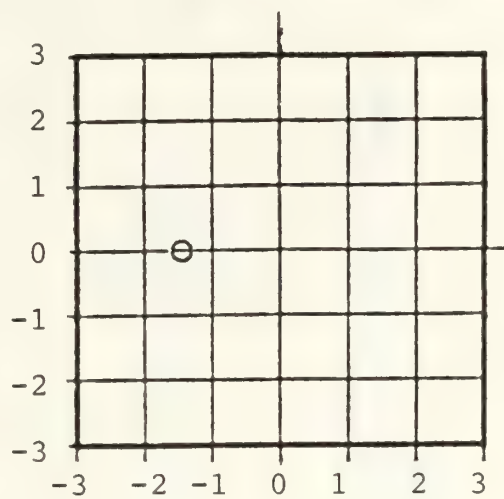


ZERO ( 2 TO 2 )

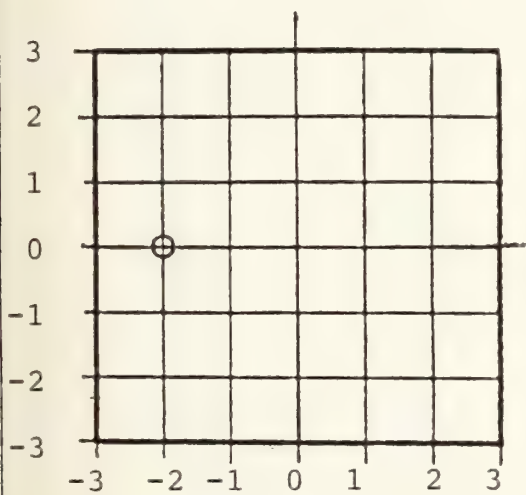
Figure 5.7 Closed-Loop Pole-Zero Plots (Unity Gain FB).



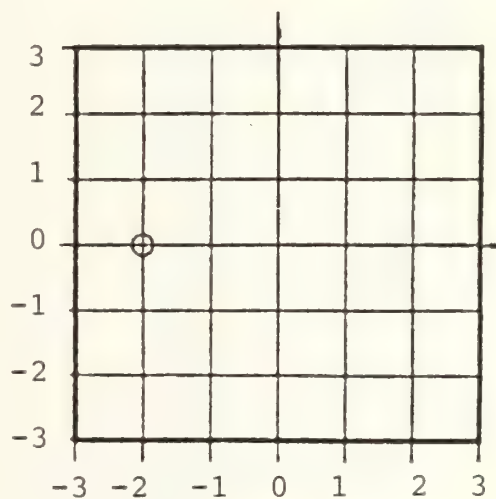
POLES ( ALL )



ZERO ( 1 TO 1 )



ZERO ( 2 TO 1 )



ZERO ( 2 TO 2 )

Figure 5.8 Closed-Loop Pole-Zero Plots (LQ Design).

# OPEN LOOP GAIN 1 - 1

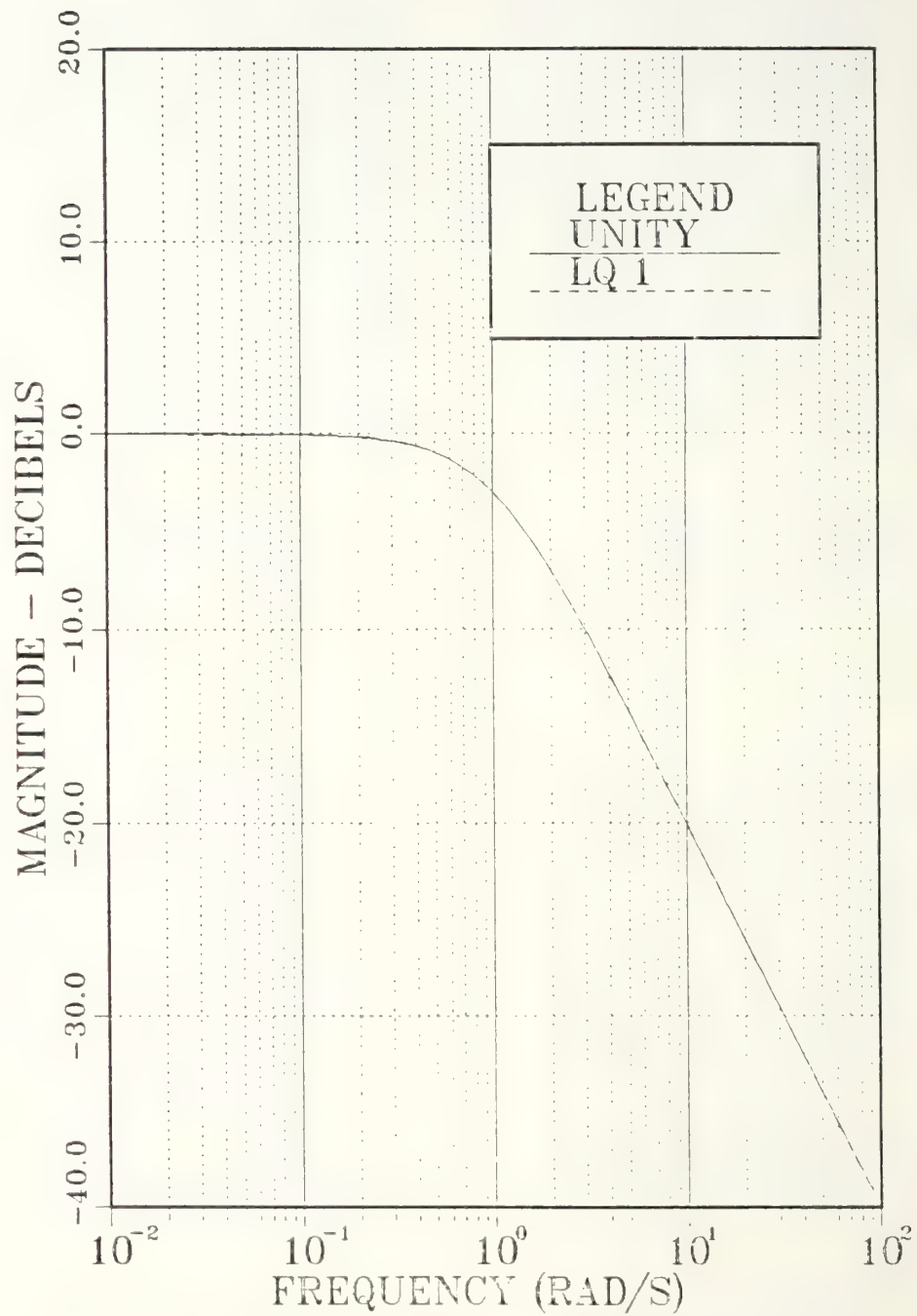


Figure 5.9 Open-Loop Bode Plots Channel 1-1.

# OPEN LOOP GAIN 2 - 1

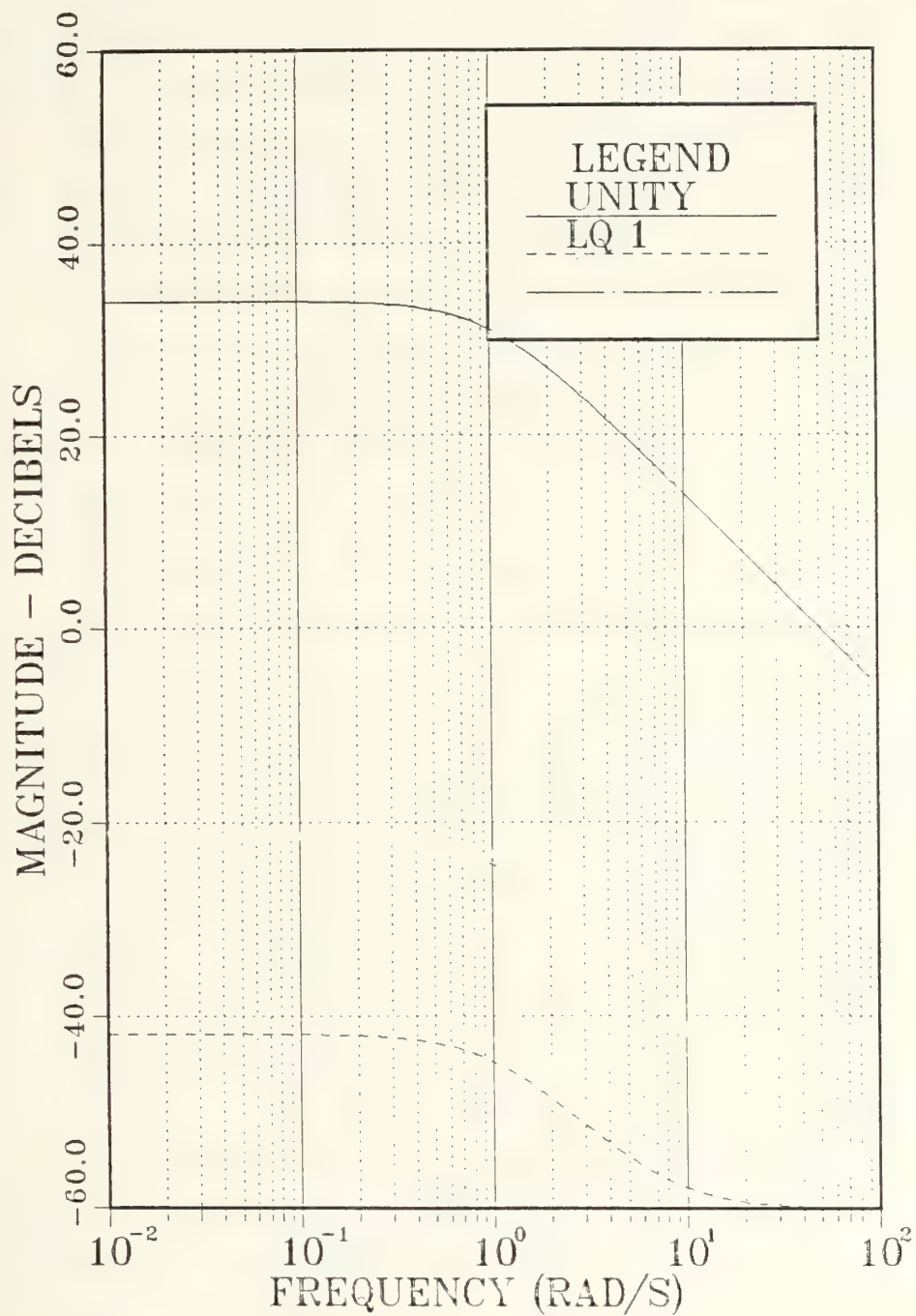


Figure 5.10 Open-Loop Bode Plots Channel 2-1.



## OPEN LOOP GAIN 2 - 2

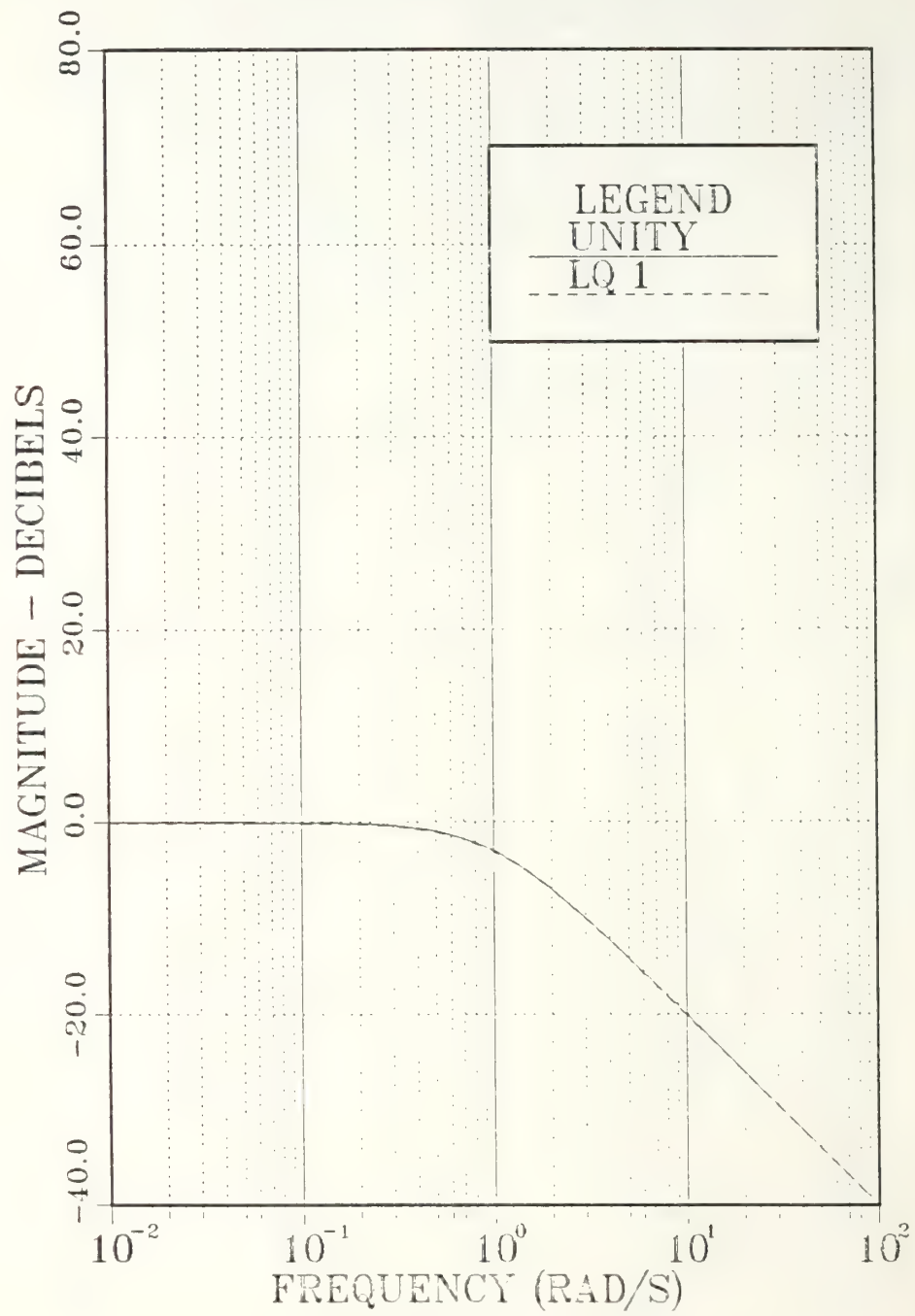


Figure 5.11 Open-Loop Bode Plots Channel 2-2.

## B. A HELICOPTER DESIGN PROBLEM

The design procedure described in Chapter 4 is further illustrated in this section by an actual design problem. A controller is designed using the Linear Quadratic Pole Placement approach for the lateral dynamic model of a CH-47 helicopter. The resulting design is then compared to multi-variable state feedback controller given in [Ref. 23].

The highly coupled two inputs lateral axis model of the CH-47 helicopter is used as a full order system. The state vector  $x(t)$  and control input vector  $u(t)$  are given by,

$x_1 = v =$  Y-axis velocity (ft/sec)

$x_2 = p =$  Roll rate (rad/sec)

$x_3 = r =$  Yaw rate (rad/sec)

$x_4 = \phi =$  Roll angle (rad)

$u_1 = \delta_b =$  Yaw rate rotor deflection control (inches.)

$u_2 = \delta_c =$  Roll rate rotor deflection control (inches.)

The state variables and the body axes of the aircraft are illustrated in Figure 5.12. The yaw and roll rotor deflection control produce changes in the yaw rate, side slip angle, roll rate and bank angle. Assuming full state feedback, the A, B, and C system matrices are given by,

$$A = \begin{bmatrix} -2.27 & 1.420 & -0.15 & 31.99 \\ .01 & -0.7 & -0.07 & 0.0 \\ 0.04 & -0.05 & -0.05 & 0. \\ 0. & 1. & 0.11 & 0. \end{bmatrix}$$

$$B = \begin{bmatrix} 0.12 & 0.95 \\ 0.04 & -8.37 \\ .34 & .020 \\ 0.0 & .0 \end{bmatrix} \quad C = \begin{bmatrix} 1 & 0 & 0 & 0 \\ 0 & 1 & 0 & 0 \\ 0 & 0 & 1 & 0 \\ 0 & 0 & 0 & 1 \end{bmatrix}$$

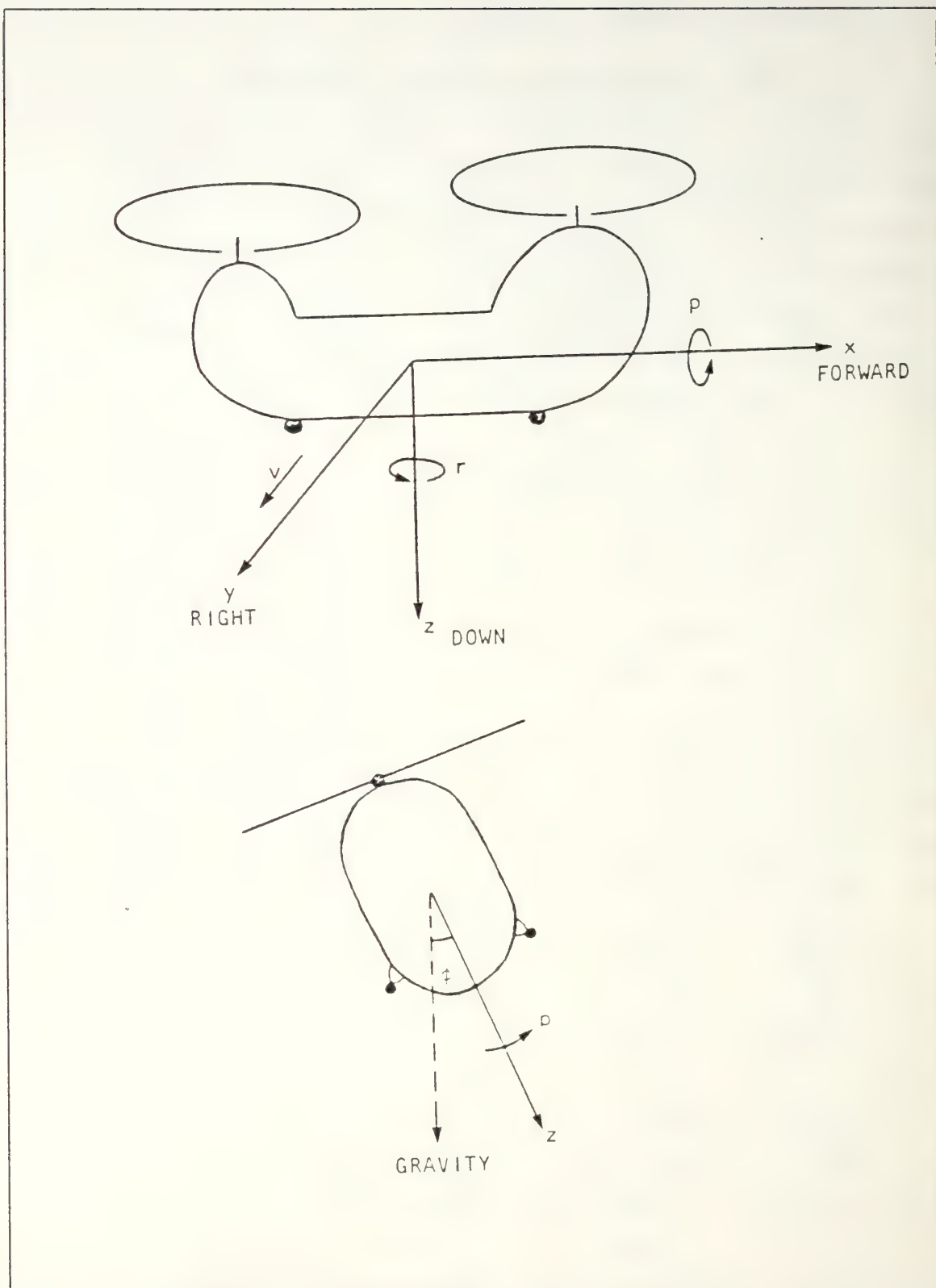


Figure 5.12 State Variables and Body Axes for CH-47.

The open loop eigenvalues of this system are;

$$\begin{aligned}s_1 &= +0.2065 \\s_2 &= -0.0503 \\s_3 &= -1.0498 \\s_4 &= -2.1263\end{aligned}$$

The open-loop system is not stable and the time response is shown in Figure 5.13 for zero input and an initial condition of  $\phi(0)=0.1$  rad

The design requirements are to satisfy specification in terms of the step input response of the roll attitude channel ( $\phi/\phi_c$ ). Stability margin requirements are those given by standard military specification. In [Ref. 23] three designs were obtained to satisfy the desired time response performance specification. All three control laws are of the form given by,

$$u(t) = -Fx(t) + h\phi_c(t) \quad (\text{eqn 5.7})$$

The values of  $F$  and  $h$  are summaried in Table III . It was shown in [Ref. 23] that two of the designs (design 1 and 2 ) were extremely sensitive to model errors and perturbations. It is now shown that LQ formulation using the pole placement procedure developed here will result in robustness design and yet satisfy the conventional time response criteria.

It is assumed that the closed-loop poles requirement are the same as those obtained in the AlphaTech's design 1. (-25.12, -12.51, -9.652, -2.125). The first step in the design is to establish some asymptotic properties of the system. The dimension of the control input (2) is less than the dimension of the state(4). As shown in Chapter 2, this implies that at least two closed-loop poles approach minus infinity in the complex plane when  $R \rightarrow 0$ . When  $R \rightarrow 0$  (meaning no control input allowed), the closed-loop poles



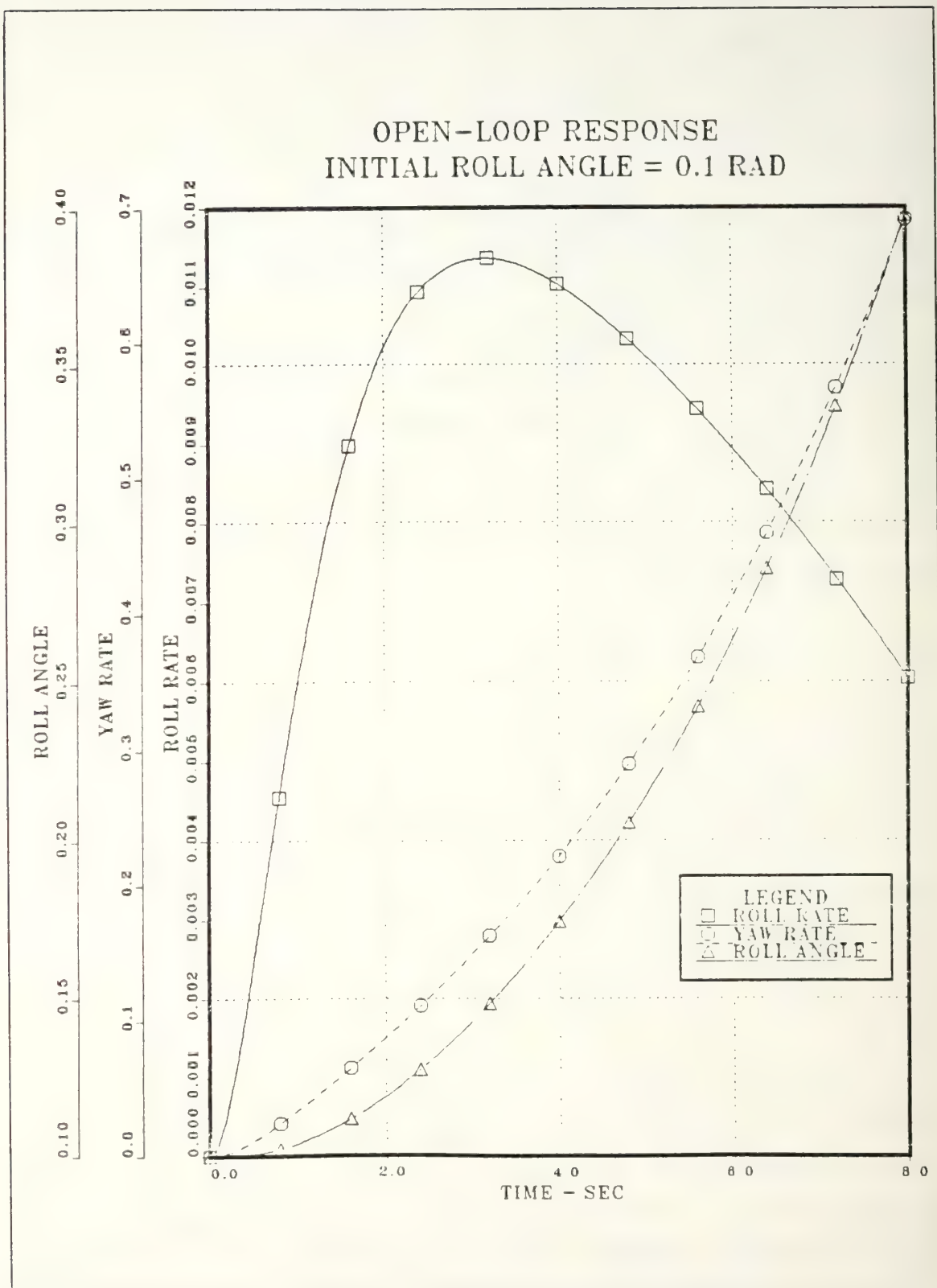


Figure 5.13 Open Loop Time Response  $\phi(0) = 0.1$  rad.

TABLE III  
ALPHATECH DESIGNS ( 1, 2, AND 3)

Designs	Feedback Gains (F)				h
one	-1.72 0.024	-23.5 -2.71	70.6 0.368	595 -7.99	595 -7.99
two	0.198 -0.01	154. -1.592	18.3 -0.189	142.0 -1.47	142.0 -1.47
three	0 0	0 -4	25.5 0	0 -27	0 -27

approach the open-loop poles or their mirror images if they are in the right hand plane. (i.e. -0.2065, -0.0503, -1.04987, and -2.12635).

The next step in the design procedure is to select a suitable starting control weighting matrix. Based on guideline given in [Ref. 4] and assuming that  $u_{1max}$  and  $u_{2max}$  are equal to 1 inch.  $R = I$  is selected for the initial design. (In the present formulation  $\rho$  is not needed as only  $Q$  is varied to place the pole ).

The sequence of the reassignment is determined next. At present there is no known established guideline for selecting the preferred sequence of moving the poles. Two extreme sequences are considered as follows,

A. Move the left most open-loop pole to the left most desired closed-loop pole etc. The reassignment sequence then become:

1. move pole at -2.1265 to -25.12
2. move pole at -1.0483 to -12.51

3. move pole at -0.2065 to -9.652
4. move pole at -0.0503 to -2.125

B. Move the right most open-loop pole to the left most desired closed-loop pole etc. For the problem given, the reassignment sequence are :

1. move pole at +0.2065 to -25.12
  2. move pole at -0.0503 to -12.51
  3. move pole at -1.0498 to -9.652
  4. move pole at -2.126 to -2.125
- (close, so no move required)

Using the pole placement program developed in this thesis, the corresponding  $Q$  and  $F$  for each of the reassignments are obtained and tabulated in Tables IV and V for the two cases selected (design LQ-A and LQ-B). It can be seen from the table that difference reassignment sequence results in different set of  $Q_e$  and  $F_e$ . In general, once the matrix  $R$  and the  $n$  closed-loop poles are selected, there are  $n(n+1)/2$  extra degrees of freedom available in  $Q$ . This also verifies the well-known fact that the general solutions of  $Q$  and  $R$  for a given set of closed-loop eigenvalue are non-unique. The elements of the  $Q$  matrix obtained during each reassignment depends on the transformation matrix ( $M$ ,  $L$  or  $U$ ) and hence the eigenvectors that are used to construct them. The important of eigenvector type of assignment is evident as  $Q$ ,  $F$  and the resulting closed-loop poles depend on the eigenvectors used. The designer can shape the design by choosing appropriate eigenvectors for the transformation matrix. The application of these extra degrees of freedom will be discussed in the following section. The resulting designs (LQ-A and LQ-B) are now compared with the first design in [Ref. 23].

TABLE IV  
RESULTS FROM POLE PLACEMENT SEQUENCE(LQ-A)

Move	Q and F obtained during each reassignment			
Q <sub>1</sub>	0.10027	0.96194	0.11959	-1.50849
	0.96194	9.22847	1.14725	-14.47182
F <sub>1</sub>	0.11959	1.14725	0.14262	-1.79908
	-1.50849	-14.47182	-1.79908	22.69429
Q <sub>2</sub>	0.00387	0.03151	0.00399	-0.06416
	-0.24260	-2.83522	-0.34541	3.11642
Q <sub>3</sub>	6.12853	-2.99198	0.51376	-95.14285
	9198	1.46070	-0.25082	46.44916
F <sub>2</sub>	0.51376	-0.25082	0.04307	-7.97589
	-95.14284	46.44916	-7.97589	1477.05225
Q <sub>4</sub>	0.05825	-0.02844	0.00490	-0.90426
	2.27529	-1.11079	0.19079	-35.32260
Q <sub>5</sub>	80.37563	18.91502	13.64762	218.27522
	18.91502	4.45133	3.21173	51.36732
F <sub>3</sub>	13.64761	3.21173	2.31734	37.06267
	218.27521	51.36732	37.06267	592.76758
Q <sub>6</sub>	1.58772	0.37365	0.26961	4.31182
	-8.62241	-2.02917	-1.46414	-23.41618
Q <sub>7</sub>	0.15575	0.02839	-2.48989	0.19453
	0.02839	0.00517	-0.45383	0.03546
F <sub>4</sub>	-2.48989	-0.45383	39.80322	-3.10981
	.19453	0.03546	-3.10981	0.24297
Q <sub>8</sub>	-0.38007	-0.06927	6.07574	-0.47469
	-0.06411	-0.01168	1.02482	-0.08007
Q <sub>9</sub>	86.76016	16.91336	11.79108	121.81841
	16.91336	15.14567	3.65433	83.38010
F <sub>5</sub>	11.79107	3.65433	42.30624	24.17787
	121.81841	83.38010	24.17787	2092.75684
Q <sub>10</sub>	1.26977	0.30745	6.35424	2.86871
	-6.65383	-5.98686	-0.59394	-55.70242

$$u(t) = -Fx(t) + h\phi_c(t), \quad h = \begin{bmatrix} 2.8687 \\ -55.7024 \end{bmatrix}$$



TABLE V  
RESULTS FROM POLE PLACEMENT SEQUENCE(LQ-B)

Move	Q and F obtained during each reassignment			
Q <sub>1</sub>	0.00031	0.05289	0.00589	0.04781
	0.05289	9.06491	1.00865	8.19296
	0.00589	1.00865	0.11223	0.91163
	0.04781	8.19296	0.91163	7.40489
F <sub>1</sub>	0.00017	0.02851	0.00317	0.02576
	-0.01771	-3.03548	-0.33776	-2.74347
Q <sub>2</sub>	0.26982	0.46312	16.33746	10.89106
	0.46312	0.79492	28.04224	18.69380
	16.33746	28.04222	989.23975	659.45752
	10.89106	18.69380	659.45728	439.61426
F <sub>2</sub>	0.44607	0.76563	27.00978	18.00517
	-0.26207	-0.44982	-15.86824	-10.57837
Q <sub>3</sub>	0.16317	-0.35205	6.24519	-9.35123
	-0.35205	0.75956	-13.47424	20.17563
	6.24519	-13.47425	239.02527	-357.90405
	-9.35123	20.17563	-357.90381	535.90698
F <sub>3</sub>	0.19939	-0.43018	7.63129	-11.42668
	0.30220	-0.65201	11.56628	-17.31876
Q <sub>e</sub>	0.43330	0.16396	22.58853	1.58764
	0.16396	10.61939	15.57663	47.06238
	22.58853	15.57661	1228.37695	302.46509
	1.58764	47.06238	302.46509	982.92603
F <sub>e</sub>	0.64563	0.36396	34.64423	6.60425
	0.02242	-4.13731	-4.63971	-30.64059

$$u(t) = -F_x(t) + h \phi_c(t), \quad h = \begin{bmatrix} 6.60425 \\ -30.64059 \end{bmatrix}$$

Closed loop time response for a step input in roll attitude command ( $\phi_c = 0.1$  rad) for the three designs are shown in Figures 5.14 to 5.16. It can be seen from the response plots that although all three designs have almost identical closed-loop pole location, the step response for various states differs. The AlphaTech design's response is characterized by the large 'overshoot' in the yaw rate step response. In the Linear Quadratic Design (LQ-A), the 'overshoot' occurs with the roll attitude response rather than

the yaw rate response; the yaw rate response is well damped. The LQ-B design appears to be a better design as coupling among modes are small and can not be detected from the time response plot. It is noted that the difference in response for the same set of closed-loop eigenvalue is due to coupling among various modes through their respective eigenvectors. The 'overshoot' in this case is obviously not due to complex conjugate poles as all closed-loop poles in the three designs are on the real axis. The set of final eigenvector for the three designs are tabulated in Table VI. Inter-mode coupling for the yaw rate response in the AlphaTech design and roll attitude response in the LQ design case A can be readily seen from the table. The issue of eigenvector assignment will be discussed in the next section.

TABLE VI  
CLOSED-LOOP EIGENVECTORS

Eigenvalues/Eigenvector				
Alpha one	-24.79907	-2.12242	-9.72403	-11.9449
	-0.39336	-0.99976	-0.48016	-0.41854
	0.10767	0.00822	-0.32948	-0.33640
	-0.91306	0.01955	-0.81181	-0.84283
	-0.00029	-0.00488	0.04306	0.03593
LQ-A	-2.12499	-9.26645	-12.52066	-25.20990
	0.22870	-0.15459	0.01894	-0.12653
	0.18018	-0.98218	-0.99664	0.99118
	-0.95603	-0.01258	-0.00396	0.00031
	-0.03529	0.10614	0.07964	-0.03932
LQ-B	-25.17894	-9.62708	-12.51644	-2.12630
	-0.12652	-0.13209	0.05042	-0.99977
	0.99118	-0.98557	-0.99375	0.00797
	0.00024	-0.02568	0.06075	0.01945
	-0.03937	0.10267	0.07886	-0.00475

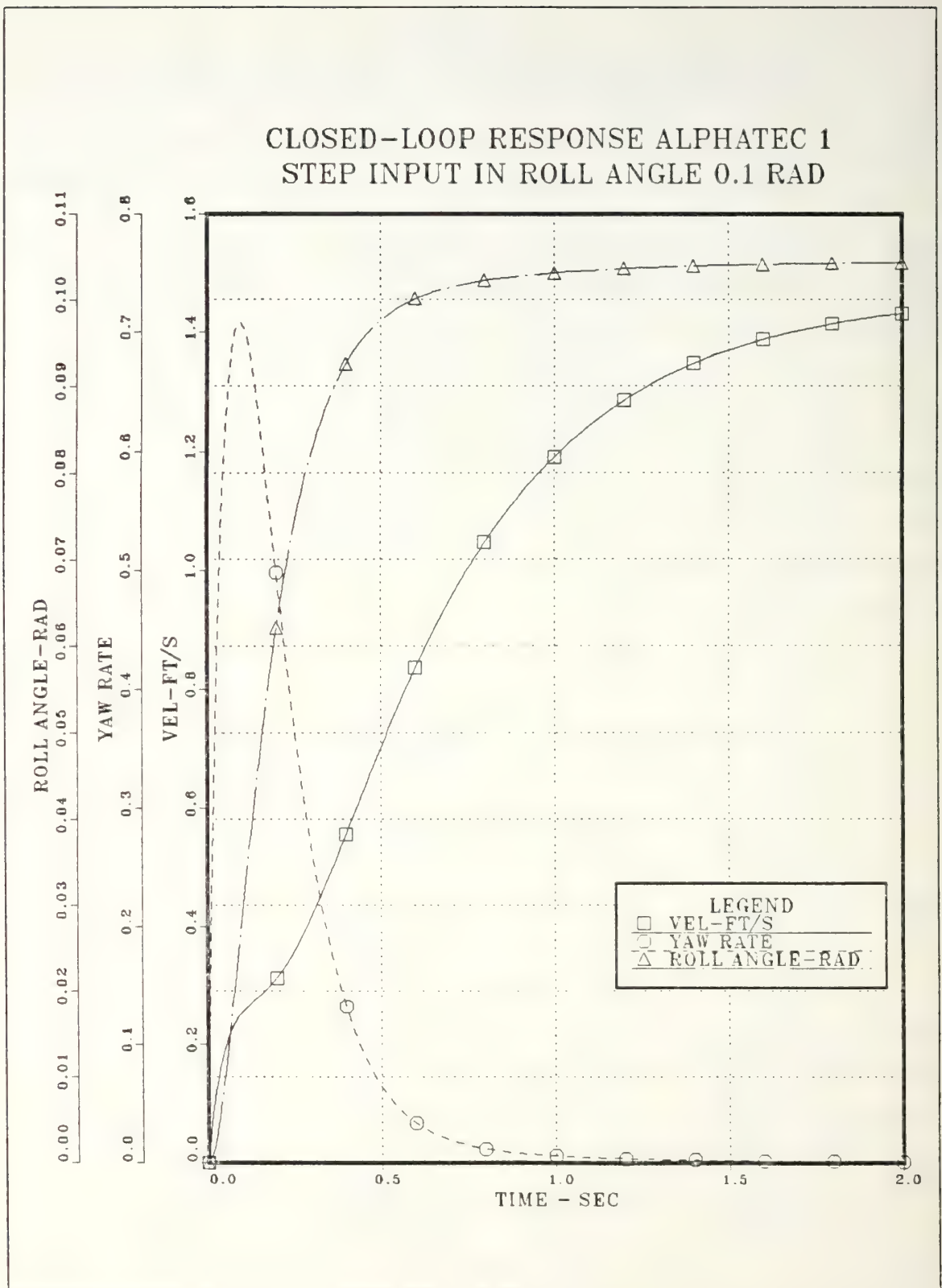


Figure 5.14 Closed-Loop Time Response Plot (AlphaTech 1).

# CLOSED LOOP RESPONSE LQ-A STEP INPUT IN ROLL ANGLE 0.1 RAD

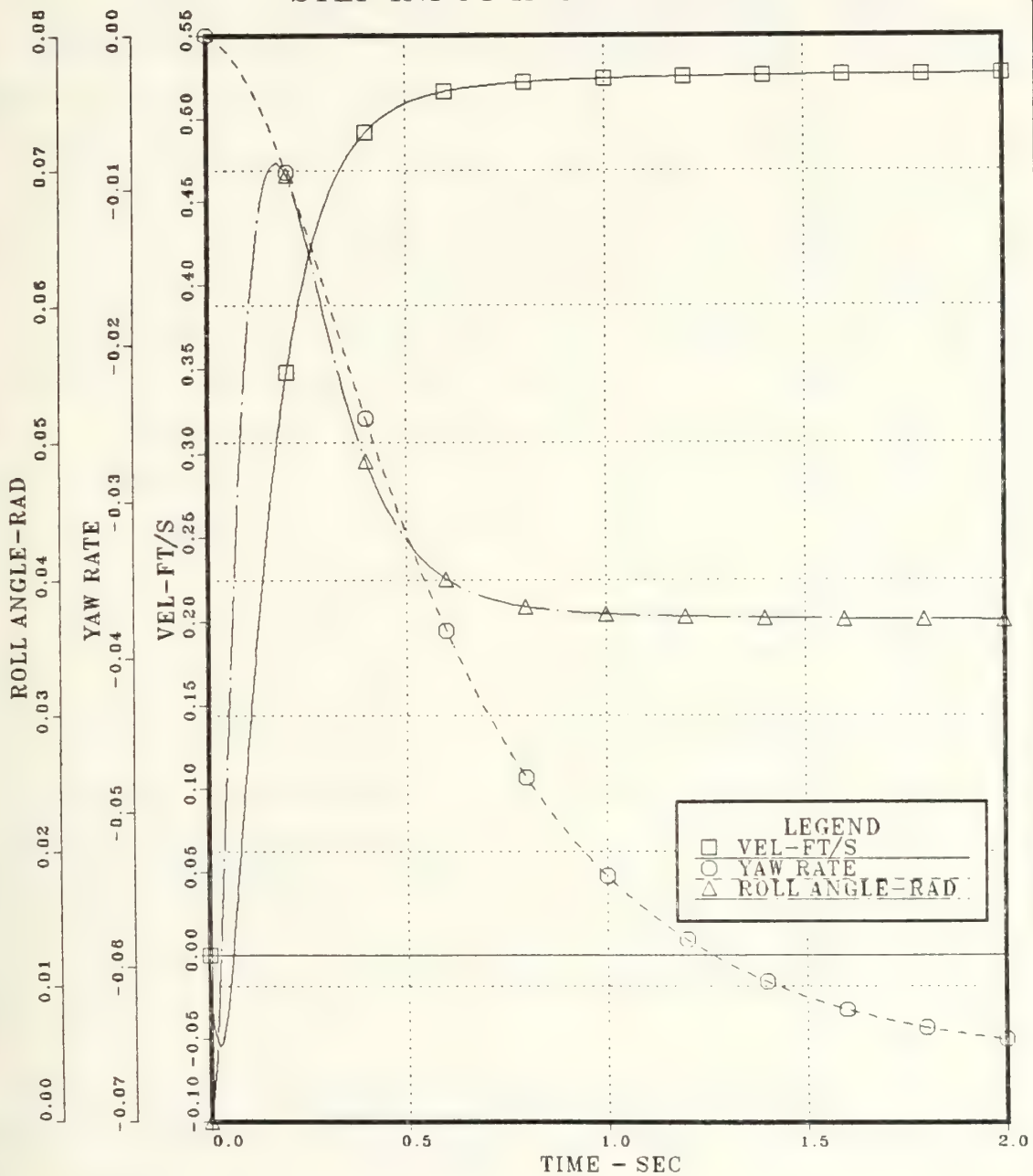


Figure 5.15 Closed-Loop Time Response Plot (LQ-A).

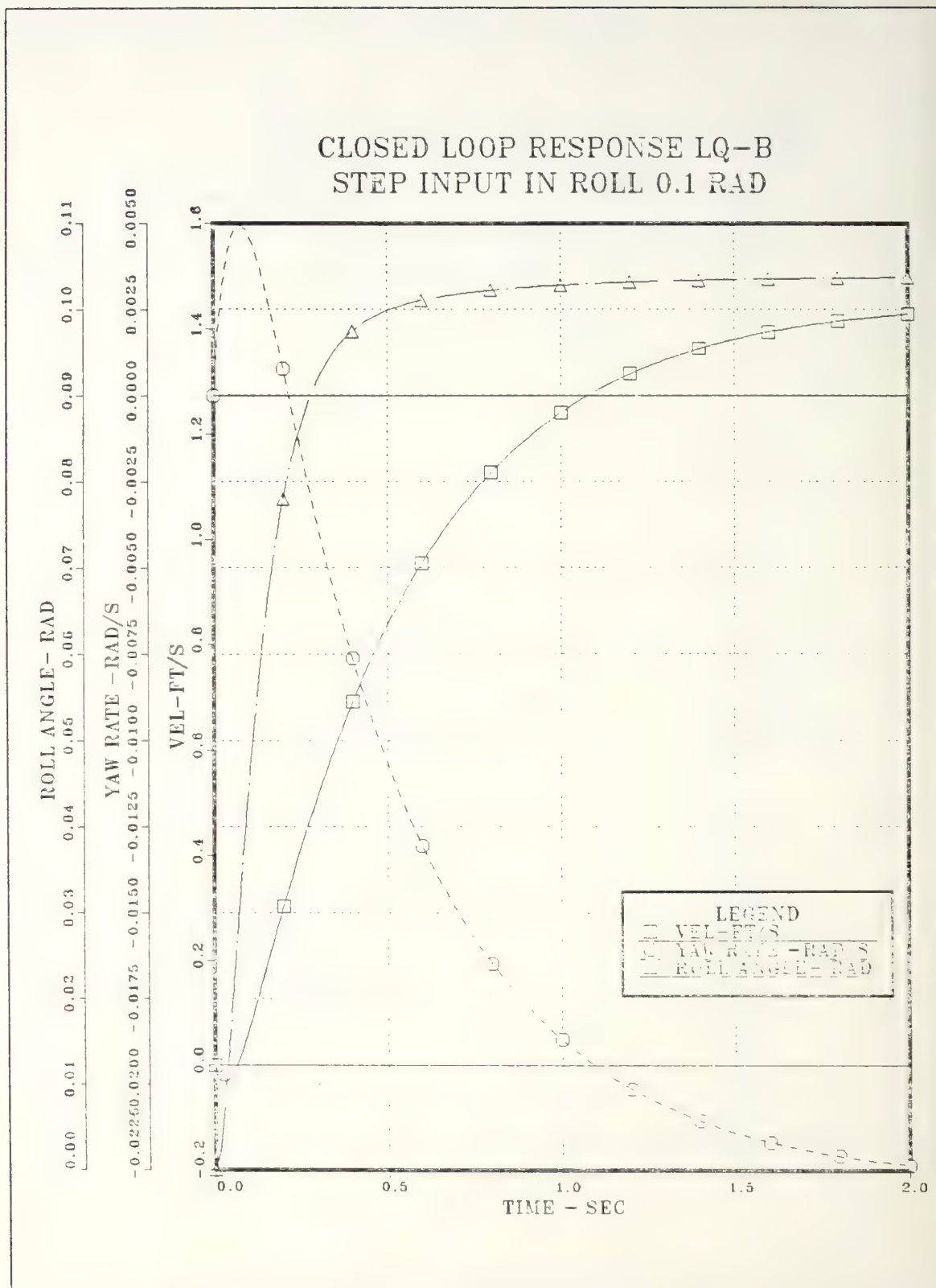


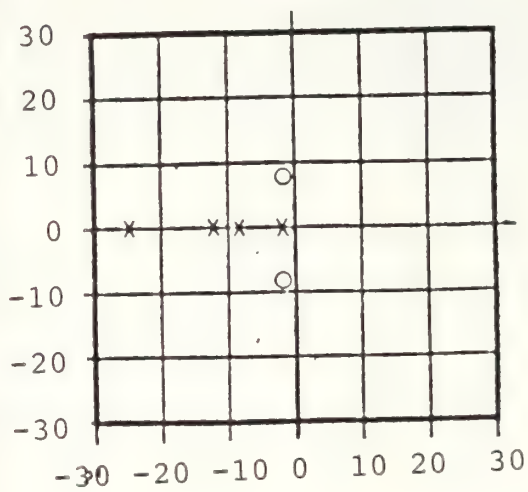
Figure 5.16 Closed-Loop Time Response Plot (LQ-B).



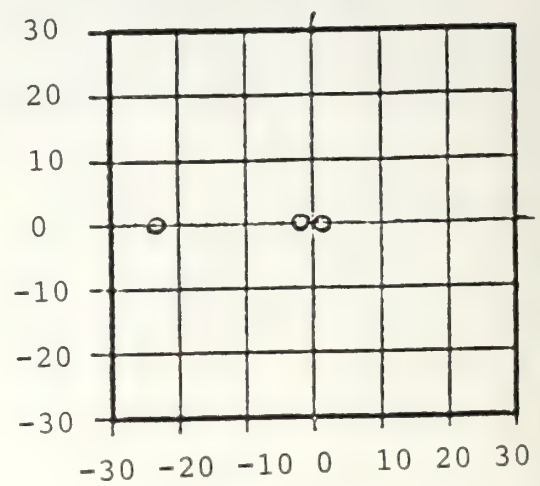
The difference in time response performance for the three designs can also be interpreted in term of the closed-loop pole-zero plots in the frequency domain. The pole-zero plots for the designs, with  $\phi_c$  as the input, are shown in Figures 5.17 to 5.19 . As all pole locations are the same for the three designs, they are indicated only once in each diagram.

In the AlphaTech's design, the zero locations for the various channels clearly indicate the weakness in the design. Most transmissions zeros are located away from the poles locations. The system is therefore strongly coupled to its external environment. A good example is the lightly "damped" pair of zero at  $(-1.05, \pm 7.31j)$  for the  $v-\phi_c$  channels. It is in fact these undesired zeros that reduce the overall robustness of the system. The mechanism of robustness improvement in the LQ design can also be seen in the pole-zero plots in Figures 5.18 and 5.19 The built-in robustness in the LQ design causes the zeros at various channels to move to locations where their transmission properties can be canceled by the closed-loop poles. An excellent example is in the  $v-\phi_c$  channel, where the zeros at -2, -7, and the mirror image of +24.0 are fairly close to the closed-loop pole locations at -2.12, -9.26 and -25.12. In the case where the zero from LQ design are not close to the closed-loop poles ( $r-\phi_c$  channel for LQ-A ) the zeros are "well damped" and their transmission properties can be neglected.

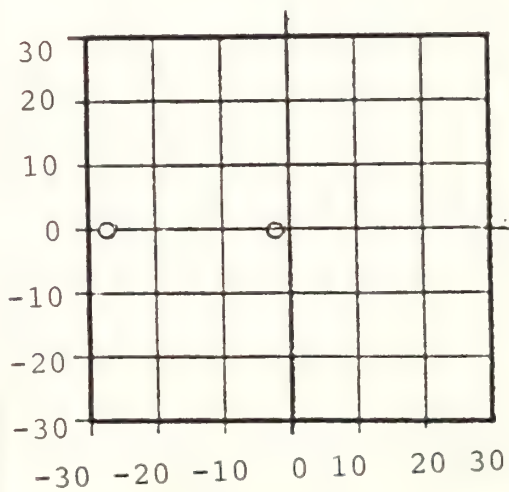
Robustness properties of the three designs presented here can also be analyzed from the open-loop Bode plots. The open-loop transfer function gain plots for channel 1-1, 1-2, 2-1 and 2-2 for the three designs are shown in Figures 5.20 to 5.24 Cross coupling problem for the AlphaTech design is clearly indicated by the relatively high gain of



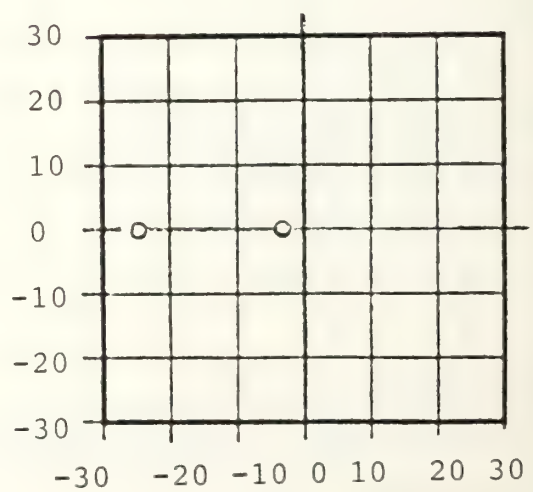
$$V - \phi_c$$



$$\dot{\phi} - \phi_c$$

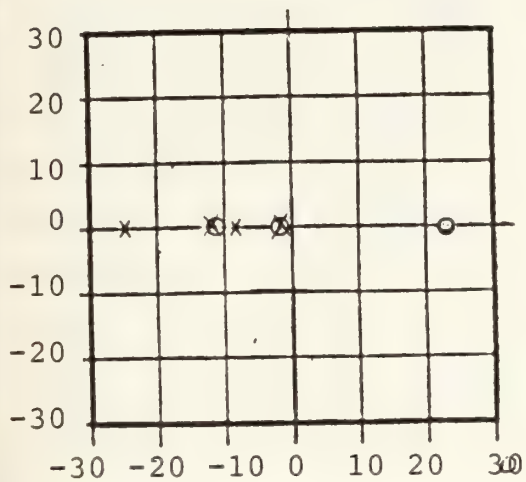


$$R - \phi_c$$

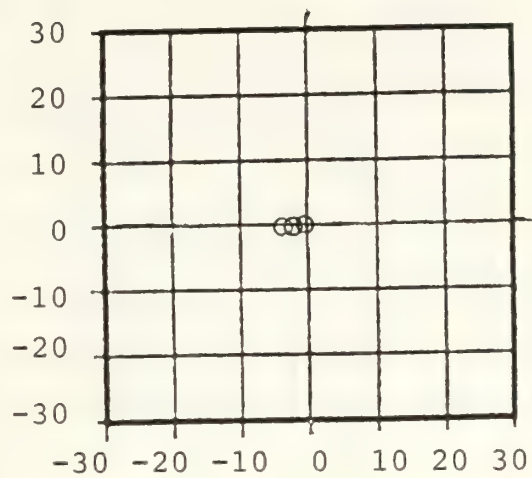


$$\phi - \phi_c$$

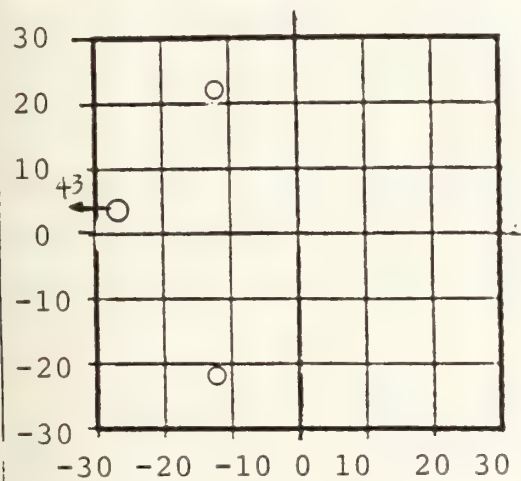
Figure 5.17 Closed-Loop Pole-Zero Plots (AlphaTech 1).



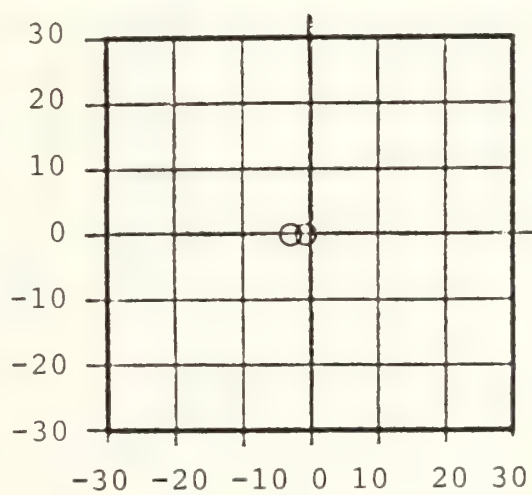
$$V - \phi_c$$



$$\dot{\phi} - \phi_c$$

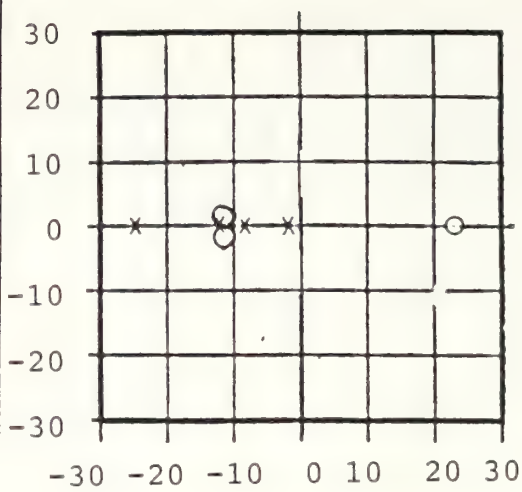


$$R - \phi_c$$

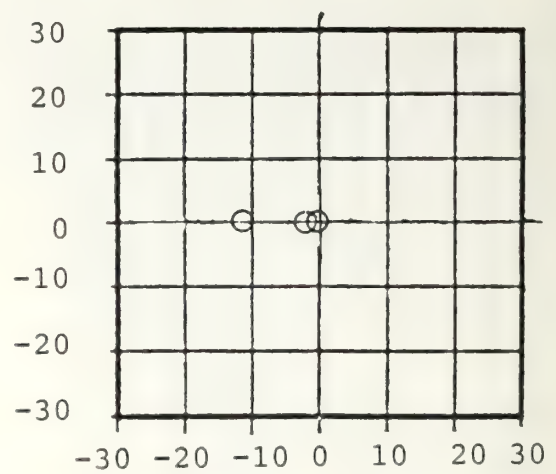


$$\phi - \phi_c$$

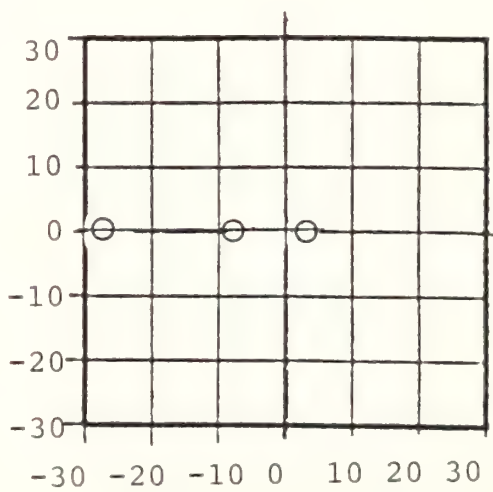
Figure 5.18 Closed-Loop Pole-Zero Plots (LQ-A).



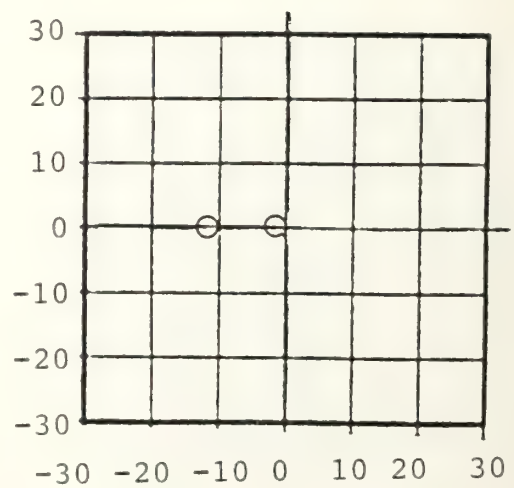
$$V - \phi_c$$



$$\dot{\phi} - \phi_c$$



$$R - \phi_c$$



$$\phi - \phi_c$$

Figure 5.19 Closed-Loop Pole-Zero Plots (LQ-B).



the channel from input 2 to input 1 (2-1). Both LQ designs presented here reduced the gain in this channel by more than 40 dB in the frequencies of interest. The bandwidth is reduced from above 100 rad/s to about 8 rad/s. Unlike the simple (2x2) system where there was little difference between the direct channels of the two designs, gain adjustment is observed in all channels. For example, LQ designs reduce the gain in channel 1-1 but increase the gain in channel 2-2. There is also a slight increase in the coupling channel 1-2. The overall effect is that of gain balancing, gains in channels that are affected by cross-coupling perturbation are lowered together with some adjustments in other channels. Different reassignment sequence results in different adjustments. The designer has to choose a set of gain curve depending on the particular requirement. The relationship between the open-loop Bode plots and the zeros of the system is also evident from these diagrams. The low frequency resonance (or 'peak') in the gain vs frequency plot for the AlphaTech design correspond to the undesirable zero mentioned earlier. In the LQ designs, these low frequency resonances are absent because of the more desirable zero locations. It is also interesting to note that the LQ-B gain curves fall nicely in between the other two designs. This fact, together with its better overall low frequency gain characteristic, may account for the better time response behavior of the LQ-B design.

As a final comparison, the closed-loop frequency response plots of the various channel for the three designs are shown in Figures 5.25 to 5.32. At high frequency, all the gain plots approach the -20dB/decade slope as all eigenvalues are on the real axis. The AlphaTech design has a near 0db gain for frequency up to about 2 rad/s. It appears



# OPEN LOOP GAIN 1 - 1

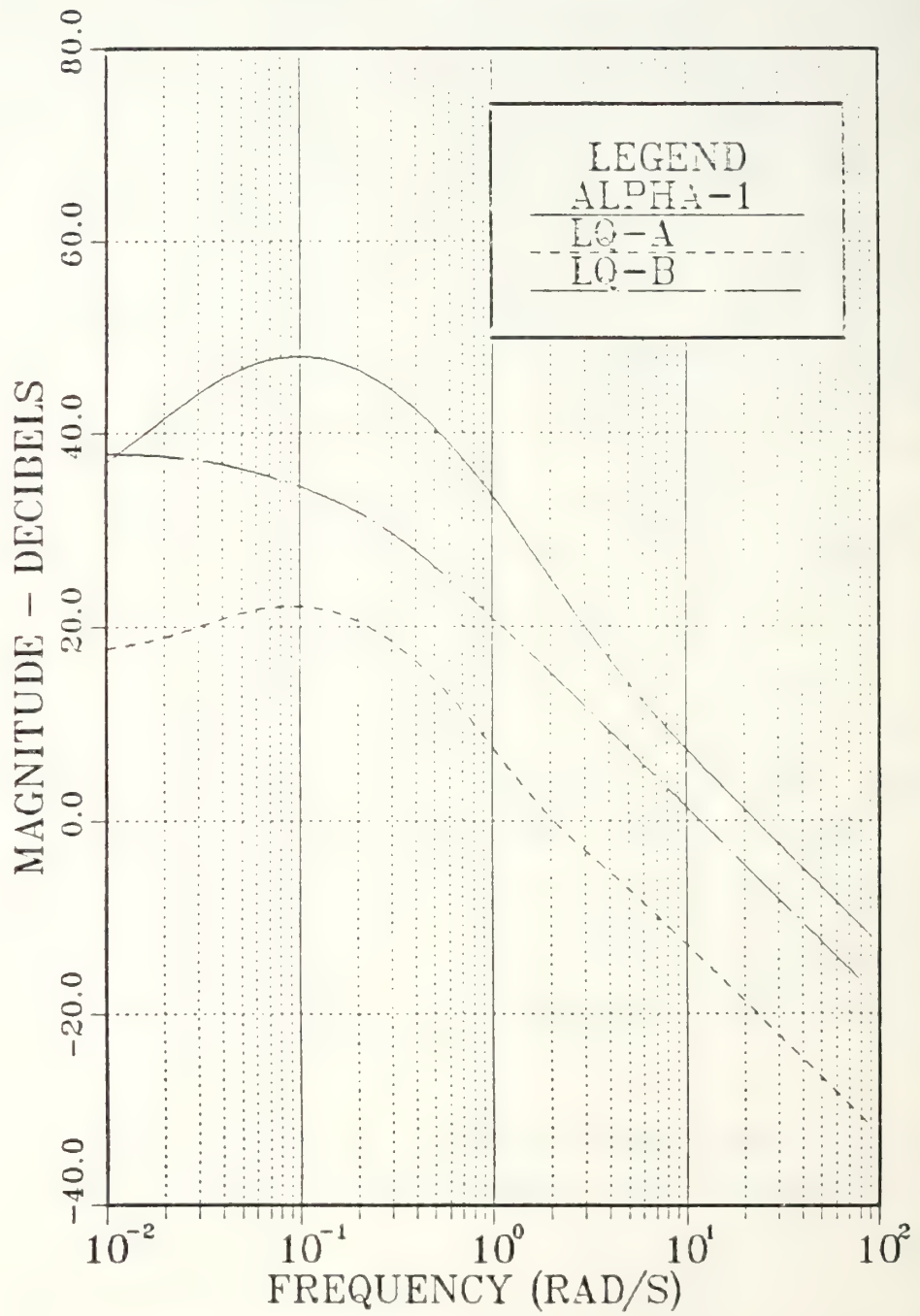


Figure 5.20 Bode Plots Comparison- Input 1-1.

# OPEN LOOP GAIN 1-2

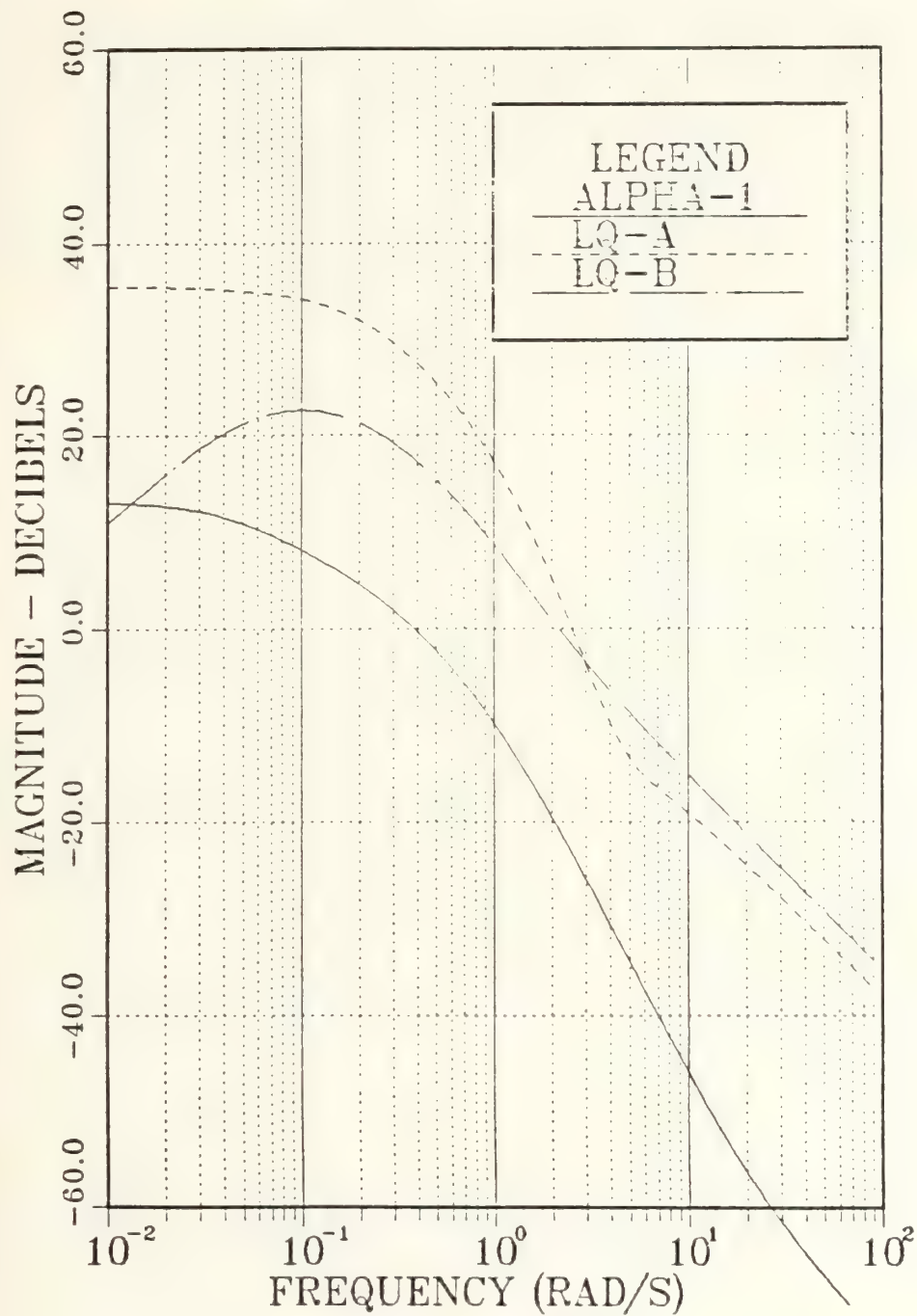


Figure 5.21 Bode Plots Comparison - Input 1-2.

# OPEN LOOP GAIN 2-1

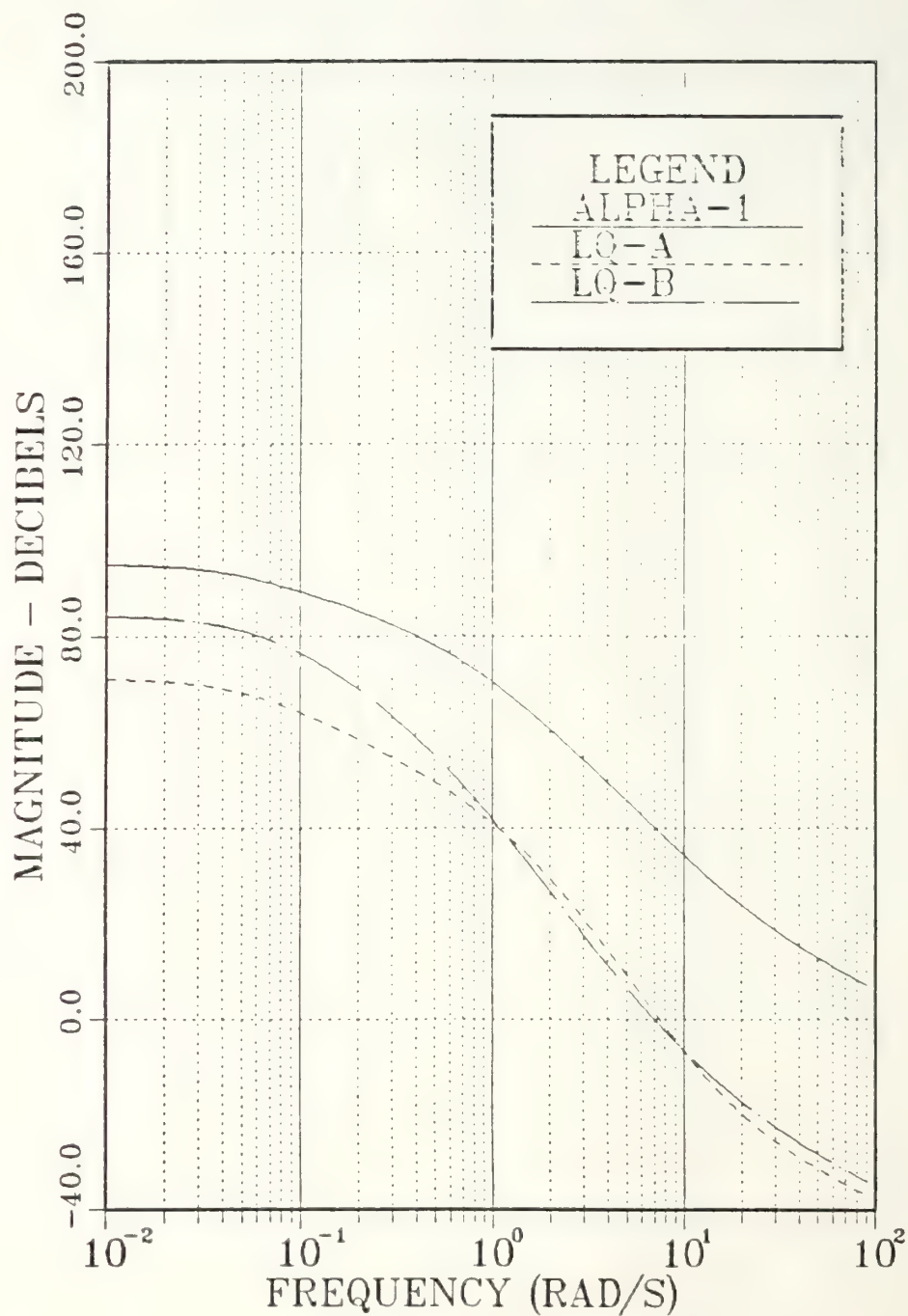


Figure 5.22 Bode Plots Comparison - Input 2-1.

# OPEN LOOP GAIN 2-2

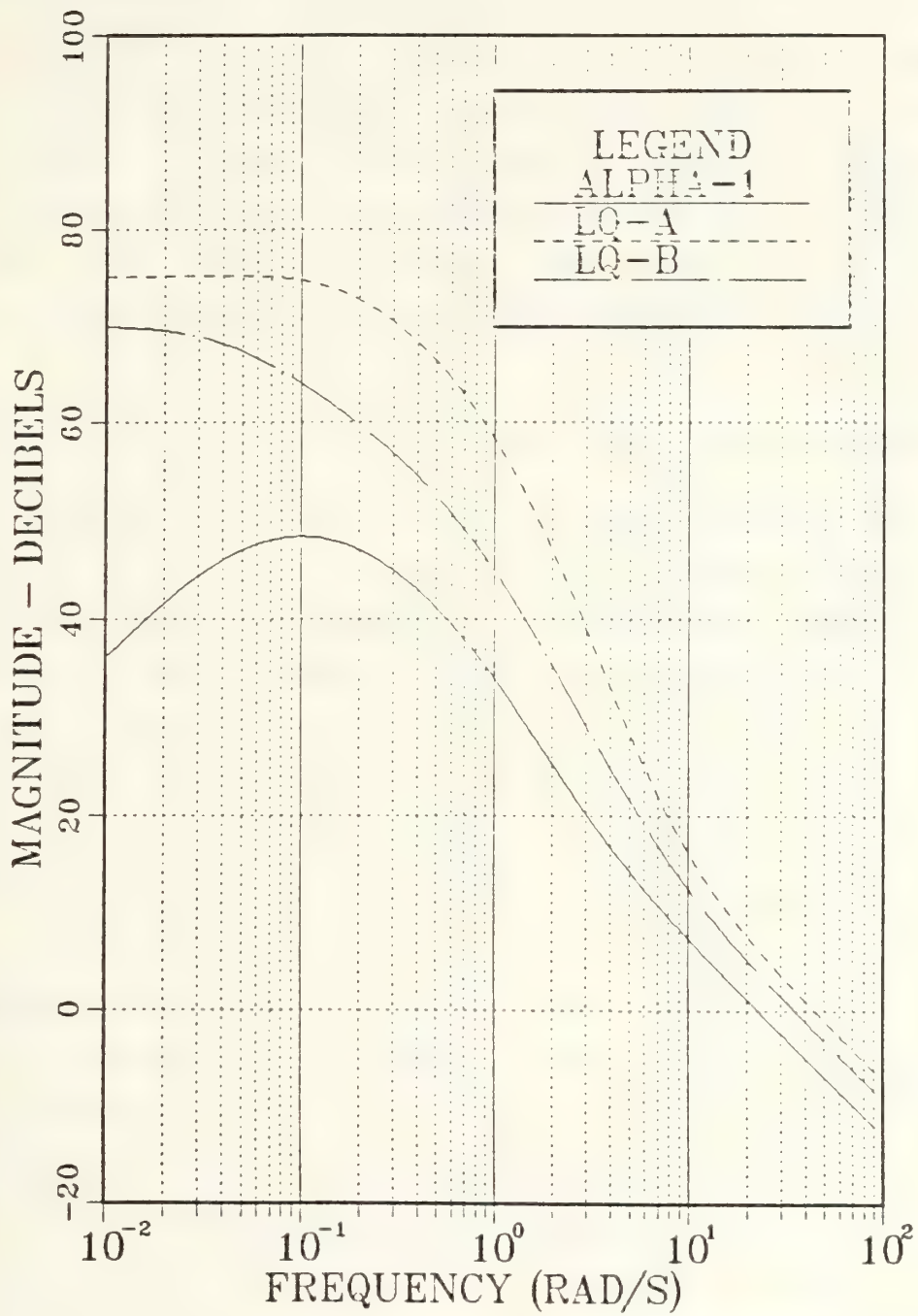


Figure 5.23 Bode Plots Comparison - Input 2-2.

to be an acceptable design but was shown to have undesired transmission zeros in other channels; this can also be seen from the closed-loop plot for the  $r-\phi_c$  channel in Figure 5.31. Design LQ-A, obtained from the reassignment sequence A, is characterized by very low DC gain (-9dB) and 'peak' in frequencies near 10 rad/s. These have been shown, both in the time response and pole-zero discussions that it will have undesired effect on the pilot's control. Design LQ-B, obtained from the second reassignment sequence appears to be the best compromise. All channels (Figures 5.30 to 5.32) have flat low frequency characteristic and coupling between modes are almost absent.

### C. DISCUSSION AND CONCLUDING REMARKS

A new computer aided design procedure for the multivariable linear time-invariant system using Linear Quadratic Pole Placement formulation is presented. The two design examples presented above have served to demonstrate the complexity involved in a multivariable design. The main problem lies in the fact that the solution of a MIMO problem is in general non-unique. This was shown in the helicopter problem where different approaches result in different designs, although the closed-loop eigenvalues for all designs were the same. It was also shown that the extra degrees of freedom in MIMO system design can be accounted for by analyzing the singular value plots, transmission zero movements and closed-loop eigenvectors of the designs. It becomes apparent that the success of any multivariable design methodology hinges on how to make use of these extra degrees of freedom available in MIMO system. It was also shown in the above design examples that the Linear Quadratic Pole Placement procedures possess such quality. Some unique properties of the method presented here are as follows;



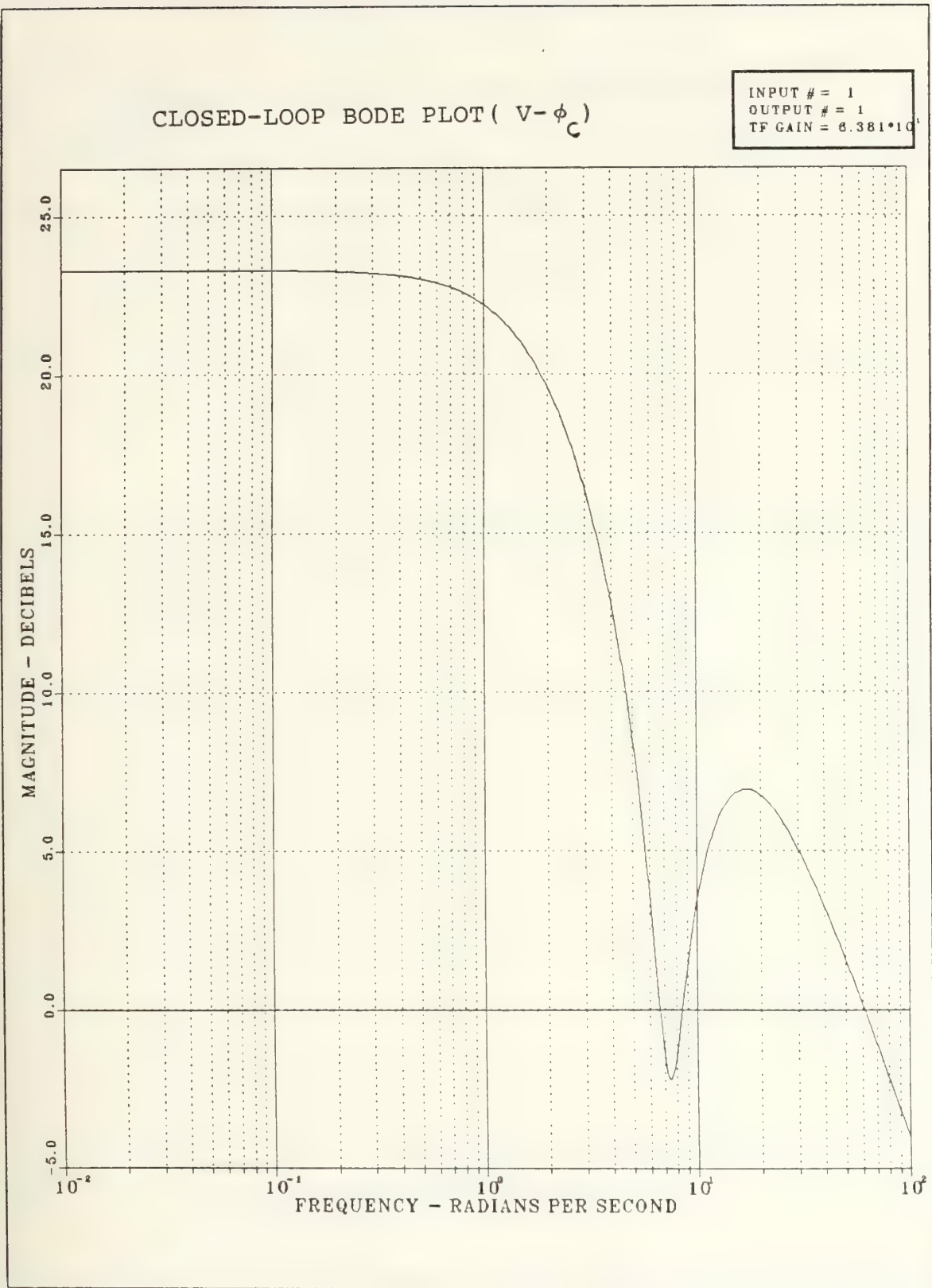


Figure 5.24 Closed-Loop Bode Plot- AlphaTech 1-1.

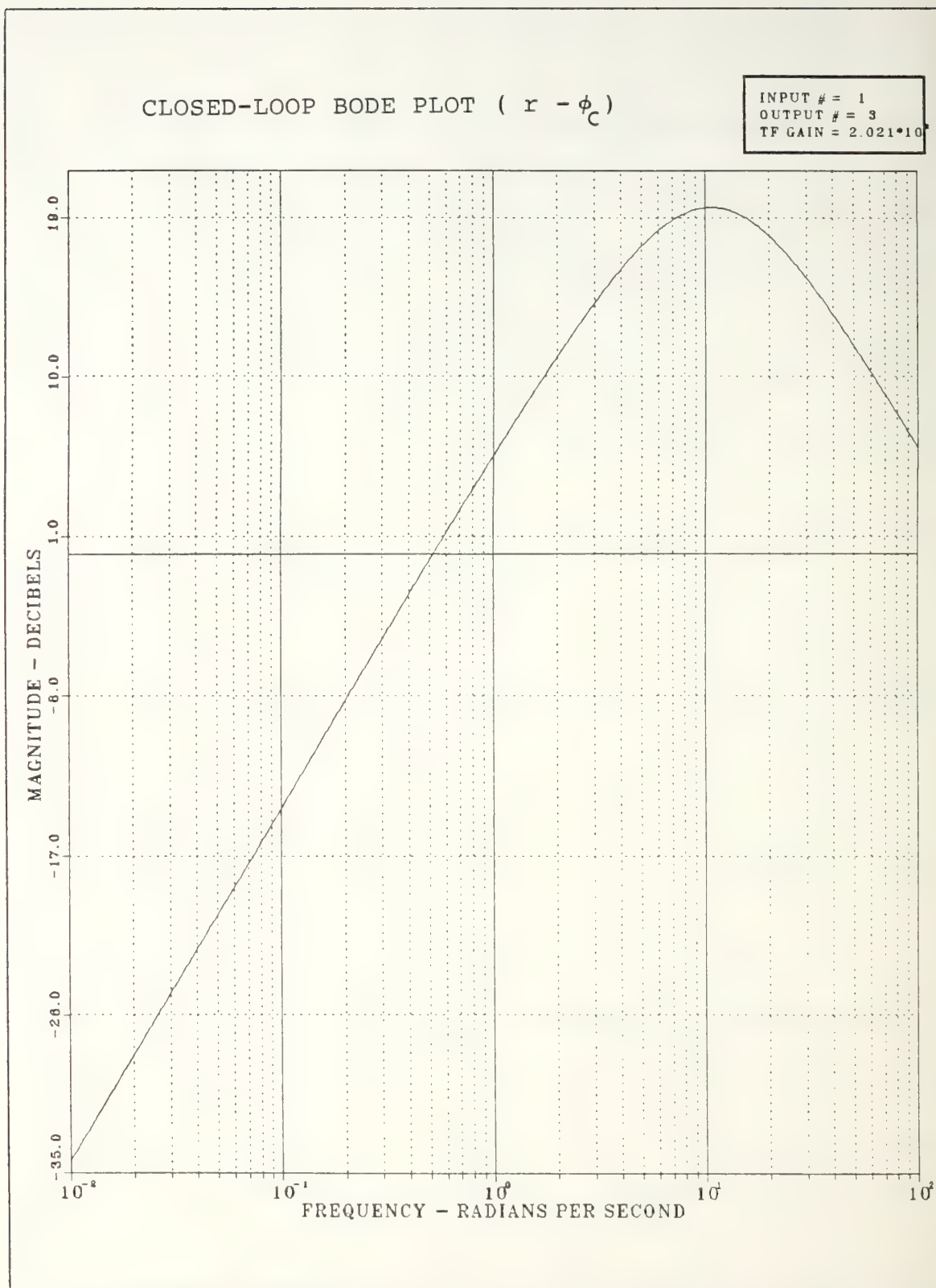


Figure 5.25 Closed-Loop Bode Plot- AlphaTech 1-3.

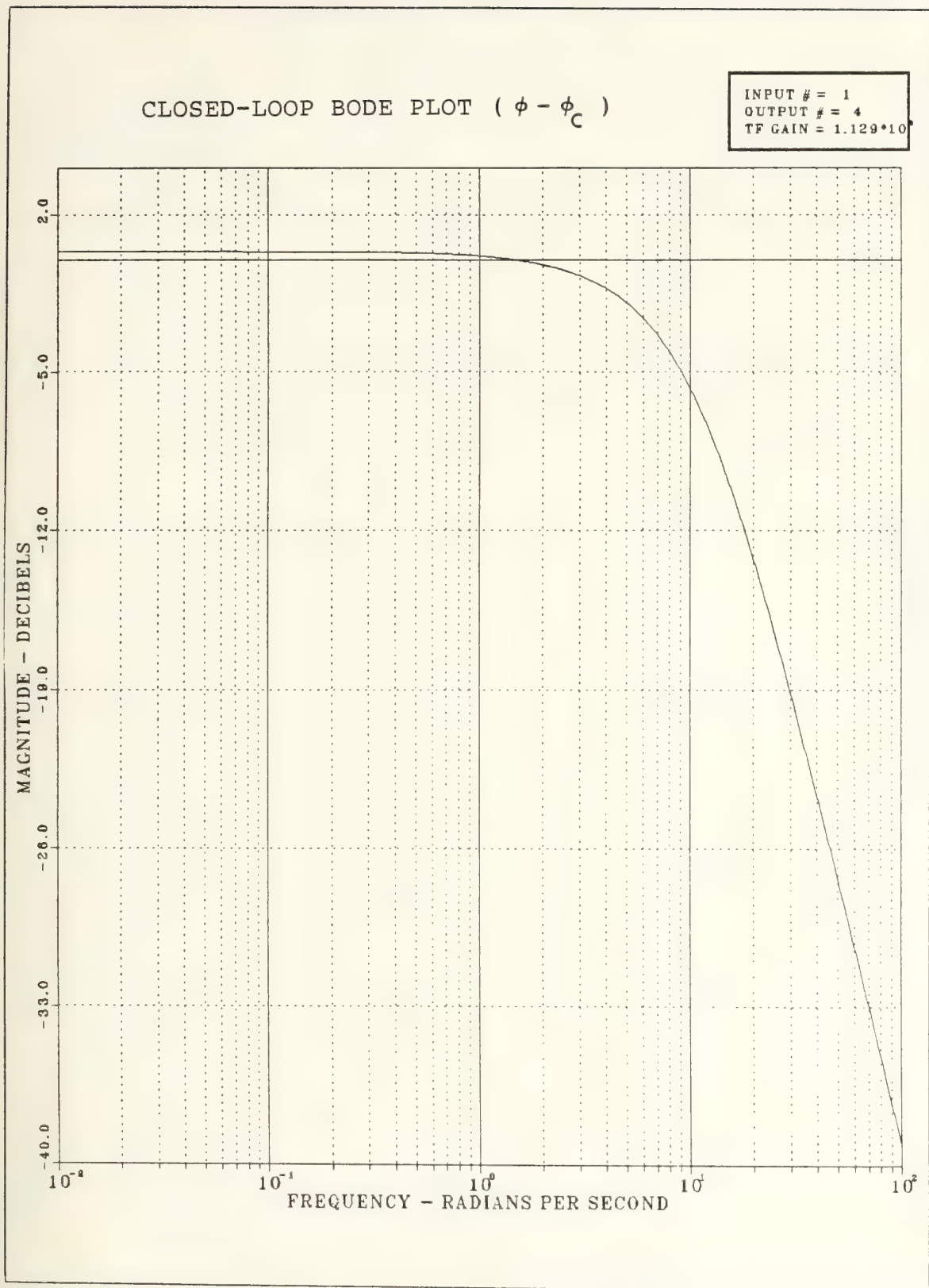


Figure 5.26 Closed-Loop Bode Plot- AlphaTech 1-4.

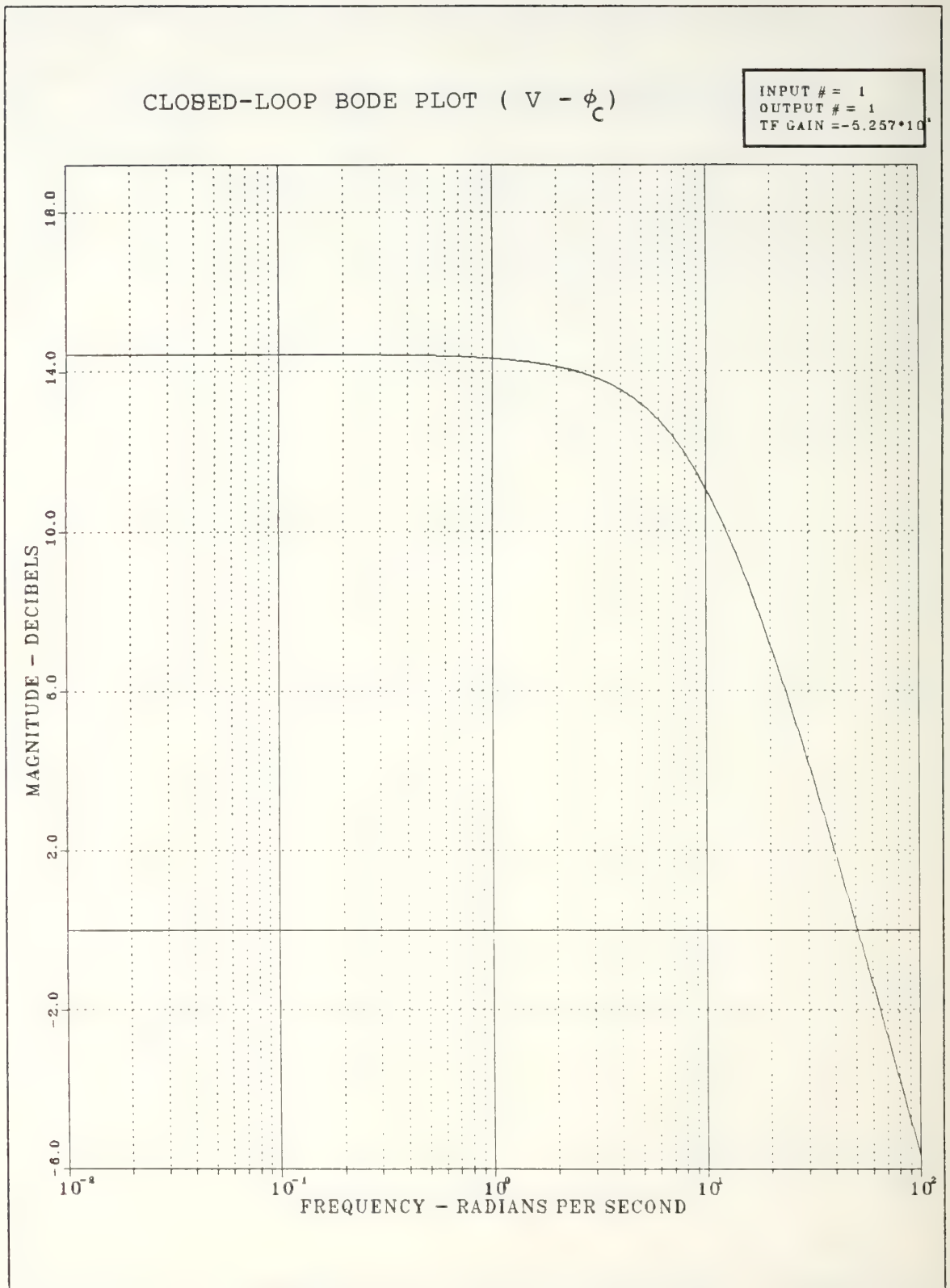


Figure 5.27 Closed-Loop Bode Plot- LQ-A 1-1.

# CLOSED-LOOP BODE PLOT ( $r - \phi_c$ )

INPUT # = 1  
OUTPUT # = 3  
TF GAIN = -1.388\*10<sup>-1</sup>

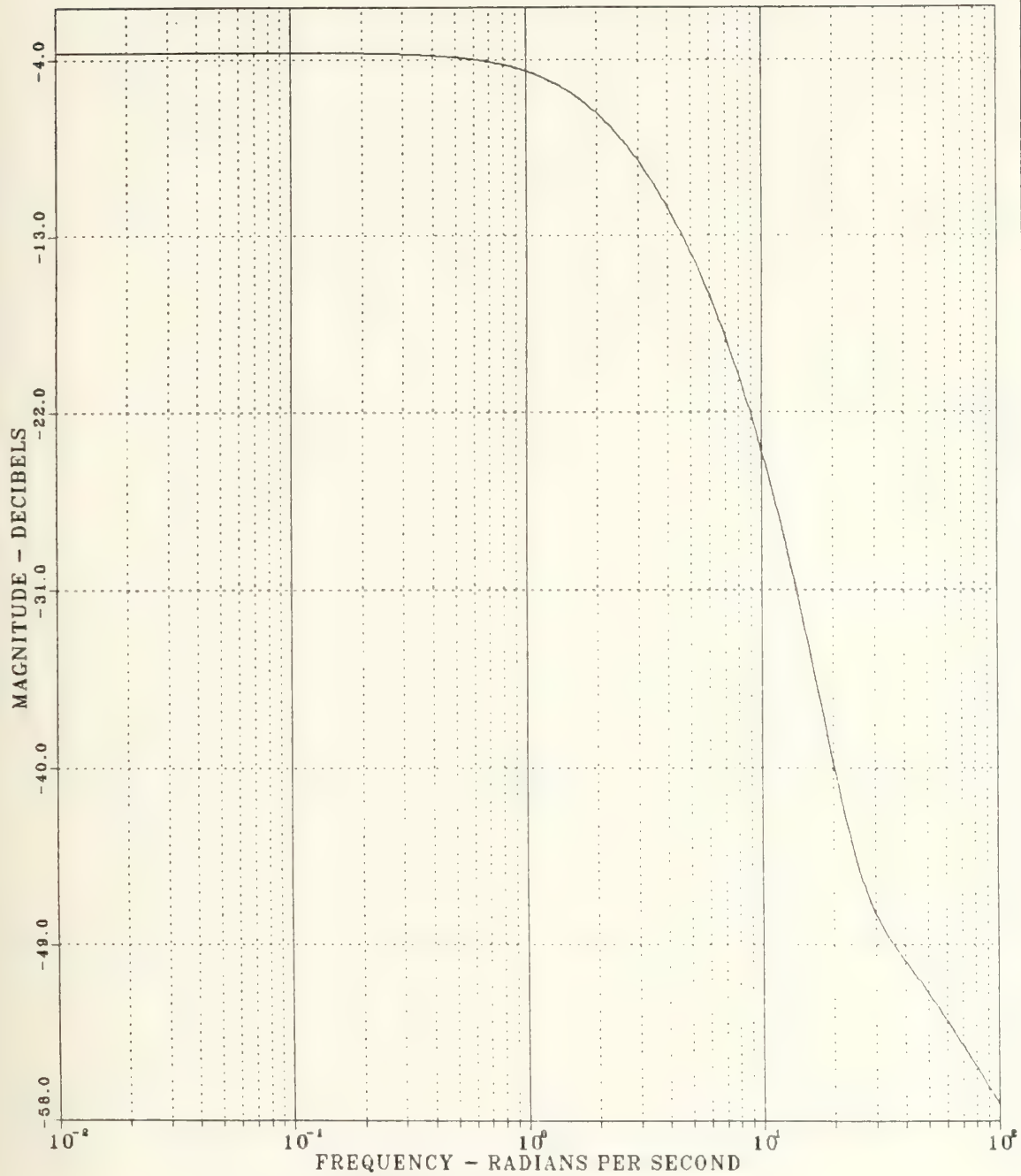


Figure 5.28 Closed-Loop Bode Plot- LQ-A 1-3.



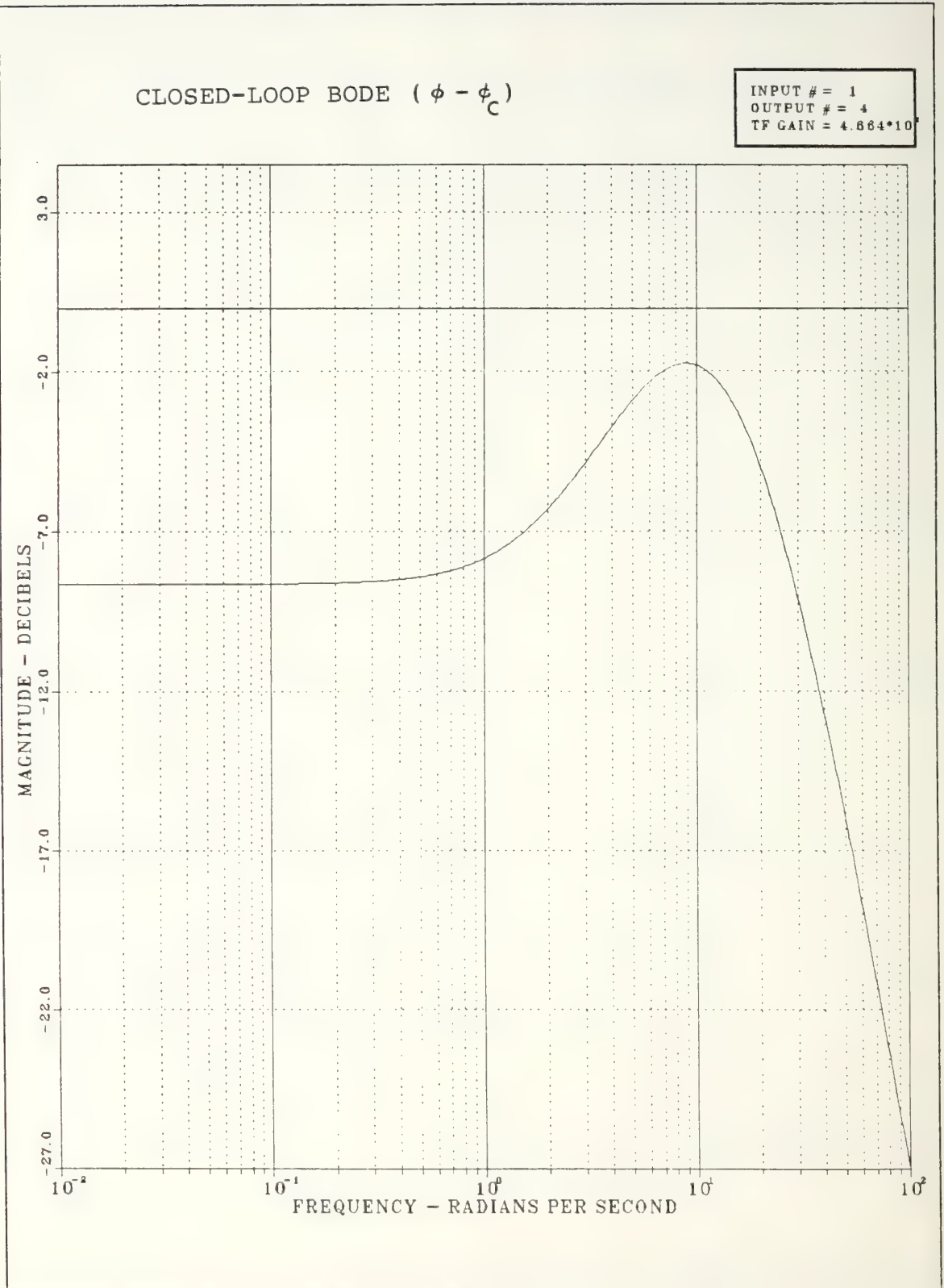


Figure 5.29 Closed-Loop Bode Plot- LQ-A 1-4.

# CLOSED-LOOP BODE PLOT ( $V - \phi_C$ )

INPUT # = 1  
 OUTPUT # = 1  
 TF GAIN =  $-2.831 \cdot 10^1$

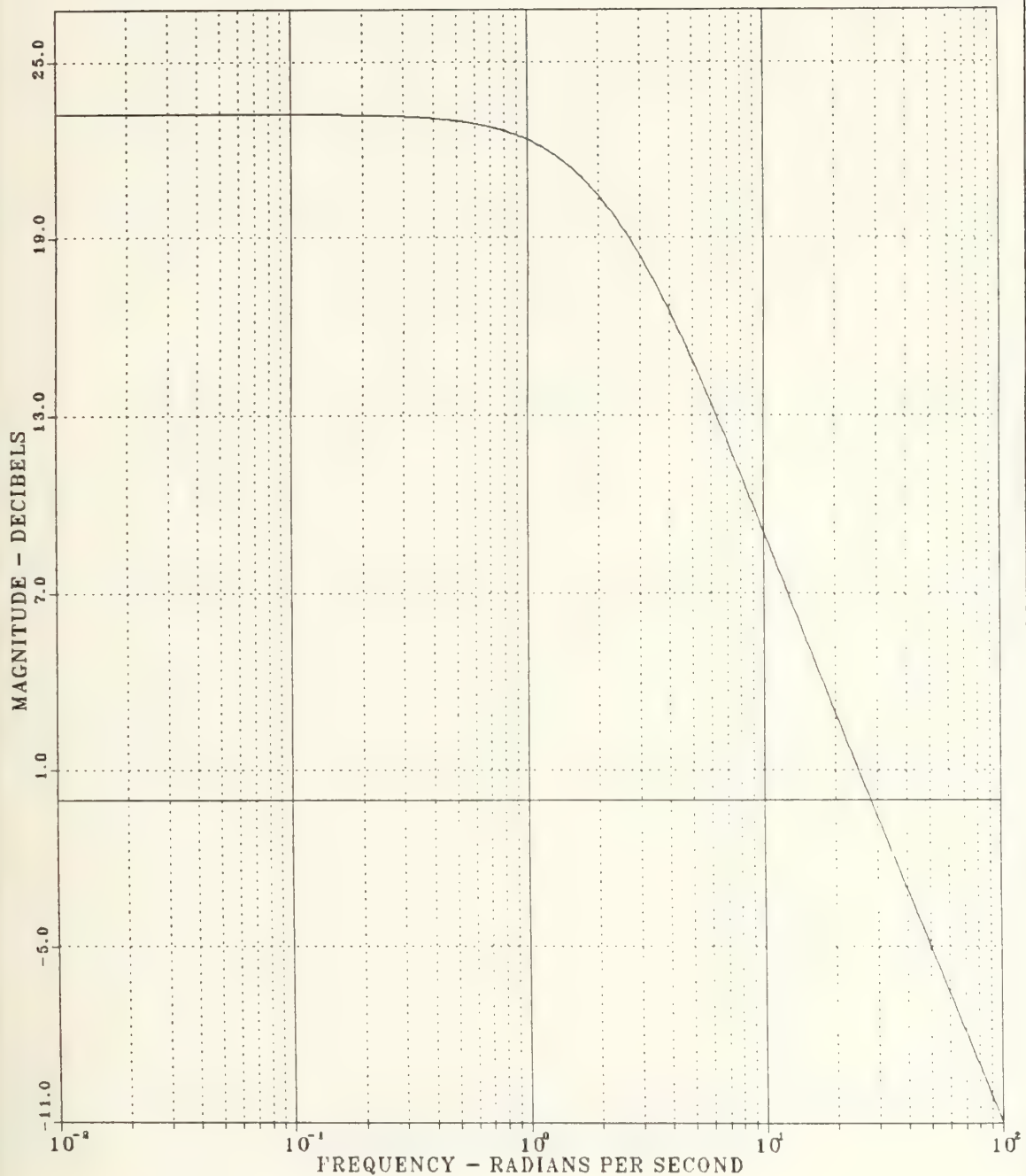


Figure 5.30 Closed-Loop Bode Plot- LQ-B 1-1.

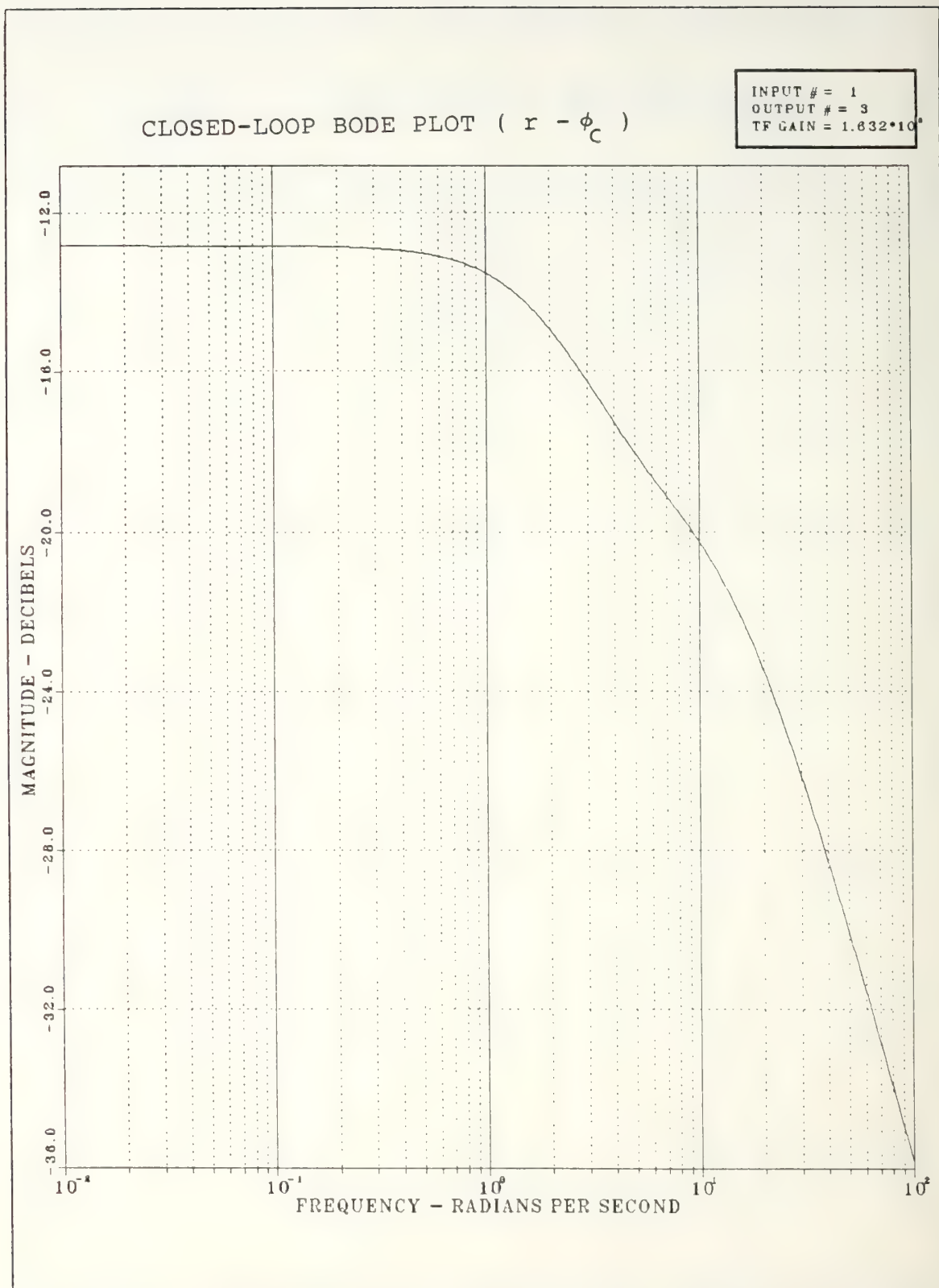


Figure 5.31 Closed-Loop Bode Plot- LQ-B 1-3.

# CLOSED-LOOP BODE PLOT ( $\phi - \phi_c$ )

INPUT # = 1  
OUTPUT # = 4  
TF GAIN =  $2.560 \cdot 10^7$

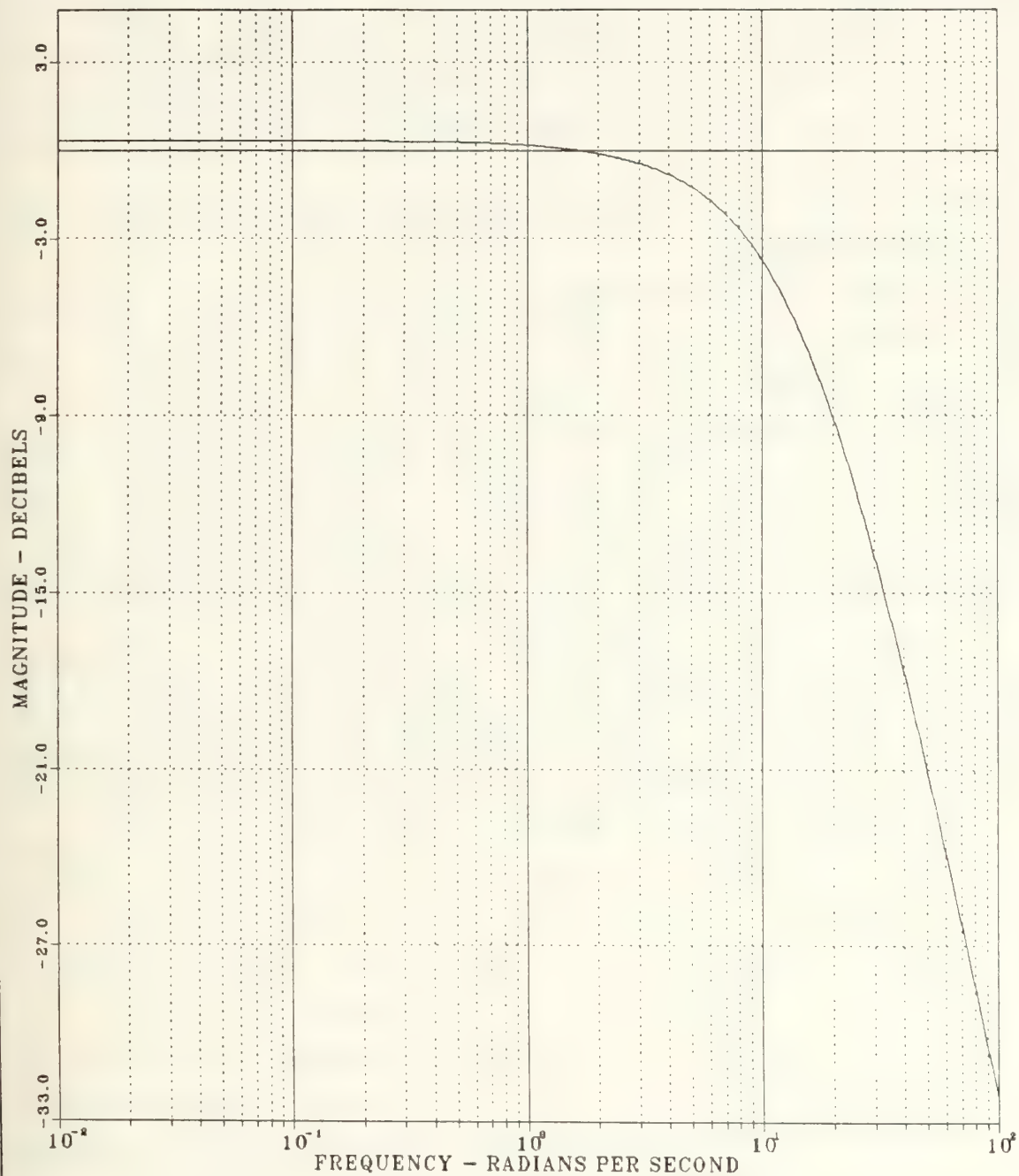


Figure 5.32 Closed-Loop Bode Plot- LQ-B 1-4.

1. It guarantees stability automatically.
2. It has partly overcome the main difficulty in applying optimal control theory to practical problems; i.e. that of selecting suitable performance indices (Q and R matrices). The designer can now choose to compute Q (if he knows something about R) or vice versa or compute both Q and R if both of them are unknown.
3. It has built-in robustness to model's error and perturbation.
4. Reduced-order type of problem formulation is possible as the procedure can reassign poles one at a time without affecting others.

On the other hand, the design procedure developed here is not without some shortcomings. Three main problem areas are described below, one of which can be overcome by additional programming efforts while the others are still active research areas pursued by many researchers.

1. Eigenvectors Assignments: It was shown in the design examples presented above that while the overall speed of response of the closed-loop system is determined by its eigenvalues, the 'shape' of the transient response depends on the closed-loop eigenvectors. The problem of eigenvectors assignments was first formulated in [Ref. 16]. Since then many eigenvectors assignment algorithms have been developed [Refs. 17,24] for use in multivariable design. In principle, the eigenvectors assignment routine can be incorporated into the coordinate transformation portion of the OPTPP program (as indicated in Figure 4.1 in Chapter 4). In essence, a new similarity transformation different from M in Equation 4.6 is computed once the eigenvalues and eigenvectors are specified. As most eigenvector algorithms available



at present are iterative in nature and their inclusion requires major programming efforts, it is recommended for future work.

2. Perturbation or Model's Error Structure: The guaranteed robustness obtained from the LQ formulation given by equations 3.4 and 3.5 ensures that the perturbation or model's error ( $L(j\omega)$ ) is sufficiently small so that the closed-loop system remains stable. However, the above only applies to simple model's error structure where both  $L(j\omega)$  and  $R$  are diagonal matrices. There may be cases when the above equations do not hold and hence the design becomes very conservative. An example of this nature is shown in [Ref. 19]. An ad hoc solution is to use non-diagonal control weighting matrix as mentioned in Chapter 4. Two designs for the helicopter problem are obtained using non-diagonal  $R$ . Their results in terms of singular value plots, Bode plots etc are compared with other designs in Appendix A
3. Reassignment Sequence: As shown in the last section, different reassignment sequences result in different designs. At present there are no known methods for determining the best reassignment sequences.

## VI. CONCLUSIONS

It was demonstrated that the general pole assignment problem in multivariable state feedback control system design can be formulated using the Linear Quadratic Control approach. This method of formulation is effective for two main reasons; First, the extra degrees of freedom available in a multivariable system structure is utilized to produce designs that are robust to perturbations in the system and gain matrices. Secondly, the classical difficulty of selecting suitable performance index in optimal control formulation was partly overcome, as designers now have the flexibility of specifying only  $Q$  (the state weighting matrix) or  $R$  (the control weighting matrix) or both  $Q$  and  $R$  as the design parameters to be varied. In other words, knowledge of the performance index which ideally should come from physical argument is used to the best of designer's advantage. In addition, the structure of the present formulation is such that eigenvector assignment can be further incorporated into the procedure. The above properties, when combined with the reduced-order formulation capability, have been shown to be very versatile and have important impact on the performance of the resulting design.

The optimal pole placement (OPTPP) program developed here is combined with other well established routines to form a computer aided design and synthesis package. Together with the design procedure and philosophy presented here, it provides the control system designer an excellent and viable tool to solve complex multivariable problems.

The procedure was applied to practical test examples, and numerical results were presented and discussed. Results indicated that all controllers obtained from the formulation

given here were stable and robust. Introducing perturbation in the system matrices leaded only to small errors in the assigned poles. The main shortcoming of the design procedure is the ad hoc nature in which the poles are reassigned. More research is required to develop a systematic way of assigning poles and its eigenvectors thus allowing the designer to optimally shape the response of the system.

## APPENDIX A

### NON-DIAGONAL R DESIGNS

The two design examples presented in Chapter 5 were based on diagonal control weighting matrix (i.e.  $R = I$ ). It is now illustrated that design using non-diagonal  $R$  will provide yet another degrees of freedom available to the designer. This type of formulation is especially useful when the model's or error structure is known. For multiplicative type of perturbation, the effect of control weighting matrix on the system stability has been explored in [Ref. 12]. In essence, the selection of the  $R$  matrix determines the coordinate frame in which the sensitivity assessment is to be made. This can be readily seen from equation 3.1, the general form in which  $R$  is non-diagonal is given below;

$$\bar{\sigma} [R^{1/2} L^{-1}(s) R^{-1/2} - I] < \underline{\sigma} [I + G(s)] \quad (\text{eqn A.1})$$

In general, the sensitivity of the system to perturbation in a particular  $L(s)$ 's direction can be reduced by making  $\bar{\sigma} [R^{1/2} L^{-1}(s) R^{-1/2} - I]$  small. This can be done simply by choosing an appropriate  $R$ . The main problem with this kind of approach is that  $L(s)$  must be known precisely for all frequency for the computation of  $\bar{\sigma} [R^{1/2} L^{-1}(s) R^{-1/2} - I]$ . In addition, the worst case direction of  $L(s)$  must be known otherwise the resulting design may be too conservative.

The helicopter problem presented in Chapter 5 is now analyzed using the non-diagonal control weighting matrix. Two designs are obtained as follows;



Design one (LQ-C):

$$R = \begin{bmatrix} 1.0 & 0.0 \\ 0.0 & 2.0 \end{bmatrix}$$

Design two (LQ-D):

$$R = \begin{bmatrix} 1.0 & 0.5 \\ 0.5 & 1.0 \end{bmatrix}$$

Design LQ-C is obtained using an assignment sequence similar to LQ-A with no off-diagonal element in R. Design LQ-D is obtained using placement sequence for design LQ-B but has off-diagonal element in R. Q and F obtained during each move and the final  $Q_e$  and  $F_e$  are tabulated in Tables VII and VIII. Singular value plots and the open-loop Bode Plots are compared with other designs in Figures A.1 to A.5

Both design has singular value greater than one for all frequency. It is interesting to note that similar reassignment sequence produce similar singular value plots. This can be readily seen by comparing LQ-A with LQ-C and LQ-B with LQ-D in the figures. The effect of using non-diagonal R merely changes the shape of the singular value plots. For the cases presented here, both non-diagonal R designs are slightly less conservative (having lower singular value).

As in the singular value plots, the shape of the open-loop Bode plots (with feedback) are closely related to the reassignment sequence. (compare Bode plots of LQ-A with LQ-C and LQ-B with LQ-D in Figures A.2 to A.5 . Results from pole-zero maps also indicate similar trends.

In summary, it is demonstrated that designs using non-diagonal control weighting matrix (including possibly off-diagonal elements) provide yet another means of 'fine



tuning' the design. This capability, such as using the off-diagonal elements directly in design, is unique to the present formulation. Robustness between the upper and lower crossfeed (of  $L(s)$ ) can be controlled by adjusting the relative weighting of the upper and lower (or off-diagonal) elements of the control weighting matrix. It must be emphasized that this kind of fine tuning is only possible for a class of rather well-defined structure of  $L$ . In practices, other constraints, such as the energy of the control input, the conditioning of  $R$  etc must be considered over the range of frequencies. The key issue of model's error structure and how it can be used in multivariable control system design is currently being investigated by many researchers.

TABLE VII  
RESULTS FROM POLE PLACEMENT SEQUENCE (LQ-C)

Move	Q and F obtained during each reassignment			
Q <sub>1</sub>	0.00062	0.10604	0.01180	0.09584
	0.10604	18.17288	2.02209	16.42484
	0.01180	2.02209	0.22500	1.82758
	0.09584	16.42485	1.82758	14.84496
F <sub>1</sub>	0.00033	0.05708	0.00635	0.05159
	-0.01773	-3.03892	-0.33814	-2.74657
Q <sub>2</sub>	4.17258	-3.78394	0.13594	-108.79945
	-3.78394	3.43150	-0.12328	98.66574
	0.13594	-0.12328	0.00443	-3.54455
	-108.79944	98.66574	-3.54455	2836.93335
F <sub>2</sub>	0.02701	-0.02449	0.00090	-0.70429
	1.21663	-1.10329	0.03967	-31.72316
Q <sub>3</sub>	154.23135	36.25874	26.52098	418.56201
	36.25874	8.52419	6.23491	98.40111
	26.52100	6.23491	4.56044	71.97421
	418.56201	98.40114	71.97421	1135.91846
F <sub>3</sub>	2.80842	0.66025	0.48291	7.62180
	-7.58133	-1.78234	-1.30355	-20.57501
Q <sub>4</sub>	0.44288	0.09189	-4.22665	0.82784
	0.09189	0.01906	-0.87692	0.17176
	-4.22665	-0.87692	40.33727	-7.90052
	0.82784	0.17176	-7.90052	1.54741
F <sub>4</sub>	-0.63449	-0.13165	6.05549	-1.18605
	-0.09950	-0.02064	0.94961	-0.18599
F <sub>e</sub>	2.20127	0.56119	6.54565	5.78305
	-6.48193	-5.94519	-0.65241	-55.23073
Q <sub>e</sub>	158.84741	32.67273	22.44206	310.68604
	32.67273	30.14761	7.25680	213.66344
	22.44208	7.25680	45.12712	62.35670
	310.68604	213.66348	62.35670	3989.24390

$$u(t) = -Fx(t) + h\phi_c(t), \quad h = \begin{bmatrix} 5.7839 \\ -55.23 \end{bmatrix}$$

TABLE VIII  
RESULTS FROM POLE PLACEMENT SEQUENCE (LQ-D)

Move	Q and F obtained during each reassignment			
$Q_1$	0.00023	0.03940	0.00438	0.03561
	0.03940	6.75195	0.75129	6.10249
	0.00438	0.75129	0.08360	0.67902
	0.03561	6.10249	0.67902	5.51550
$F_1$	0.00895	1.53374	0.17065	1.38619
	-0.01765	-3.02506	-0.33659	-2.73405
$Q_2$	0.24621	0.11866	14.98355	9.73271
	0.11866	0.05719	7.22105	4.69050
	14.98355	7.22105	911.83813	592.29370
	9.73272	4.69050	592.29370	384.73022
$F_2$	0.56910	0.27424	34.63293	22.49620
	-0.32115	-0.15476	-19.54404	-12.69504
$Q_3$	0.17288	-0.43406	7.14036	-7.87012
	-0.43406	1.08987	-17.92834	19.76067
	7.14036	-17.92834	294.92139	-325.06299
	-7.87012	19.76067	-325.06299	358.28516
$F_3$	0.05761	-0.14465	2.37951	-2.62273
	0.34047	-0.85487	14.06264	-15.49990
$F_e$	0.63566	1.66333	37.18307	21.25964
	0.00167	-4.03469	-5.81798	-30.92899
$Q_e$	0.41932	-0.27600	22.12828	1.89820
	-0.27600	7.89901	-9.95601	30.55365
	22.12828	-9.95601	1206.84302	267.90967
	1.89821	30.55365	267.90967	748.53076

$$u(t) = -F x(t) + h \phi_C(t), \quad h = \begin{bmatrix} 21.159 \\ -30.9289 \end{bmatrix}$$

# SINGULAR VALUE PLOT

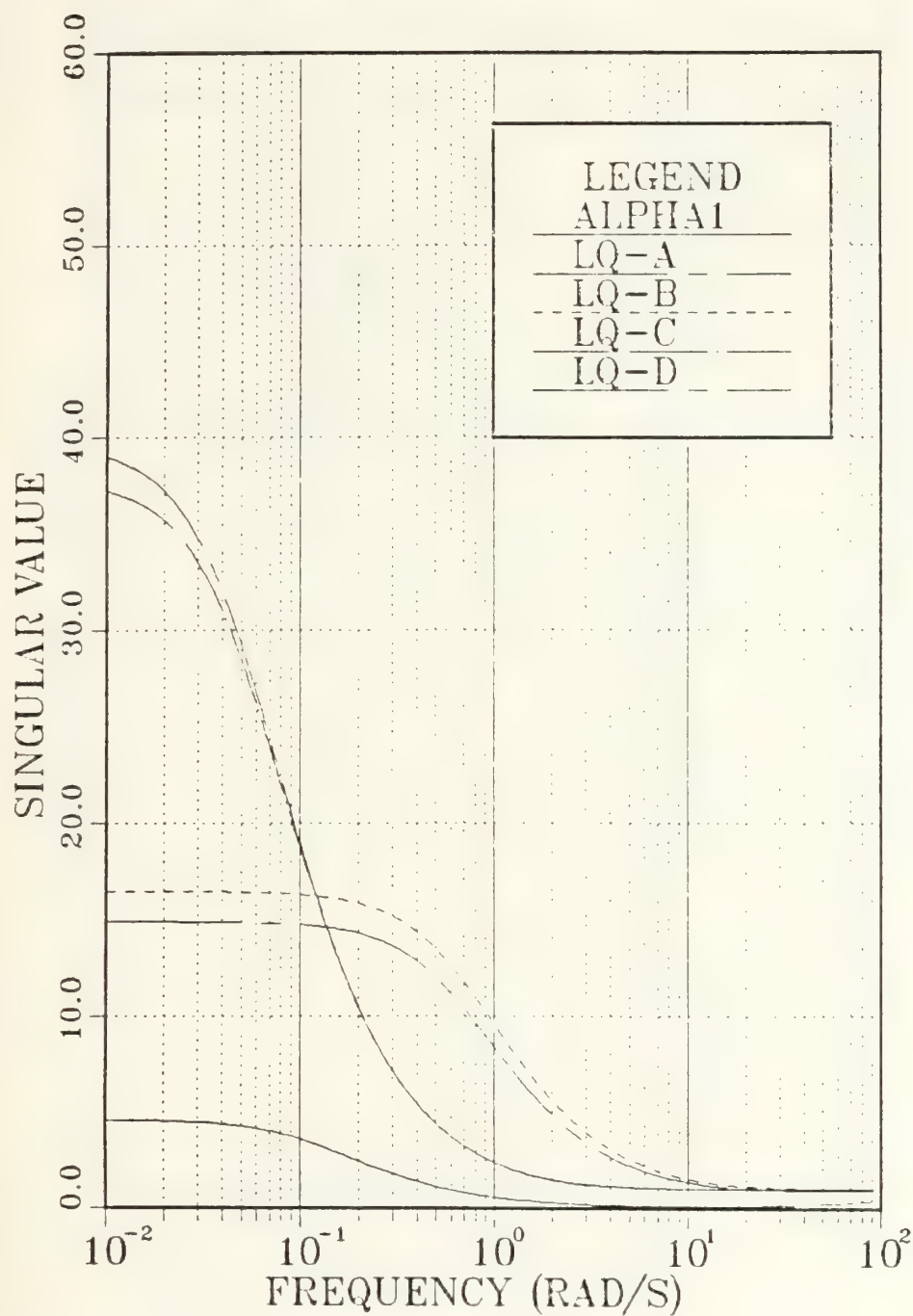


Figure A.1 Singular Value Plots - Comparison.

# OPEN LOOP GAIN 1 - 1

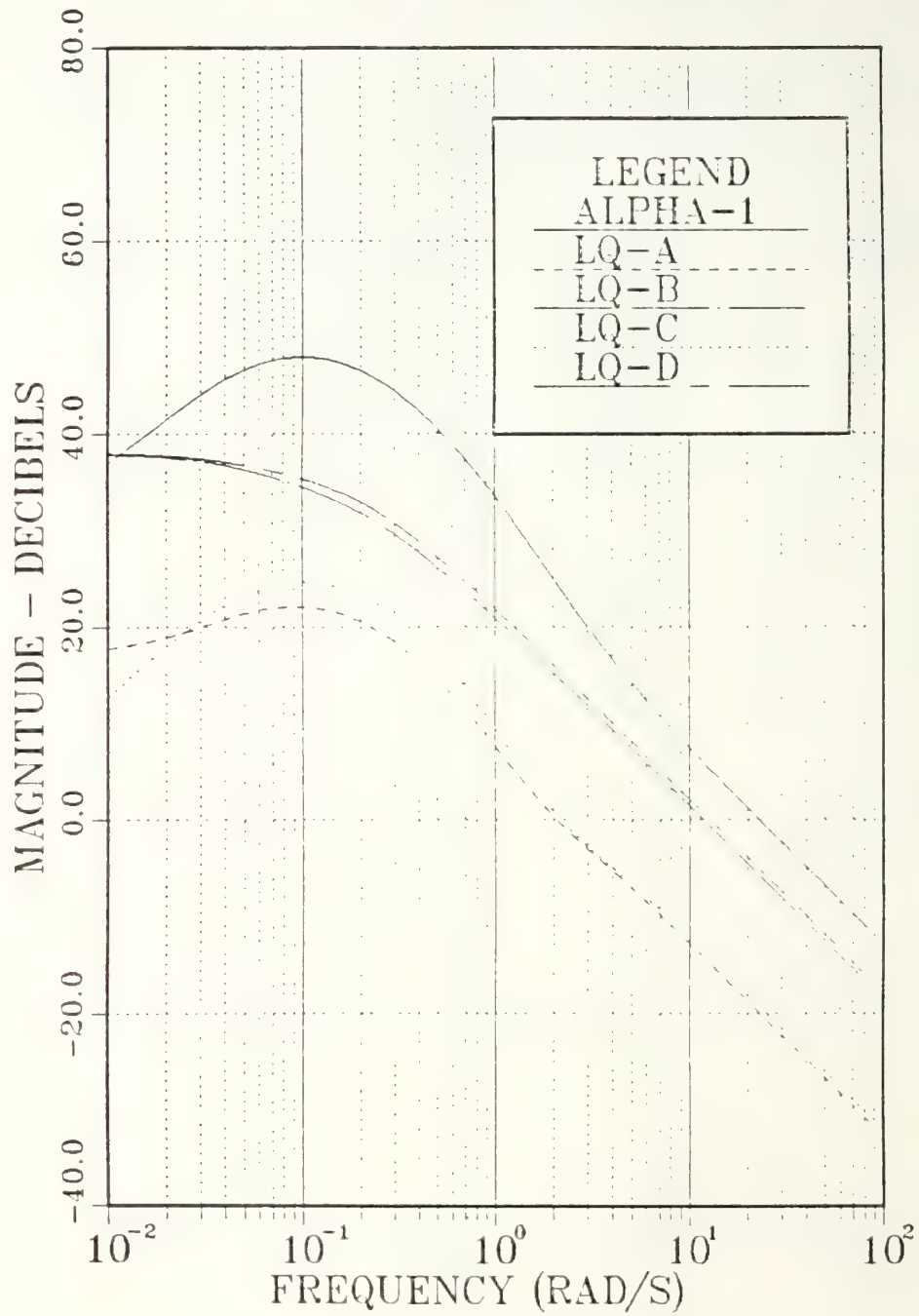


Figure A.2 Bode Plots Comparison- Input 1-1.



# OPEN LOOP GAIN 1-2

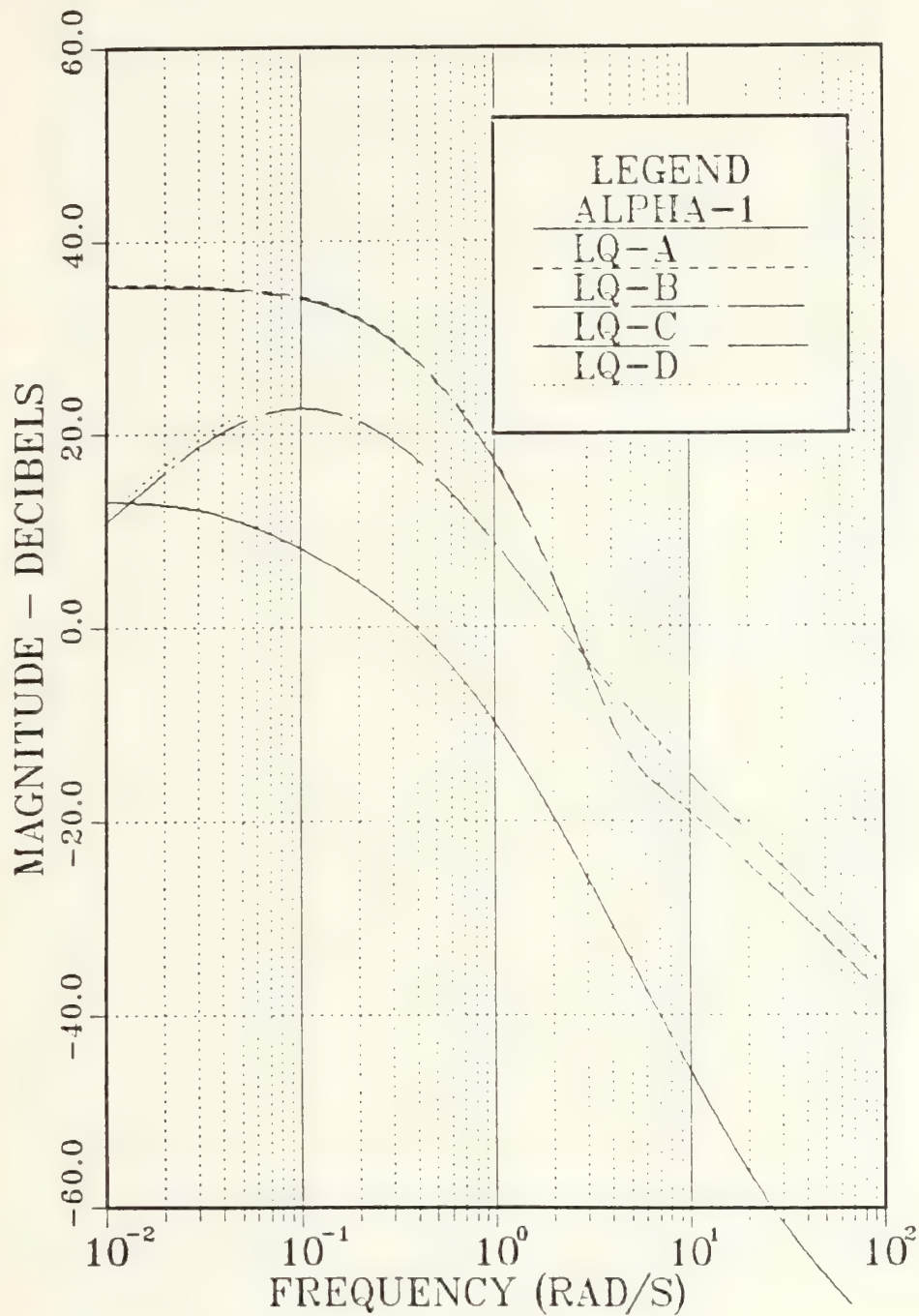


Figure A.3 Bode Plots Comparison - Input 1-2.

# OPEN LOOP GAIN 2-1

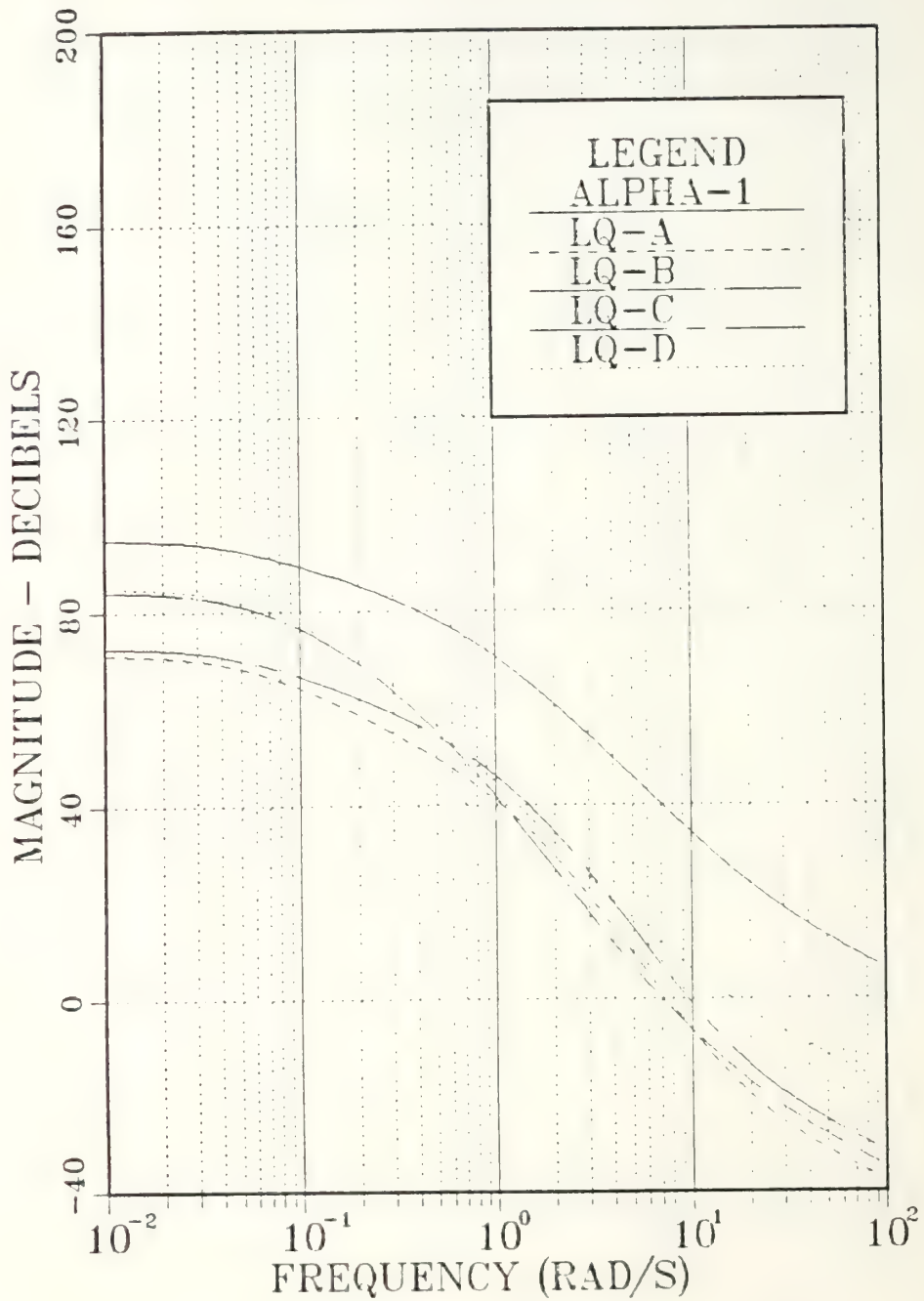


Figure A.4 Bode Plots Comparison - Input 2-1.

# OPEN LOOP GAIN 2-2

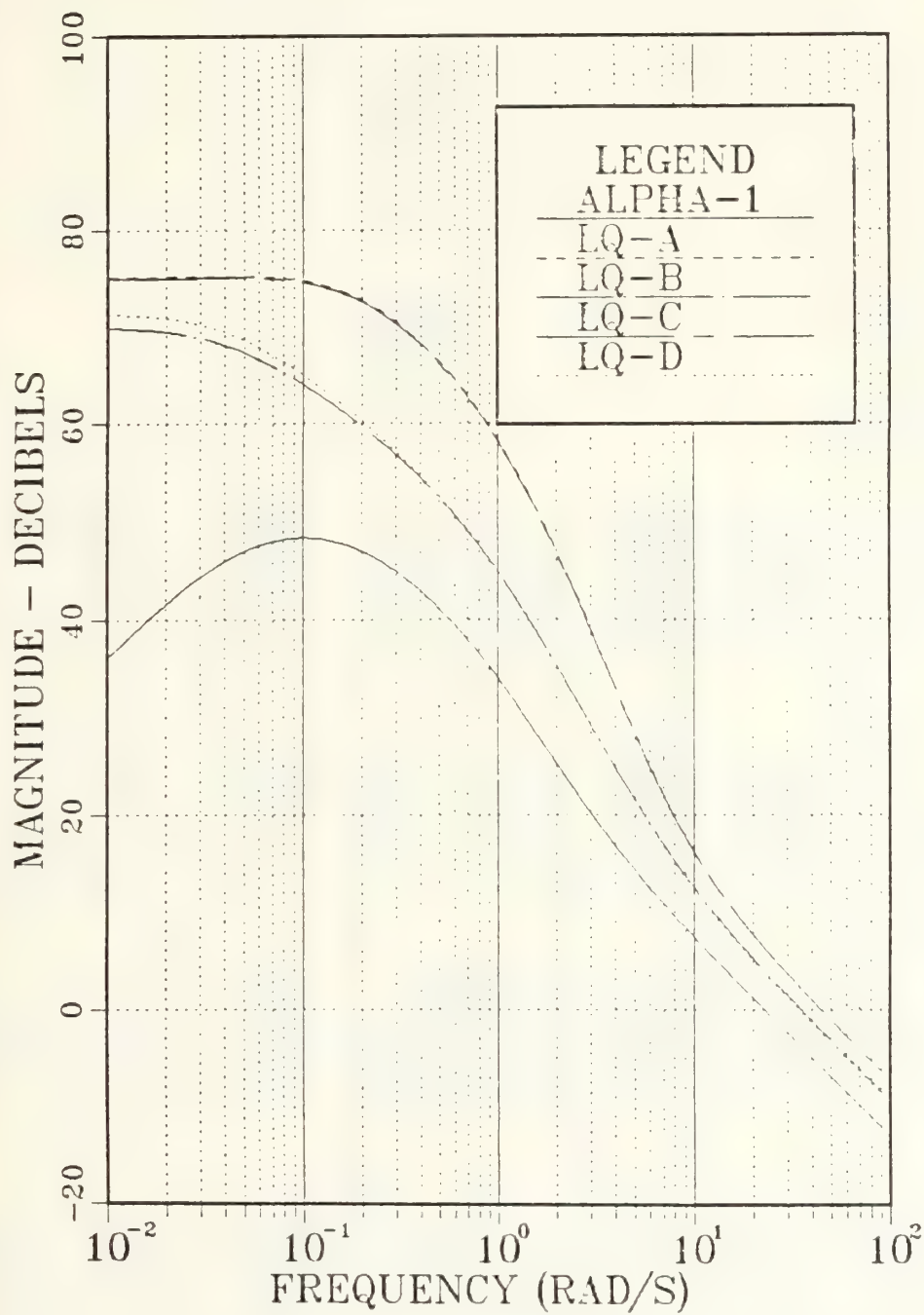


Figure A.5 Bode Plots Comparison - Input 2-2.

## APPENDIX B : EXAMPLE DESIGN RUN OUTPUTS

```

** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** 
THIS EXAMPLE DEMONSTRATES THE POLE REASSIGNMENT WHERE THE OPEN
LOOP POLE AT -2.126 IS MOVED TO ITS NEW LOCATION AT -25.21
(64, 4) IS THE DESIGN VARIABLE, NOTE THAT THE UNSTABLE POLES
0.2005 IS AUTOMATICALLY MOVED TO ITS MIRROR IMAGE DUE TO LQ
FORMULATION.
** ** ** ** 

```

```

KONTROL      0
*** THE A PLANT MATRIX ***
-2.27000      1.42000      -0.15000      31.99001
 0.04000     -0.70000     -0.07000      C.00000
 0.04000     -0.05000     -0.05000      C.00000
 0.00000      1.00000      0.10000      C.00000

```

```
*** THE B CONTROL INPUT MATRIX ***
```

6.12000	6.95000
0.04000	-8.37000
0.34000	0.02000
0.00000	0.00000

THE STARTING Q WEIGHTING MATRIX

0	0	0	0
0	0	0	0
0	0	0	0
0	0	0	0

THE DESIGN VARIABLE(G) X

0000

0000

0000

0000

\*\*\* THE R WEIGHTING MATRIX \*\*\*

1.00000	0.00000
1.00000	1.00000
1.00000	0.00000

\*\*\* THE STARTING/FINAL F MATRIX \*\*\*

-14.78000	2.16000	77.97000	-55.30000
-0.00567	-2.55600	0.39400	-15.05000

\*\*\* THE ORDERED COMPLEX EIGENVALUES (INPUT)

-25.21001 C.00000

```

** ICOMP **
0

```

\*\*\*AUX TRANSFORMATION L\*\*\*

Figure 1 shows a 4x4 grid of circles. The top row has 4 circles. The second row has 4 circles with a dot in the center. The third row has 4 circles with a dot in the center. The bottom row has 4 circles. The circles are arranged in a square pattern.

\* \* \*  
EIGENVECTOR OF A  
\* \* \*

0.14268	0.98509	0.99767
0.10820	-	-0.03687
-0.98384	0.15380	-0.04176
0.00049	0.07703	0.03949

\*\*\* TRANSFORMED A MATRIX

-0.05030	6.00000	0.00000
0.00000	0.20653	0.00000
0.00000	-0.00001	-1.04987
0.00008	0.00001	0.00002

\*\*\*  
TRANSFORMED  
C-MATRIX

[illegible]

TRANSFORMED C. MATRIX

-0.15647  
 -0.85855  
 -1.80459  
 -1.09721

I.O.#121 BRNT INVERSE  
\*\*SQUARE \*\*  
\*\*95.72333 \*\*  
\*\*OF R \*\*

SQUARE	KLUI	INVERSE
1.00000	0.00000	0.00000
0.00000	1.00000	1.00000

The four 4x4 grids are as follows:

- Grid 1:**
  - Row 1: All circles are empty.
  - Row 2: All circles are empty.
  - Row 3: All circles are empty.
  - Row 4: All circles are empty.
- Grid 2:**
  - Row 1: All circles are empty.
  - Row 2: All circles are empty.
  - Row 3: All circles are empty.
  - Row 4: All circles are empty.
- Grid 3:**
  - Row 1: All circles are empty.
  - Row 2: All circles are empty.
  - Row 3: All circles are empty.
  - Row 4: All circles are empty.
- Grid 4:**
  - Row 1: All circles are empty.
  - Row 2: All circles are empty.
  - Row 3: All circles are empty.
  - Row 4: All circles are empty.

○○○○  
●●●●  
○○○○



```

AAAAA DDDDD SSSSS
A  D  D  S
A  D  D  S
AAAAAA D  SSSSS
A  D  D  S
A  D  D  S
A  DDDDD SSSSS
A

```

F O R T R A N   P R O G R A M  
 F O R  
 A U T O M A T E D   D E S I G N   S Y N T H E S I S  
 V E R S I O N 1.00

```

CONTROL PARAMETERS      =      IONED =      IPRINT = 1000
ISTRAT = 5             =      NCCN  =      2
IGRAD  = 0             =      NDV   =

```

1

-----  
 OPTIMIZATION RESULTS  
 -----

```

OBJECTIVE FUNCTION VALUE      0.56055E-13

DESIGN VARIABLES
VARIABLE      LOWER      VALUE      UPPER
              BOUND
1      0.0000E+00      0.68858E-01      0.10000E+05

```

```

DESIGN CCNSTRANTS
1) -0.5000E-01 -0.9000E+00
FUNCTION EVALUATIONS =      41

```

\*\*\* THE OPTIMAL Q MATRIX

0.00000	0.00000	0.00000	0.00000
0.00000	0.00000	0.00000	0.00000
0.00000	0.00000	0.00000	0.00000
0.00000	0.00000	0.00000	0.06886

END OF POLE PLACEMENT ROUTINE

THE Q REQUIRED FOR THIS ASSIGNMENT IS

0.10027	0.96194	0.11959	-1.50849
0.96194	9.22847	1.14725	-14.47182
0.11959	1.14725	0.14262	-1.79908
-1.50849	-14.47182	-1.79908	22.69429

EIGENSYSTEM OF OPTIMAL REGULATOR.....

C-LOOP OPTIMAL REG. E-VALUES...DET(SI-F+G\*C)..

-2.52094E+01:-1.04978E+00:-2.06591E-01:-5.02113E-02:

CONTROL EIGENVECTOR MATRIX.....C\*M..

-3.326553E-C2	1.117587E-08	-6.642234E-04	-4.134316E-06
2.902164E+00	-1.370907E-06	-2.356589E-03	-5.652895E-06

\*\*\* THE STARTING/FINAL F MATRIX \*\*\*

0.00387	0.03151	0.00399	-0.06416
-0.24260	-2.83522	-0.34541	3.11642

\*\*\* THE AUGMENTED A-B\*F\*C MATRIX \*\*\*

-2.03999	4.10968	0.17766	29.03711
-2.02074	-24.43202	-2.96126	26.08698
0.04354	-0.00401	-0.04445	-0.04051
0.00000	1.00000	0.11000	0.00000

END OF CPTP ANALYSIS





\*\*\* THE R WEIGHTING MATRIX \*\*\*

2.00000	2.00000
0.00000	0.00000
7.00000	7.00000
9.00000	9.00000

\*\*\* THE STARTING/FINAL F MATRIX \*\*\*

[illegible]

\*\*\* THE ORDERED COMPLEX EIGENVALUES (INPUT)

-0.70000 1.42000

并并并 ICOMP 并并

1

\*\*\*AUX TRANSFORMATION L\*\*\*

[illegible]

CONFIDENTIAL

-0.13554	-0.13554	0.67738
0.14603	0.14603	-0.47971
-0.01263	-0.01263	-0.00119
0.00453	0.00453	-0.00865

# TRANSFORMED A MATRIX

-0.39354	-1.42648	-0.00001	0.00000
1.42646	-0.39355	0.00000	0.00000
0.00000	0.00001	0.13768	0.00000
0.00000	-0.00001	0.00000	-0.18058

TRANSFORMED Q MATRIX \*\*\*

\*\*\* TRANSFORMED B MATRIX \*\*\*

-24.68213  
 -1.52755  
 -11.17529  
 -1.63321  
 -1.65275  
 -1.02616  
 -1.73118  
 -1.99311

\*\*\*\*\*SQUAPE RCOT INVERSE OF R\*\*\*

0.70711  
0.00000  
0.00000  
0.37796

[illegible]

0000  
.  
0001



```

AAAAA DDDDD SSSSS
A A D D S
A A D D S
AAAAA D D SSSSS
A A D D S
A A D D S
A A D D SSSSS

```

F O R T R A N P R O G R A M  
 F O R  
 A U T O M A T E D D E S I G N S Y N T H E S I S  
 V E R S I O N 1.00

```

CONTROL PARAMETERS
ISTRAT = 5 IOPT = 3 IONED = 3 IPRINT = 1000
IGRAD = 0 NDV = 2 NCCN = 3

```

-----  
 OPTIMIZATION RESULTS  
 -----

OBJECTIVE FUNCTION VALUE 0.28365E-10

DESIGN VARIABLES

VARIABLE	LOWER BOUND	VALUE	UPPER BOUND
1	0.00000E+00	0.23088E-02	0.10000E+04
2	0.00000E+00	0.22134E-02	0.10000E+04

DESIGN CCNSTRANTS

1) -C.4999E-01 -C.9000E+00 0.9545E-04

FUNCTION EVALUATIONS = 48

```

*** THE OPTIMAL Q MATRIX
      0.00231      C.00000      0.00000      C.00000
      0.00000      C.00221      0.00000      C.00000
      0.00000      C.00000      0.00000      C.00000
      0.00000      C.00000      0.00000      C.00000

END OF POLE PLACEMENT ROUTINE

THE Q REQUIRED FOR THIS ASSIGNMENT IS
      0.00060      0.00106      -0.00908      C.00301
      0.00106      0.00189      -0.01970      0.00579
      -0.00908      -0.01970      12.94063      -1.60992
      0.00301      0.00579      -1.60992      0.20628

EIGENSYSTEM OF OPTIMAL REGULATOR.....

C-LOOP CFTIMAL REG. E-VALUES...DET(SI-F+G*C)..

-6.99887E-01, 1.41996E+00:-1.80579E-01:-1.37682E-01:

CONTROL EIGENVECTOR MATRIX.....C*M..

4.996814E-03 -2.528824E-02 -6.565824E-08 -5.181365E-03
2.956046E-04 -4.560151E-04 -3.259629E-09 -1.896438E-04

*** THE STARTING/FINAL F MATRIX ***
      -0.01311      -0.02106      2.67146      2.79805
      -0.00052      -0.00084      0.06034      C.09177

*** THE AUGMENTED A-B*F*C MATRIX ***
      -0.18440      -0.03706      10.48966      -30.92160
      -0.20052      -0.55084      109.49033      2.87177
      -0.00566      -0.01073      -0.98285      -0.92528
      0.00000      0.00000      1.00000      C.00000

END OF CPTPP ANALYSIS

```



# APPENDIX C : COMPUTER PROGRAM LISTINGS

```

*** CPTPP --- OPTIMAL POLE PLACEMENT PROGRAM***
THIS PROGRAM IS DESIGNED TO COMPUTE THE STATE WEIGHTING MATRIX
OF A MIMO OPTIMAL CONTROL PROBLEM GIVEN THE DESIRED CLOSED-LOOP
POLES LOCATIONS. THE DESIGNER HAS THE CHOICE OF ASSIGNING ONE
OR MORE PCLES DURING ONE RUN. ON COMPLETION OF POLE ASSIGNMENT,
A MODIFIED VERSION OF THE OPTSYS ROUTINE IS CALLED TO COMPUTE
THE FEEDBACK GAIN MATRIX. SINGULAR VALUE PLOTS ARE THEN COMPUTED
TO DETERMINE THE SYSTEM ROBUSTNESS.

THE PROGRAM CAN BE MODIFIED TO COMPUTE THE CONTROL WEIGHTING MATRIX
OR BOTH THE STATE AND CONTROL WEIGHTING MATRIX IF BOTH OF THEM ARE
UNKNOWN.

THE EIGENVECTOR TYPE OF ASSIGNMENT CAN BE INCORPORATED IF REQUIRED
BY CHOICE. REPUBLIC OF SINGAPORE
VERSION 1.0 SEPT 1985

*** THIS FIRST BLOCK SETS DIMENSIONS AND DECLARES REAL AND
COMPLEX FUNCTIONS. THE FOLLOWING IS A LIST OF PROGRAM SYMBOLS:
***
REAL VARIABLES BY NAME AND BRIEF DESCRIPTION
THE SYSTEM UNDER CONSIDERATION IS GIVEN AS:
XDOT = A*X + B*U ; Y = C*X, FOR STATE FEEDBACK OR
OUTPUT FEEDBACK OF THE FORM, U = -FX + R OR U = -FY + R
A - THE PLANT A MATRIX (NSTATE X NSTATE)
B - THE CONTROL MATRIX (NSTATE X NCONTROL)
C - THE PLANT OBSERV. OR OUTPUT MATRIX (NOUTPUT X NSTATE;
FOR STATE FEEDBACK PROBLEMS)
F - THE FEEDBACK GAIN MATRIX (NCONTROL X NSTATE;
FOR STATE FEEDBACK PROBLEMS)
QW - THE STATE WEIGHTING MATRIX (INPUT/OUTPUT)
RW - THE STATE FEEDBACK PROBLEM (INPUT)
MU - THE CONTROL WEIGHTING MATRIX (INPUT)
REALMU - THE DESIRED CLOSED-LOOP POLES LOCATION
IMAGMU - THE REAL PART OF THE DESIRED POLE LOCATION
FC - F*C
BFC - B*F*C
AMBFC - A - B*F*C

CONOC100
CONOC110
CONOC120
CONOC130
CONOC140
CONOC150
CONOC160
CONOC170
CONOC200
CONOC210
CONOC220
CONOC230
CONOC240
CONOC250
CONOC260
CONOC270
CONOC280
CONOC290
CONOC300
CONOC310
CONOC320
CONOC330
CONOC340
CONOC350
CONOC360
CONOC370
CONOC380
CONOC390
CONOC400
CONOC410
CONOC420

```



```

**-----REIG - REAL COMPUTED EIGENVALUE OF THE SYSTEM-----**
**THE FOLLOWINGS ARE USED BY THE SINGULAR VALUE ANALYSIS MODE**
**-----**
OMEGA - FREQUENCY
SV - SINGULAR VALUE OF (I + F * PLANT TRANSFER FUNCTION(G))
SVM1 - SINGULAR VALUE OF (I + INV(F * G))
SVAC - SINGULAR VALUE OF (I + G * F)
SVMC - SINGULAR VALUE CF (I + INV(G * F))
SIGNM1 - ONLY OF INTEREST IF NO. OUTPUTS = NO. INPUTS.
SIGNM2 - FIRST SINGULAR VALUE CF (I + F * G)
SIGNMX - SECOND SINGULAR VALUE OF (I + F * G)
SIGPRG - MAXIMUM SINGULAR VAL * SECOND SING VAL (I + G * F)
SVACMX - SQR(T(FIRST SING VAL * SINGULAR VALUE (I + G * F)
SVACXD - MIN ADDITIVE OUTPUT SINGULAR VALUE
SVMIM - MIN MULTIPLICATIVE INPUT SINGULAR VALUE (I + INV(FG))
SVMIX - MIN MULTIPLICATIVE INPUT SINGULAR VALUE
SVMMC - MIN MULTIPLICATIVE OUTPUT SINGULAR VALUE (I + INV(GF))
SVMXD - MIN MULTIPLICATIVE CUTPUT SINGULAR VALUE
**-----**
IMPLICIT REAL*4(A-H,O-Z)
REAL*4 A(10,10),B(10,10),C(10,10),REALMU(50),IMAGMU(50),
1F(10,10),FC(10,10),BFCC(10,10),WK(1000),MEIG(10),
2REIG(50),IEIG(50),SV(10),W(10,10),WA(100),MINEIG(500),
3OMEGA(500),SIGNM1(500),SIGNM2(500),SIGNMX(500),SIGPRD(500),
4SVACMD(500),SVACXD(500),SVMIM(500),SVMIX(500),
5LPL1(500),LPL2(500),LP21(500),LP22(500),
6QW(10,10),RWSQ(10,10),RWSPI(10,10),RCOND,Z1(10),
**-----**
THE COMPLEX PARAMETERS USED IN THE PROGRAM
AX - COMPLEX A
BX - COMPLEX B
CX - COMPLEX C
CFX - COMPLEX F
QWX - COMPLEX OF QW
RWX - COMPLEX OF RW
RWSQX - COMPLEX OF R**(-1/2)
**-----**
**THE FOLLOWINGS ARE USED IN THE COORDINATE TRANSFORMATION BLOCK**
**-----**
Z - EIGENVECTOR OF A ( M IN THE THESIS )

```

CON0C430

CON0C470  
 CON0C480  
 CON0C490  
 CON0C500  
 CON0C510  
 CON0C520  
 CON0C530  
 CON0C540  
 CON0C550  
 CON0C560  
 CON0C570  
 CON0C580  
 CON0C590  
 CON0C600  
 CON0C610  
 CON0C620  
 CON0C630  
 CON0C640

CON0C650  
 CON0C660  
 CON0C670  
 CON0C680  
 CON0C690  
 CON0C700

CON0C720  
 CON0C730  
 CON0C740  
 CON0C750  
 CON0C760  
 CON0C770

CON0C790

CCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCC

CCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCC



```

** ** ** ** ** ** ** **  CZI - INVERSE OF Z                       CON0C780
** ** ** **  CZTI- INVERSE OF TRANPOSE OF Z      CONCC600
** ** ** **  LXI - AUX TRANSFORMATION MATRIX FOR COMPLEX EIGENVALUE  CON0CE10
** ** ** **  LXI - INVERSE OF LX                  CN0CC820
** ** ** **  ZLI - INVERSE GF (Z*LX)              CN000830
** ** ** **  -----THE FOLLOWINGS ARE USED TO COMPUTE THE OBJECTIVE FUNCTION-----  CON0CE40
** ** ** **  GPS - COMPLEX MATRIX COMPUTE BY PLANT1 G(S)            CON0CE50
** ** ** **      WHERE G(S)=C*(S1-A)**(-1) * B      CCN00860
** ** ** **      SAME AS ABOVE BUT G(-S)          CCN0C870
** ** ** **      G(S)*R***(-1/2)                CCN0C890
** ** ** **      G*GPSRSQ                        CCN0C900
** ** ** **      GGR - GMS*QGGR                  CON0C910
** ** ** **      RGQGR - R**((-1/2) * QQGR      CON0C920
** ** ** **      XIRQGR - I + RGQGR              CGN0C930
** ** ** **      DETERM - AN ARRAY CONSISTING OF THE DET OF XIRQI  CCN0C940
** ** ** **      TO BE USED IN THE OBJECTIVE FUNCTION OF THE OPTIMIZER  CCN00950
** ** ** **      -----THE FOLLOWING ARE USED BY THE SINGULAR VALUE ANALYSIS-----  CON00960
** ** ** **      EIG - EIGENVALUE OF A- B*F*C      CON0C970
** ** ** **      MU - INPUT DESIRED POLE LOCATION  CON0C980
** ** ** **      OMU - ORDERED VALUE OF MU          CCN00990
** ** ** **      OEIG - ORDERED VALUE OF EIG      CCN01000
** ** ** **      OZ - ORDERED EIGENVECTOR          CCN01C10
** ** ** **      XI - IDENTITY MATRIX              CCN01C20
** ** ** **      XXI - IDENTITY MATRIX            CCN01C30
** ** ** **      UI - INPUT ADDITIVE SINGULAR VECTOR ASSOCIATED WITH SV
** ** ** **      VI - INPUT ADDITIVE SINGULAR VECTOR (SVAO)
** ** ** **      VCI - OUTPUT ADDITIVE SINGULAR VECTOR
** ** ** **      VC - OUTPUT ADDITIVE SINGULAR VECTOR
** ** ** **      JMI - INPUT MULTIPLICATIVE SINGULAR VECTOR
** ** ** **      VMI - INPUT MULTIPLICATIVE SINGULAR VECTOR
** ** ** **      UMO - OUTPUT MULTIPLICATIVE SINGULAR VECTOR
** ** ** **      VMO - OUTPUT MULTIPLICATIVE SINGULAR VECTOR
** ** ** **      FXPLT - F # PLANT TRANSFER FUNCTION (G)
** ** ** **      XIPEXP - I + F#G
** ** ** **      PLAN - PLANT TRANSFER FUNCTION (G)
** ** ** **      PLTFX - G#F
** ** ** **      XIPPEX - I + G#F
** ** ** **      PLTFXI - INV(F#G)
** ** ** **      FXPLTI - INV(G#F)
** ** ** **      XIFPLI - I + INV (F#G)
** ** ** **      XIPLFI - I + INV (F#F)

```







```

      MODIFIED BY PROGRAM AT EACH DECADE SHIFT
CARD 3  WT1,WT2,WT3: FFORMAT(3F10.0)
      WEIGHTING FACTORS TO BE USED IN THE MULTIPLE POLES
      PLACEMENT MCCES ( NOT USED IN THE PRESENT FORMULATION)

CARD 4  SVMINI,SVMINO,RJ,NIDG: FFORMAT(3F10.0,15)
      ( ONLY NIDG IS USED IN THIS PROGRAM )
      SVMINI - DESIRED SINGULAR VALUE LEVEL FOR THE S.V. OF
      (I+FG). FOUND USING UNIVERSAL GAIN AND PHASE CHART
      TO GIVE A DESIRED PHASE AND GAIN MARGIN
      SVMINO - OUTPUT VERSION OF SVMINI
      RJ - FACTOR TO SET PERCENT POLE PLACEMENT ERROR THE
      DESIGNER WISHES TO PUT INTO THE OPTIMIZER

----- NIDG - PARAMETER THAT SETS TYPE CONSTRAINT CONSIDERED
      SEE ADS MANUAL FOR USE

CARD 5  IGRAD,NDV,NCON,ISTRAT,IOPT,IONED,IPRINT,INFO
      FFORMAT(8I5)
      IGRAD - PARAMETER CONCERNING GRADIENT COMP SEE ADS
      NDV - NUMBER OF DESIGN VARIABLES
      NCON - NUMBER OF CONSTRAINTS
      ISTRAT - OPTIMIZER STRATEGY SEE ADS MANUAL
      IOPT - OPTIMIZATION METHOD SEE ADS
      IONED - ONE DIMENSIONAL SEARCH TECHNIQUE SEE ADS
      IPRI NT - ADS PRINT CONTROL SEE ADS
      INFO - OPTIMIZER CONTROL PARAMETER SEE ADS

CARD 6  NROWA,NCOLA,NROWB,NCOLB,NROWC,NCCLC,NROWF,NCOLF,NROWQ
      NCOLQ,NROWR; NCOLR,NMU,
      FFORMAT(12I2)
      NUMBER OF ROWS AND COLUMNS CF INPUT MATRICES AND
      NUMBER OF POLES TO BE INPUT FOR PLACEMENT
      EXAMPLE: NMU = 1 MEANS TO PLACE PCLE ONE AT A TIME

CARD 7  A MATRIX; READ BY ROWS AS:
      A(1,1) A(1,2)
      A(2,1) A(2,2)
      THERE WILL BE ONE OR MORE CARDS FOR EACH ROW OF A
      AFTER THE PROPER CARDS ARE READ FOR A THE NEXT MATRIX MUST
      BE REACT IN. THE REMAINDER OF THIS COMMENT WILL REFER TO EACH NEW
      DATA SET AS A CARD. REMEMBER, THERE MAY BE SEVERAL CARDS PER
      SET SO THE NUMBERS DON'T CORRESPOND DIRECTLY WITH THE DATA
      LISTED IN THE INPUT FILE.

CARD 8  B MATRIX; READ ROW BY ROW
CARD 9  C MATRIX; READ ROW BY ROW

```

```

CCN01600
CCN01650
CCN01610
CCN01620
CCN01630
CCN01650
CCN01720
CCN01730
CCN01740
CCN01750
CCN01760
CCN01770
CCN01780
CCN01750
CCN01790
CCN01800
CCN01850
CCN01810
CCN01820
CCN01830
CCN01840
CCN01850
CCN01860
CCN01870
CCN01880
CCN01890
CCN01900
CCN01950
CCN01910
CCN01920
CCN01930
CCN01940
CCN01950
CCN01960
CCN01970
CCN01980
CCN01990
CCN02000
CCN02010
CCN02020
CCN02030
CCN02040
CCN02050

```

\*\*\*\*\*

\*\*\*\*\*

CC

```

CGN02C60
*****
CARD 10 F MATRIX; READ ROW BY ROW ONLY FOR SINGULAR VALUE
      THE F ENTERED HERE IS USED ONLY FOR SINGULAR VALUE
      ANALYSIS MODE, FOR OTHER MODES THE POLE PLACEMENT
      ROUTINE WILL GENERATE Q AND THEN F (FROM INNER ROUTINE)
CARD 11 Q MATRIX; READ ROW BY ROW ( Q=0 WHEN NO STARTING VALUES
      IS USED )
*****
CARD 12 R MATRIX; READ ROW BY ROW
CARD 13 IQW MATRIX; ROW BY ROW
      FORMAT(8I2); THIS MATRIX DEFINES THE DESIGN VARIABLE
      TO THE OPTIMIZER. THE ENTRY WOULD BE OF THE FORM:
      1 2 3
      THIS WOULD TELL THE OPTIMIZER TO MAKE Q(1,1) THE FIRST
      DESIGN VARIABLE (X(1)) AND SO FORTH. THE ZERO TELLS THE
      OPTIMIZER THAT F(2,1) (IN THIS CASE) IS NOT A DESIGN
      VARIABLE AND IS NOT TO BE CHANGED.
      AS Q IS REQUIRED TO BE SYMMETRIC, ONLY ONE OFF
      DIAGONAL TERM IS REQUIRED. I.E. ONLY C(1,2) OR Q(2,1)
      IS ASSIGNED. THE PROGRAM AUTOMATICALLY MAKES Q(1,2)
      EQUAL Q(2,1) ETC..
*****
CARD 14 VLB,VUB; FORMAT(2F10.0)
      THERE WILL BE ONE CARD FOR EACH DESIRED POLES
*****
CARD 15 REALMU,IMAGMU; FORMAT (2F10.0)
      INPUT REAL AND IMAGINARY DESIRED POLE LOCATION
      ONE POLE PER CARD
*****
CALL ERFSET(207,256,-1,1,209)
CALL ERFSET(215,256,-1,1)
CALL ERFSET(187,256,-1,1)
*****
***** INPUT MODES *****
***** INPUT MODES *****
***** READ (1,750) KODE,KONTRL *****
***** WRITE (6,*) KONTRL0,KONTRL *****
*****
---INPUT MAXN, INITIAL FREQUENCY, DELTA FREQ, OPTIMIZER WEIGHTS-----
READ (1,710) WMAX,W19,DELM
READ (1,570) WTL,W12,W13
*****
---INPUT DESIRED SINGULAR VALUES (NOT USED) AND TYPE OF CONSTRAINTS---

```

```

CCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCCC
CCCCC
CCC
CC

```



```

C      READ (1,580) SVMINI,SVMINO,RJ,NIDG
C      W=WI9
C      NC=1
C      ----INPUT OPTIMIZER INPUT DATA (SEE ADS MANUAL)-----
C
C      READ (1,760) IGRAD,NDV,NCON,ISTRAT,IOPT,IONED,IPRINT,INFO
C      ----INPUT THE PARAMETER VALUES AND THE MATRICES A,B,C,F,QW,RW-----
C
C      READ (1,770) NROWA,NCOLA,NROWB,NCOLB,NROWC,NCOLC,NROWF,NCOLF,
C      1NROWQ,NCOLQ,NROWR,NCOLR,NMU
C      CALL REAC (A,NROWA,NCOLA)
C      CALL REAC (B,NROWB,NCOLB)
C      CALL REAC (C,NROWC,NCOLC)
C      CALL REAC (F,NROWF,NCOLF)
C      CALL REAC (QW,NROWQ,NCOLQ)
C      CALL REAC (RW,NROWR,NCOLR)
C      DO 13 I=1,NROWR
C      DO 13 J=1,NCOLR
C      RWSP(I,J)=RW(I,J)
C      CONTINUE
C
C      13 ----SPECIFY THE DESIGN VARIABLES WITHIN THE Q MATRIX-----
C      IF R OR BOTH Q AND R IS TO BE VARIED, MODIFICATION
C      IS REQUIRED FOR THE FOLLOWING BLOCK
C
C      DO 10 J=1,NROWQ
C      READ (1,780) (IQW(J,K),K=1,NCOLQ)
C      CONTINUE
C      10 ----SET THE DESIGN VARIABLE BOUNDS-----
C
C      DO 20 J=1,NDV
C      READ (1,790) VLB(J),VUB(J)
C      CONTINUE
C      20 ---- REAC THE DESIRED EIGENVALUES -----
C
C      DO 60 I=1,NMU
C      READ (1,860) REALMU(I),IMAGMU(I)
C      CONTINUE
C      DO 70 I=1,NMU
C      MU(I)=CMPLX(REALMU(I),IMAGMU(I))
C      CONTINUE
C      70 ---- SORT THE INPUT EIGENVALUES USING IMSL ROUTINE VSRTR-----
C
C      DO 80 I=1,NMU

```

```

CCN02350
CCN02360
CCN02370
CCN02380
CCN02390
CCN02400
CCN02410
CCN02420
CCN02430
CCN02440
CCN02450

CCN02460
CCN02470
CCN02480
CCN02490
CCN02460
CCN02470

CCN02500
CCN02510
CCN02520

CCN02530
CCN02540

CCN02550
CCN02560
CCN02570
CCN02580
CCN02590

CCN02710
CCN02720
CCN02730
CCN02740
CCN02750

CCN02760
CCN02770
CCN02780
CCN02800
CCN02810
CCN02820

```









```

C      CALL CMATML (OZ,LX,NROWA,NCOLA,NROWA,TEMPX2)
C      CALL CMATML (AX,TEMPX2,NROWA,NCOLA,NROWA,TEMPX)
C      CALL CMATML (OZI,TEMPX,NROWA,NCOLA,NROWA,TEMPX2)
C      CALL CMATML (LXI,TEMPX2,NROWA,NCOLA,NROWA,AX)
C
C----- TRANSFORM BW -----
C
C      CALL CPLEQU (BX,TEMPX,NROWB,NCOLB)
C      CALL CMATML (OZ,LX,NROWA,NCOLA,NROWA,TEMPX2)
C      CALL LECTIC (TEMPX2,NROWA,IO,ZLI,NROWA,IO,O,WA,IER)
C      CALL CMATML (ZLI,TEMPX,NROWA,NROWA,NCOLB,BX)
C
C----- TRANSFORM GWX -----
C
C      CALL CMATML (OZ,LX,NROWA,NCOLA,NROWA,TEMPX2)
C      CALL CMATML (QWX,TEMPX2,NROWQ,NCOLQ,NROWA,TEMPX)
C      CALL CMATMT (TEMPX2,TEMPX,NROWC,NCOLQ,NROWA,QWX)
C
C      ELSE
C
C----- TRANSFORM AX (REAL EIG VALUE)-----
C
C      CALL CMATML (AX,OZ,NROWA,NCOLA,NROWA,TEMPX)
C      CALL CMATML (OZI,TEMPX,NROWA,NCOLA,NROWA,AX)
C
C----- TRANSFORM BX -----
C
C      CALL CPLEQU (BX,TEMPX,NROWB,NCOLB)
C      CALL CMATML (OZI,TEMPX,NROWA,NROWA,NCOLB,BX)
C
C----- TRANSFORM GWX -----
C
C      CALL CMATML (QWX,OZ,NROWQ,NCOLQ,NROWA,TEMPX)
C      CALL CMATMT (OZ,TEMPX,NROWQ,NCOLQ,NROWA,QWX)
C      END IF
C
C----- END OF IF THEN ELSE BLOCK -----
C
C----- CUTPUT TRANSFORMED A,B,Q -----
C      WRITE (6,*) , *** TRANSFORMED A MATRIX *** ,
C      CALL CPLREA (AX,TEMPR,NROWA,NCOLA)
C      CALL WRITE (TEMPR,NROWA,NCOLA)
C      WRITE (6,*) , *** TRANSFORMED Q MATRIX *** ,
C      CALL CPLREA (QWX,TEMPR,NROWQ,NCOLQ)
C      CALL WRITE (TEMPR,NROWQ,NCOLQ)
C      WRITE (6,*) , *** TRANSFORMED B MATRIX *** ,
C      CALL CPLREA (BX,TEMPR,NROWB,NCOLB)
C      CALL WRITE (TEMPR,NROWB,NCOLB)

```



```

C----- END OF TRANSFORMATION BLOCK -----
C
C----- FORMULATE THE DESIGN VARIABLE X FROM THE STARTING Q -----
C
      DO 50 J=1,NROWQ
      DO 40 K=1,NCULQ
      IF (IQW(J,K).EQ.0) GO TO 30
      KK=IQW(J,K)
      X(KK)=REAL(CWX(J,K))
      CONTINUE
      CONTINUE
      CONTINUE
C-----
      CALL CPLXCV (RWX,RW,NROWR,NCOLR)
C-----
C----- CALCULATE R**1/2 -----
C----- USING LINPACK ROUTINE AND WURZEL ROUTINE
C
      CALL SPCCO(RW,10,NCCLR,RCOND,Z1,INFCL)
      CALL SPCCI(RW,10,NCCLR,DET,1)
      DO 131 I=1,NROWR
      DO 131 J=1,NROWR
      RW(J,I)=RW(I,J)
      CONTINUE
      CONTINUE
C----- COMPUTE SQUARE ROOT OF MATRIX R -----
      CALL WURZEL(RW,TEMPR,NROWR,0.99,1.E-6,10)
      CALL CPLXCV (RWSQX,TEMPR,NROWR,NCOLR)
      WRITE (6,*) '***SQUARE ROOT INVERSE OF R ***'
      CALL WRITE(TEMPR,NROWR,NROWR)
C-----
C----- ENTER OPTIMIZATION BLOCK HERE*****
C
      IF KGNTRL SET GREATER THAN 0 THE FIRST PASS JUMPS THE OPTIMIZER
      IF (KCNTRL.GT.0) GO TO 130
C-----
      CALL THE ADS OPTIMIZER TO SOLVE FOR THE BEST Q'S
C-----
      THIS FIRST CALL SETS THE SCALE FLAG SEE ADS MANUAL
      INFO=-2
      CALL ACS (INFO,ISTRAT,IOPT,IONED,IPRINT,IGRAD,NDV,NCON,X,VLB,VUB,0,
      1BJ,6,IDG,NGT,IC,DF,XA,NRA,NCA,WK1,NRWK,IWK,NRIWK)
C-----

```

CCN02610  
CCN02620  
CCN02630  
CCN02640  
CCN02650  
CCN02660  
CCN02670  
CCN02680  
CCN02690  
CCN02700  
CCN03600

CCN03590

CCN03170  
CCN03180  
CCN03190  
CCN03200  
CCN03210  
CCN03220  
CCN03230  
CCN03240  
CCN03250  
CCN03260  
CCN03270  
CCN03280  
CCN03290  
CCN03300

```

C      WK(3)=-C.05
C      IWK(2)=0      IMPLIES NO SCALING
C      IWK(2)=0
C
C      THIS CALL STARTS THE OPTIMIZATION PROCESS
C
C      CALL ACS (INFO,ISTRAT,IOP,T,IONED,IPRINT,IGRAD,NDV,NCON,X,VLE,VUB,0
120  IBJ,G,ICG,NGT,IC,DF,XA,NRA,NCA,WKI,NRWK,IWK,NRIWK)
C      IF (INFC.EQ.0) GO TO 480
C      IF (INFC.GT.1) GO TO 470
C
C      THIS PORTION OF THE PROGRAM DOES THE ACTUAL COMPUTATION
C
C      DO 160 J=1,NROWQ
C      DO 150 K=1,NCOLQ
130
C      ---EQUATE DESIGN VECTOR X WITH THE DESIRED SYSTEM MATRIX---
C
C      IF (IQW(J,K).EQ.0) GO TO 140
C      KK=IQW(J,K)
C      QWX(K,J)=X(KK)
C      QWX(J,K)=X(KK)
C      CONTINUE
C      CONTINUE
C      CONTINUE
C
C      CALL CPLXCV {CX,C,NRCWC,NCOLC}
C      CALL CPLXCV {FX,F,NROWF,NCCLF}
C
C      MAIN LOOP TO COMPUTE THE DET (1+R**((-1/2)G(-S))**T *Q *G(S)R**((-1/2))
C      TO BE USED IN THE OPTIMIZER'S OBJECTIVE FUNCTION
C
C      DO 263 I=1,NMU
C
C      --- PLANT1 COMPUTE G(S) WHERE G=C(SI-A)**(-1)*B---
C      WHERE S IS THE DESIRED POLE LCCATION
C
C      CALL PLANT1(GPS,AX,BX,CX,MU(I),NROWA,NCOLA,NROWB,NCOLB,NROWC,
140  INCCLC)
C
C      --- PLANT1 COMPUTE G(-S) WHERE G=C(SI-A)**(-1)*B---
C      WHERE S IS THE DESIRED POLE LCCATION
C

```

```

      CALL PLANTI(GMS,AX,BX,CX,-MU(I),NRDWA,NCOLA,NROWB,NCOLB,NROWC,
1NCOLC)
      CALL CMATML (GPS,RMSQX,NROWA,NCOLA,NCOLR,GPSRSQ)
      CALL CMATML (QMX,GPSFSQ,NROWA,NCOLA,NCOLR,QGR)
      CALL CMATML (GMS,JGR,NROWA,NCOLA,NCOLR,GGR)
      CALL CMATML (RMSQX,GGR,NROWA,NCOLA,NCOLR,RGGR)
-----
      I+R**-(1/2)IG(-S)*TIQIG(S)R**-(1/2)I
-----
      DO 911 J=1,NROWR
      DO 913 K=1,NCOLR
      XX1(J,K)=C.O
      XX1(J,K)=1.C
      XIROR(J,K)=XX1(J,K)+RGGR(J,K)
913 CONTINUE
911 CONTINUE
-----
      FIND DETERMINANT TO BE USED IN THE OBJECTIVE FUNCTION ---
      USING LINPACK ROUTINE
-----
      CALL CGECC(XIROR,10,NCOLR,IPVT,PCOND,WORK)
      CALL CGEDI(XIROR,10,NCOLR,IPVT,DET,WORK,10)
      DETERM(1)=DET(1)*10.**REAL(DET(2))
-----
293 CONTINUE
-----
      END OF DG LOOP
-----
      FORM QUANTITIES TO USE IN THE COST CRITERIA OF OPTIMIZER-----
      EACH REAL POLE REQUIRED ONE COST, EACH COMPLEX PAIR POLE REQUIRED
      TWO COST(COST1 AND COST2)
      COST1= ((REAL(DETERM(1)))**2+(AIMAG(DETERM(1)))**2)
      COST2= ((REAL(DETERM(2)))**2+(AIMAG(DETERM(2)))**2)
      COST3= ((REAL(DETERM(3)))**2+(AIMAG(DETERM(3)))**2)
      WRITE(6,*) 'X',COST1,DETERM(1),X(1)
-----
      THE OBJECTIVE FUNCTION IS INSERTED HERE-----
      OBJ= CCST1+COST2+COST1*COST2
-----
      WRITE (6,*) 'OBJ',OBJ
      CONSTRAINT EQUATION (IDG(3))=-2 FOR COMPLEX ROOTS)-----
      IF (NCCN.EQ.0) GO TO 460
      DO 450 J=1,2
      IDG(J)=NIDG
      CONTINUE
450 IDG(3)=-2
-----
      OTHER CONSTRAINTS CAN BE INTRODUCED HERE-----

```

CCN04240  
CCN04240  
CCN04240  
CCN04240

CCN05000  
CCN05010

CCN05130  
CCN05140

CCN05180  
CCN05190  
CCN05200  
CCN05210

[illegible]

CCN05240  
CCN05240



```

WRITE (6,*) '
CALL WRITE (Q,NROWC,NCOLC)
-----SINGULAR VALUE ANALYSIS ONLY -----
501 IF (KCODE.EQ.2.AND.KCNTRL.EQ.2) GO TO 532
N2=2*NCCLA
*****
----- THE REDUCE ROUTINE MATCHES THE VARIABLE FROM THE OPTPP
WITH THE MODIFIED VERSION OF THE INNER ROUTINE FROM
CPTSYS PROGRAM
-----

THE SYSTEM MATRIX A,B,C, AND G, F(FROM CPTPP) ARE USED
BY THE INNER ROUTINE TO COMPUTE THE FEEDBACK GAIN F.
F CAN THEN BE USED IN THE SINGULAR VALUE ANALYSIS PORTION OF
THIS PROGRAM
-----

CALL REDUCE(A,B,C,G,RWSP,DUMA,DUMB,DUMC,DUMQ,DUMR,DUMI,
INRCKA,NCCLB)
-----
CALL INNER (NCOLA,NCCLB,NRCWC,N2,DUMA,DUMB,DUMC,DUMQ,DUMR,FBG
1,KM,AA,PRC,XI,GI,DUMRI)
DO 533 I=1,NROWF
DO 533 J=1,NCOLF
F(I,J)=-FBGC(I,J)
533 CONTINUE
532 CALL CPLXCV (AX,A,NRGWA,NCOLA)
CALL CPLXCV (BX,B,NROWB,NCCLB)
CALL CPLXCV (CX,C,NRCWC,NCCLC)
CALL CPLXCV (FX,F,NROWF,NCOLF)
----- THE FINAL FEEDBACK GAIN MATRIX IS DISPLAY HERE-----
WRITE (6,840)
CALL WRITE (F,NROWF,NCOLF)
-----
COMPUTE THE A-B*F*C SYSTEM MATRIX FOR THE NEXT POLE ASSIGNMENT
-----
CALL MMUL (F,C,NROWF,NCOLF,NCOLC,FC)
CALL MMUL (B,FC,NRCWB,NCLE,NCOLC,BFC)
DO 180 I=1,NROWA
DO 170 J=1,NCOLA

```

CCN033590  
CCN033590  
CCN033590

CCN033130  
CCN033140

CCN033630  
CCN033640  
CCN033650

CCN033660  
CCN033670  
CCN033680  
CCN033690



```

170 AMBFC(I,J)=A(I,J)-BFC(I,J)
180 CONTINUE
C WRITE (6,890)
C -----
C CALL WRITE (AMBFC,NROWA,NCOLA)
C
C ***** GO TO 555 *****
C IF (KODE.EQ.0) GO TO 555
C *****
C SINGULAR VALUE ANALYSIS BEGIN HERE
C -----
C CALL THE PLANT TRANSFER MATRIX ROUTINE AND FORM THE SYSTEM
C RETURN DIFFERENCE MATRICES AS REQUIRED
C -----
DEL=DELW
*II=W19
NCNT=1
W=W19
SMINAI=C.
SMINMI=C.
SMINAO=C.
SMINMO=C.
SMAXAI=C.
SMAXMI=C.
SMAXAG=C.
SMAXMG=C.
CALL CPLXCV (AX,A,NROWA,NCOLA)
CALL CPLXCV (BX,B,NROWB,NCOLB)
CALL CPLXCV (CX,C,NROWC,NCOLC)
260 CALL PLANT (PLAN,AX,BX,CX,NROWA,NCOLA,NROWB,NCOLB,NROWC,NCOLC)
CALL CMATML (FX,PLAN,NROWF,NCOLF,NCOLB,NCCLF,PLTFX)
CALL CMATML (PLAN,FX,NROWC,NCOLB,NCCLF,PLTFX)
DO 280 J=1,NROWF
DO 270 K=1,NCOLB
XI(J,K)=0.0
CONTINUE
280 DO 290 J=1,NROWF
290 XI(J,J)=1.0
DO 310 J=1,NROWC
DO 300 K=1,NCOLB
XXI(J,K)=0.0
XXI(J,J)=1.0
XI*PPFX(J,K)=XXI(J,K)+PLTFX(J,K)
300 CONTINUE
310 DO 330 J=1,NROWF

```

```

CCN03700
CCN03710
CCN03730
CCN03740
CCN03750
CCN03760
CCN03770
CCN03780
CCN03790
CCN03800
CCN03810
CCN03820
CCN03830
CCN03840
CCN03850
CCN03860
CCN03870
CCN03880
CCN03890
CCN03900
CCN03910
CCN03920
CCN03930
CCN03940
CCN03950
CCN03960
CCN03970
CCN03980
CCN03990
CCN04000
CCN04010
CCN04020
CCN04030
CCN04040
CCN04050
CCN04060
CCN04070
CCN04080
CCN04090
CCN04100
CCN04110
CCN04120
CCN04130
CCN04140
CCN04150
CCN04160
CCN04170
CCN04180
CCN04190
CCN04200
CCN04210
CCN04220
CCN04230
CCN04240
CCN04250
CCN04260
CCN04270
CCN04280
CCN04290
CCN04300
CCN04310
CCN04320
CCN04330
CCN04340
CCN04350
CCN04360
CCN04370
CCN04380
CCN04390

```

```

320 DO 320 K=1,NCOLB
330 XIPEXP(J,K)=XI(J,K)+FXPLT(J,K)
340 CALL CPLEQU (XIPEXP,TEMPX,NROWF,NROWC)
350 DO 350 J=1,NROWF
360 DO 360 K=1,NROWC
370 FXPLTI(J,K)=0.0
380 FXPLTI(J,J)=1.0
390 CONTINUE
400 DO 400 J=1,NROWC
410 DO 400 K=1,NROWC
420 PLTFXI(J,K)=J.0
430 PLTFXI(J,J)=1.
440 CONTINUE
450 C THIS ESTABLISHES THE RETURN DIFFERENCE MATRIX FOR MULT. CASE
460 C
470 C
480 CALL LECTIC (FXPLT,NROWF,10,FXPLTI,NROWF,10,0,WA,IER)
490 CALL LECTIC (PLTFX,NROWC,10,PLTFXI,NROWC,10,0,WA,IER)
500 DO 500 J=1,NROWF
510 DO 500 K=1,NCOLB
520 XIPLI(J,K)=XI(J,K)+FXPLTI(J,K)
530 CONTINUE
540 CONTINUE
550 DO 550 J=1,NROWC
560 DO 550 K=1,NROWC
570 XIPLFI(J,K)=XI(J,K)+PLTFXI(J,K)
580 CONTINUE
590 CONTINUE
600 -----
610 DO SINGULAR VALUE DECCMP AND QUANTIFY ALL DESIRED SV'S
620 -----
630 CALL CSVD (XIPEXP,10,10,NROWF,NROWF,0,NROWF,NROWF,SV,UI,VI)
640 CALL CSVD (XIPEXP,10,10,NROWC,NROWC,0,NROWC,NROWC,SVAG,LO,VO)
650 CALL CSVD (XIPLI,10,10,NROWF,NROWF,0,NROWF,NROWF,SVMI,UMI,VMI)
660 CALL CSVD (XIPLFI,10,10,NROWC,NROWC,0,NROWC,NROWC,SVMO,LMO,VMO)
670 -----
680 C----- THIS PORTION COMPUTES THE MAXIMUM EIG-VALUES OF THE -----
690 C RETURN DIFFERENCE MATRIX WHICH GIVE THE UPPER BOUND
700 C FOR THE SINGULAR VALUE
710 C
720 CALL EIGCC(TEMPX,NROWF,10,0,EIG,Z,10,WK,IER)
730 DO 730 I=1,NROWF
740 MEIG(I)=SQRT((REAL(EIG(I))**2+(AIMAG(EIG(I))**2)
750 IF (I.EC.1) THEN
760 MEIG(I)=MEIG(I)

```







```

740 1X,13HMAX ADD IN SV,2X,18HMIN PRCD ADD IN SV)
750 FORMAT (6(F10.5,1X))
760 FORMAT (15,15)
770 FORMAT (815)
780 FORMAT (1312)
790 FORMAT (812)
800 FORMAT (2F10.0)
810 FORMAT (1H1,///,12H<<<< RUN #,15,6H >>>>,///)
820 FORMAT (///,35H THE A PLANT MATRIX INPUT MATRIX ***,///)
830 FORMAT (///,33H THE B CCONTRGL INPUT MATRIX ***,///)
831 FORMAT (///,33H THE C OBSERVATION MATRIX ***,///)
832 FORMAT (///,33H THE K WEIGHTING MATRIX ***,///)
840 FORMAT (///,38H THE DESIGN VARIABLE (Q) X ***,///)
841 FORMAT (///,40H THE STARTING Q/FINAL F MATRIX ***,///)
850 FORMAT (///,44H THE STARTING Q WEIGHTING MATRIX ***,///)
860 FORMAT (2F10.0)
870 FORMAT (///,37H THE ORDERED COMPLEX EIGENVALUES (INPUT),/)
880 FORMAT (///,29H THE ORDERED COMPUTED EIGENVALUES,/)
890 FORMAT (///,29H THE OPTIMAL Q MATRIX ,/)
900 FORMAT (///,37H THE AUGMENTED A-E#F#C MATRIX ***,///)
910 END

```

```

** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** ** 
** ** ** ** THE END OF THE MAIN PROGRAM (OPTPP) ** ** ** 
** ** ** ** ** 

```

```

CCN05570
CCN05580
CCN05590
CCN06000
CCN06010
CCN06020
CCN06030
CCN06040
CCN06050
CCN06060
CCN06070
CCN06070
CCN06070
CCN06080
CCN06080
CCN06090
CCN06100
CCN06110
CCN06120
CCN06130
CCN06140

```







```

370 DO 370 K=1,NC
    PRG(I,J)=PRG(I,J)+BLI(I,K)*GL(J,K)
    CONTINUE
380 DO 380 I=1,MH
    DO 380 J=1,MH
    RM(I,J+MH)=C.O
    DO 380 K=1,NC
    RM(I,J+MH)=(RM(I,J+MH)-GL(I,K)*PRG(K,J))
    CONTINUE
380 -----2NX2N HAMILTONIAN MATRIX-----
C -----DIAGONAL BLOCKS-----M11 AND M22-----
C
C    WRITE (6,*) 'BA'
C    CALL WRITE (BA,2,2)
C    DO 390 I=1,MH
C    DO 390 J=1,MH
C    RM(I,J)=C.EC
C    RM(I,J)=BA(I,J)
C    RM(I+MH,J+MH)=-BA(J,I)
C -----M21 BLOCK-----
C    RM(I+MH,J)=-RM(I+MH,J)
C    CONTINUE
390 -----M12 BLOCK IS DEFINED IN LINE 430 ABOVE-----
C
400 CONTINUE
C -----EISPACK ROUTINES-----
410 CALL BALANC (M,M,RM,LOW,HIGH,D1)
CALL ORTHES (M,M,LOW,HIGH,RM,D2)
CALL CRRAN (M,M,LOW,HIGH,RM,D2,X1)
CALL HGR2 (M,M,LOW,HIGH,RM,WR,X1,X1,IERR)
C    WRITE (6,*) 'IERR', IERR
C    IF (IERR.NE.0) CALL EREXIT (M,RM,IERR)
C    CALL BALBAK (M,M,LOW,HIGH,D1,M,X1)
C -----DEBUG DIAGNOSTICS ON EULER-LAGRANGE EQUATIONS-----
430 CONTINUE
C    IF (NOB.EQ.0) WRITE (6,1550)
C    IF (NOB.EQ.0) CALL RGAIN TO COMPUTE THE FEEDBACK GAIN
C    CALL RGAIN (M,NS,NC,NCB,WR,WI,X1,GN,W1,RM,W2,D1,CWR,CWI,SC,MHS,
1D2)
C
450 CONTINUE
470 CONTINUE
C -----CALCULATION OF FEEDBACK GAIN-----
C -----FEEDBACK GAINS--> U = -(BINVPSE)*GT*G1&-----
C
C    DO 480 I=1,NS
C    DO 480 J=1,NS
C    PRG(I,J)=C.O
C    DO 480 K=1,NS
C    PRG(I,J)=PRG(I,J)+GL(K,I)*GN(K,J)
C    DO 480 I=1,NC

```

CPT08860  
CPT08870  
CPT08880  
CPT08890  
CPT08900  
  
CPT08910  
CPT08920  
  
CPT08930  
CPT08940  
  
CPT08950  
CPT08960  
CPT08970  
CPT08980  
CPT08990  
CPT09000  
  
CPT09040  
CPT09050  
CPT09060  
CPT09070  
  
CPT09080  
CPT09090  
CPT09100  
CPT09170  
CPT09190  
  
CPT09220  
CPT09230  
CPT09280  
CPT09290  
CPT09340  
CPT09350  
CPT09360  
CPT09370  
CPT09380  
CPT09390  
CPT09400  
CPT09410  
CPT09420  
CPT09430









CCWRCC  
CCWRCC  
CCWRCC  
CCWRCC  
CCWRCC

```

INTEGER N,J
WRITE(6,10) (A(J),J=1,N)
RETURN
FORMAT (2F12.5)
END

```

[illegible]

CWRC 280

WRITE THE REAL VECTOR

```

SUBROUTINE VECWR (A,N,IR)
  REAL*4 A(10)
  DIMENSION IR(50)
  INTEGER N,J
  WRITE(*,*) (A(J),IR(J),J=1,N)
  RETURN
  FORMAT (F12.5,5X,I5)
  END

```

[illegible]

CWROC290

# MATRIX MULTIPLICATION WITH COMPLEX MATRIX

0	0	0	0	0	0	0	0
1	0	0	0	0	0	0	0
2	0	0	0	0	0	0	0
3	0	0	0	0	0	0	0
4	0	0	0	0	0	0	0
5	0	0	0	0	0	0	0
6	0	0	0	0	0	0	0
7	0	0	0	0	0	0	0
8	0	0	0	0	0	0	0
9	0	0	0	0	0	0	0
A	0	0	0	0	0	0	0
B	0	0	0	0	0	0	0
C	0	0	0	0	0	0	0
D	0	0	0	0	0	0	0
E	0	0	0	0	0	0	0
F	0	0	0	0	0	0	0
G	0	0	0	0	0	0	0
H	0	0	0	0	0	0	0
I	0	0	0	0	0	0	0
J	0	0	0	0	0	0	0
K	0	0	0	0	0	0	0
L	0	0	0	0	0	0	0
M	0	0	0	0	0	0	0
N	0	0	0	0	0	0	0
O	0	0	0	0	0	0	0
P	0	0	0	0	0	0	0
Q	0	0	0	0	0	0	0
R	0	0	0	0	0	0	0
S	0	0	0	0	0	0	0
T	0	0	0	0	0	0	0
U	0	0	0	0	0	0	0
V	0	0	0	0	0	0	0
W	0	0	0	0	0	0	0
X	0	0	0	0	0	0	0
Y	0	0	0	0	0	0	0
Z	0	0	0	0	0	0	0
[	0	0	0	0	0	0	0
\	0	0	0	0	0	0	0
]	0	0	0	0	0	0	0
_	0	0	0	0	0	0	0
`	0	0	0	0	0	0	0
{	0	0	0	0	0	0	0
	0	0	0	0	0	0	0
}	0	0	0	0	0	0	0
~	0	0	0	0	0	0	0
	0	0	0	0	0	0	0

```

SUBROUTINE CMATML (R,T,M,LL,N,U)
  COMPLEX *8 R(10,10),T(10,10),J(10,10)
  INTEGER X,LL,N
  DO 20 I=1,M
    DO 20 J=1,N
      U(I,J)=C.O
      DO 10 INDEX=1,LL
        U(I,J)=U(I,J)+T(INDEX,J)
      CONTINUE
    CONTINUE
  CONTINUE
  RETURN
END

```

[illegible]

CWR00550

# REAL MATRIX MULTIPLICATION ROUTINE

CHROCE70  
CHROCE80  
CHROCE90  
CHROCE00  
CHROCE10  
CHROCE20  
CHROCE30

```

SUBROUTINE MMUL (R,T,M,LL,N,U)
  REAL*4 R(10,10),T(10,10),J(10,10)
  INTEGER M,LL,N
  DO 20 I=1,M
    DO 20 J=1,N
      U(I,J)=C.O
  DO 10 INDEX=1,LL

```



```

C      C      PHASE TRANSFORMATION
C      Q=-CONJG(A(K,K))/CABS(A(K,K))
C      DO 60 J=K1,NP
C      A(K,J)=C*A(K,J)
C      60
C      70
C      ELIMINATION OF A(K,J),J=K+2,...,N
C      IF (K.EC.N) GO TO 140
C      Z=C.EO
C      DO 80 J=K1,N
C      Z=Z+REAL(A(K,J))*2+AIMAG(A(K,J))*2
C      C(K1)=C.EO
C      IF (Z.LE.TOL) GO TO 130
C      Z=SCRT(Z)
C      C(K1)=Z
C      W=CABS(A(K,K1))
C      W=(1.-C.EO)/W
C      IF (W.NE.C.EO) Q=A(K,K1)/W
C      A(K,K1)=C*(Z+W)
C      DO 110 I=K1,M
C      O=(C.EO,C.EO)
C      DO 90 J=K1,N
C      U=C+CONJG(A(K,J))*A(I,J)
C      Q=Q/(Z*(Z+W))
C      DO 100 J=K1,N
C      A(I,J)=A(I,J)-Q*A(K,J)
C      CUNTINLE
C      90
C      100
C      110
C      PHASE TRANSFORMATION
C      Q=-CONJG(A(K,K1))/CABS(A(K,K1))
C      DO 120 I=K1,M
C      A(I,K1)=A(I,K1)*Q
C      K=K1
C      GO TO 10
C      120
C      130
C      TOLERANCE FOR NEGLIGIBLE ELEMENTS
C      EPS=0.EO
C      DO 150 K=1,N
C      S(K)=B(K)
C      T(K)=C(K)
C      EPS=AMAX1(EPS,S(K)+T(K))
C      EPS=EPS*ETA
C      150
C      INITIALIZATION OF U AND V
C      IF (NU.EC.O) GO TO 180
C      DO 170 J=1,NU
C      DO 160 I=1,M
C      U(I,J)=(C.EO,C.EO)
C      160

```

```

170 U(J,J)=(1.EC,0.EO)
180 IF (NV.EC.O) GO TO 210
DO 200 J=1,NV
DO 190 I=1,N
V(I,J)=(0.EC,0.EO)
200 V(J,J)=(1.EC,0.EO)
C
C QR DIAGONALIZATION
210 DO 380 KK=1,N
K=N1-KK
C
C TEST FOR SPLIT
220 DO 230 LL=1,K
L=K+1-LL
IF (ABS(T(L)).LE.EPS) GO TO 290
IF (ABS(S(L-1)).LE.EPS) GO TO 240
230 CCONTINUE
C
C CANCELLATION OF E(L)
240 CS=C.EC
SN=1.EO
LI=L-1
DO 280 I=L,K
I=L,K
F=SN*T(I)
T(I)=C*T(I)
IF (ABS(F).LE.EPS) GO TO 290
H=S(I)
W=SQRT(F*F+H*H)
S(I)=W
CS=F/W
SN=-F/W
IF (NV.EC.O) GO TO 260
DO 250 J=1,N
X=REAL(L(J,LI))
Y=REAL(L(J,I))
U(J,LI)=CMPLX(X*CS+Y*SN,0.EO)
250 U(J,I)=CMPLX(Y*CS-X*SN,0.EO)
IF (NP.EC.N) GO TO 280
DO 270 J=N1,NP
Q=A(LI,J)
R=A(I,J)
A(LI,J)=G*CS+R*SN
270 A(I,J)=R*CS-Q*SN
280 CCONTINUE
C
C TEST FOR CONVERGENCE
290 W=S(K)
IF (L.EC.K) GO TO 360

```

```

CWR01580
CWR01590
CWR01600
CWR01610
CWR01620
CWR01630
CWR01640
CWR01650
CWR01660
CWR01670
CWR01680
CWR01690
CWR01700
CWR01710
CWR01720
CWR01730
CWR01740
CWR01750
CWR01760
CWR01770
CWR01780
CWR01790
CWR01800
CWR01810
CWR01820
CWR01830
CWR01840
CWR01850
CWR01860
CWR01870
CWR01880
CWR01890
CWR01900
CWR01910
CWR01920
CWR01930
CWR01940
CWR01950
CWR01960
CWR01970
CWR01980
CWR01990
CWR02000
CWR02010
CWR02020
CWR02030
CWR02040
CWR02050

```

C

```

C CRIGIN SHIFT
X=S(L)
Y=S(K-I)
G=T(K-I)
H=T(K)
F=((Y+H)*(G-H)*(G+H))/(2.EO*H*Y)
G=SQR(T(F*F+1.EO))
IF (F.LT.0.EO) G=-G
F=((X-H)*((X+H)+(Y/(F+G)-H)*H)/X

```

C

```

C CR STOP
CS=1.EO
SN=1.EO
LI=L+1 I=LI,K
DO 350 J=I,N
G=T(I)
Y=S(I)
H=SN*G
G=CS*G
W=SQR(T(H*H+F*F))
T(I-I)=W
CS=H/W
SN=H/W+G*SN
F=X*CS+G*SN
G=X*CS-Y*SN
H=Y*CS
Y=Y*CS
IF (N.EQ.0) GO TO 310
DO 300 J=I,N
X=REAL(V(J,I-I))
W=REAL(V(J,I))
V(J,I-I)=CMPLX(X*CS+Y*SN,0.EO)
V(J,I)=CMPLX(W*CS-X*SN,0.EO)
W=SQR(T(H*H+F*F))
S(I-I)=W
CS=H/W
SN=H/W+SN*Y
F=CS*G+SN*Y
X=C*Y-SN*G
IF (N.EQ.0) GO TO 330
DO 320 J=I,N
Y=REAL(U(J,I-I))
W=REAL(U(J,I))
U(J,I-I)=CMPLX(Y*CS+W*SN,0.EO)
U(J,I)=CMPLX(W*CS-Y*SN,0.EO)
IF (N.EQ.NP) GO TO 350
DO 340 J=N1,NP

```

300  
310

320  
330

CPO2C60  
 CPO2C70  
 CPO2C80  
 CPO2C90  
 CPO2C100  
 CPO2C110  
 CPO2C120  
 CPO2C130  
 CPO2C140  
 CPO2C150  
 CPO2C160  
 CPO2C170  
 CPO2C180  
 CPO2C190  
 CPO2C200  
 CPO2C210  
 CPO2C220  
 CPO2C230  
 CPO2C240  
 CPO2C250  
 CPO2C260  
 CPO2C270  
 CPO2C280  
 CPO2C290  
 CPO2C300  
 CPO2C310  
 CPO2C320  
 CPO2C330  
 CPO2C340  
 CPO2C350  
 CPO2C360  
 CPO2C370  
 CPO2C380  
 CPO2C390  
 CPO2C400  
 CPO2C410  
 CPO2C420  
 CPO2C430  
 CPO2C440  
 CPO2C450  
 CPO2C460  
 CPO2C470  
 CPO2C480  
 CPO2C490  
 CPO2C500  
 CPO2C510  
 CPO2C520  
 CPO2C530



```

      Q=A(I-I,J)
      R=A(I,J)=G*CS+R*SN
      A(I-I,J)=R*CS-Q*SN
340  CONTINUE
350  T(L)=O.E0
      T(K)=F
      S(K)=X
      GO TO 220
C
C CONVERGENCE
360  IF (W.GE.0.E0) GO TO 380
      S(K)=-W
      IF (NV.EG.0) GO TO 380
      DO 370 J=1,N
370  V(J,K)=-V(J,K)
380  CONTINUE
C SCPT SINGULAR VALUES
      DO 450 K=1,N
      S=-1.E0
      J=K
      DO 390 I=K,N
      IF (S(I).LE.G) GO TO 390
      G=S(I)
      J=I
      CONTINUE
390  IF (J.EG.K) GO TO 450
      S(J)=S(K)
      S(K)=G
      IF (NV.EG.0) GO TO 410
      DO 400 I=1,N
      Q=V(I,J)
      V(I,J)=V(I,K)
      V(I,K)=Q
      IF (NU.EG.0) GO TO 430
      DO 420 I=1,N
      G=U(I,J)
      U(I,J)=U(I,K)
      U(I,K)=G
      IF (N.EG.NP) GO TO 450
      DO 440 I=N1,NP
      Q=A(J,I)
      A(J,I)=A(K,I)
      A(K,I)=Q
      CONTINUE
440  A(K,I)=Q
450  CONTINUE
C BACK TRANSFORMATION

```

```

CWR02540
CWR02550
CWR02560
CWR02570
CWR02580
CWR02590
CWR02600
CWR02610
CWR02620
CWR02630
CWR02640
CWR02650
CWR02660
CWR02670
CWR02680
CWR02690
CWR02700
CWR02710
CWR02720
CWR02730
CWR02740
CWR02750
CWR02760
CWR02770
CWR02780
CWR02790
CWR02800
CWR02810
CWR02820
CWR02830
CWR02840
CWR02850
CWR02860
CWR02870
CWR02880
CWR02890
CWR02900
CWR02910
CWR02920
CWR02930
CWR02940
CWR02950
CWR02960
CWR02970
CWR02980
CWR02990
CWR03000
CWR03010

```





```

C-----
C EQUATE ONE COMPLEX MATRIX TO ANOTHER
C-----
C SUBROUTINE CPLFQU (X,Y,N,K)
C COMPLEX *8X(10,10),Y(10,10)
C REAL*4 A(10,10)
C INTEGER N,K
C DO 20 I=1,N
C DO 10 J=1,K
C Y(I,J)=X(I,J)
C CONTINUE
C RETURN
C END
C-----
C *****
C-----
C THIS ROUTINE WILL COMPUTE THE TRANSFER FUNCTION AS A
C FUNCTION OF FREQUENCY FOR A GIVEN A, B, C SET OF
C MATRICES
C-----
C SUBROUTINE PLANT (GP,AX,BX,CX,W,NFA,NCA,NRB,NRC,NCC)
C COMPLEX *8CX(10,10),AX(10,10),BX(10,10),GP(10,10),SIA(10,
C 10),SIAI(10,10),SIAIB(10,10),SI(10,10)
C COMPLEX S
C REAL*4 WA(100)
C S=CMPLX(0.0,W)
C DO 20 J=1,NRA
C DO 10 K=1,NCA
C SI(J,K)=C.0
C I(J,K)=C.0
C CONTINUE
C DO 30 J=1,NCA
C I(J,J)=1.0
C SI(J,J)=S*I(J,J)
C DO 50 J=1,NRA
C DO 40 K=1,NCA
C SIA(J,K)=SI(J,K)-AX(J,K)
C CONTINUE
C CALL LEGTIC (SIA,NCA,10,1,NCA,10,0,WA,IER)
C CALL CMATML (I,BX,NCA,NCA,NCB,SIAIB)
C CALL CMATML (CX,SIAIE,NRC,NCC,NCB,GP)
C RETURN
C END
C-----
C *****
C-----
C THIS ROUTINE IS INPUT FOR DE SOLVER
C WHEN DE SOLVER IS ADDED DIRECTLY TO CONXSV
C-----
C-----
C-----

```









```

C=====
SUBROUTINE RGAIN (M,NS,NC,NDB,WR,WI,VF,GN,W1,TCB,W21,LT,C,CI,CT,M
IHS,MT)
C=====
IMPLICIT REAL*4 (A-H,C-Z)
DIMENSION WR(M),WI(M),VF(M,M),GN(NS,NS)
DIMENSION W1(NS,NS),TCB(M,M),W21(NS,NS),LT(NS),MT(NS)
K=1
KP=1
KN=1
NRZEV=0
NCPZEV=0
IF (K.GT.M) GO TO 210
C-----
C CHECK FOR EIGVAL AT OR NEAR J-OMEGA AXIS TO INCLUDE IN E-L EIGSYS
C TURN FIRST ONE POSITIVE AND SECOND ONE NEGATIVE
C-----
EIGVR=CABS(WR(K))
EIGVR=ABS(WI(K))
IF (EIGVR.GE.1.E-10) GO TO 60
IF (WI(K)) 40,20,40
20 NRZEV=NRZEV+1
IF (NRZEV.GT.1) GO TO 30
WR(K)=EIGVR
GO TO 80
30 WR(K)=-EIGVR
WRITE (6,290)
GO TO 150
40 NCPZEV=NCPZEV+1
IF (NCPZEV.GT.1) GO TO 50
WR(K)=EIGVR
WR(K+1)=EIGVR
GO TO 110
50 WR(K)=-EIGVR
WR(K+1)=-EIGVR
WRITE (6,300)
GO TO 180
60 IF (WR(K)) 140,70,70
70 IF (WI(K)) 110,80,110
80 CONTINUE
C----- EIGENVECTOR FOR REAL EIGENVALUE, POSITIVE -----
IF (NOB.EQ.0) GO TO 100
DO 90 J=1,M
TCB(J,KP)=VF(J,K)
KP=KP+1
K=K+1
GO TO 10
C80
C90
C100
CPT13820
CPT13830
CPT13840
CPT13850
CPT13860
CPT13870
CPT13880
CPT13890
CPT13900
CPT13910
CPT13920
CPT13930
CPT13940
CPT13950
CPT13960
CPT13970
CPT13980
CPT13990
CPT14000
CPT14010
CPT14020
CPT14030
CPT14040
CPT14050
CPT14060
CPT14070
CPT14080
CPT14090
CPT14100
CPT14110
CPT14120
CPT14130
CPT14140
CPT14150
CPT14160
CPT14170
CPT14180
CPT14190
CPT14200
CPT14210
CPT14220
CPT14230
CPT14240
CPT14250
CPT14260

```

```

C-----EIGENVECTOR FOR COMPLEX EIGENVALUE, POSITIVE REAL PART-----CPT14270
110 CONTINUE
C110 IF (NCB.EC.O) GO TO 130
C DO 120 J=1,M
C FR=VF(J,K)
C FI=-VF(J,K+1)
C TCB(J,KF)=FR+FI
C120 TCB(J,KP+1)=FR-FI
130 KP=KP+2
K=K+2
GO TO 10
140 IF (WI(K)) 180,150,180
C-----EIGENVECTOR FOR REAL EIGENVALUE, NEGATIVE REAL PART-----
150 C(KN)=WR(K)
C1(KN)=WI(K)
IF (NCB.NE.O) GO TO 170
KNS=KN+NS
DO 160 J=1,M
TCB(J,KNS)=VF(J,K)
160 KN=KN+1
170 K=K+1
GO TO 10
C-----EIGENVECTOR FOR COMPLEX EIGENVALUE, NEGATIVE REAL PART-----
180 RK=WR(K)
RI=WI(K)
C(KN)=RR
C(KN+1)=RR
C1(KN)=RI
C1(KN+1)=-RI
IF (NCB.NE.O) GO TO 200
KNS=KN+NS
DO 190 J=1,M
FR=VF(J,K)
FI=-VF(J,K+1)
TCB(J,KNS)=FR+FI
190 TCB(J,KNS+1)=FR-FI
200 KN=KN+2
K=K+2
GO TO 10
210 CONTINUE
C IF (NCB.NE.O) GO TO 240
C-----FORMATION OF W1-----
DO 220 I=1,NS
DO 220 J=1,NS
W1(I,J)=TCB(I,J+NS)
220 CT(I,J)=W1(I,J)
C-----FORMATION OF W2-----
DO 230 I=1,NS

```

```

230 DO 230 J=1,NS
240 W21(I,J)=TCB(I+NS,J+NS)
240 C CONTINUE
240 IF (NOB.EG.O) GO TO 260
240 DO 250 I=1,NS
240 DO 250 J=1,NS
240 W21(I,J)=-TCB(I,J)
240 W11(I,J)=TCB(I+NS,J)
240 C CONTINUE
240 -----INVERT w11-----
240 NSG=NS*NS
240 CALL MINV (NSQ,W11,NS,DETC,LT,MT)
240 C -----CALCULATE THE RGAIN MATRIX-----
240 DO 270 IL=1,NS
240 DO 270 JL=1,NS
240 GN(IL,JL)=0.FO
240 DO 270 KL=1,NS
240 GN(IL,JL)=GN(IL,JL)+W21(IL,KL)*W11(KL,JL)
240 C IF (NOB.EG.O) RETURN
240 DO 280 I=1,NS
240 DO 280 J=1,NS
240 CT(I,J)=W11(J,I)
240 C RETURN
240 -----
240 C -----EULER-LAGRANGE EQUATIONS HAVE A REAL EIGENVALUE AT,
240 J1+H OK NEAR ZERO./)
240 C -----EULER-LAGRANGE EQUATIONS HAVE A COMPLEX PAIR OF ,40
240 C HEIGENVALUES AT OR NEAR THE J-CMEGA AXIS.)
240 C -----
240 C SUBROUTINE MINV (NSQ,A,N,D,L,M)
240 C -----
240 C IMPLICIT REAL*4 (A-H,O-Z)
240 C DIMENSION A(NSQ),L(N),M(N)
240 C DOUBLE PRECISION A,D,BIGA,HOLD
240 C REAL*4 D,BIGA,HOLD
240 C NM=N*N
240 C D=1.D00
240 C NK=-N
240 C DO 180 K=1,N
240 C NK=NK+N
240 C L(K)=K
240 C M(K)=K
240 C KK=NK+K
240 C BIGA=A(KK)
240 C DO 20 J=K,N
240 C IZ=N*(J-1)

```

CPT14740  
CPT14750

CPT14760  
CPT14770  
CPT14780  
CPT14790  
CPT14800  
CPT14810  
CPT14820  
CPT14830  
CPT14840  
CPT14850  
CPT14860  
CPT14870  
CPT14880  
CPT14890  
CPT14900  
CPT14910  
CPT14920  
CPT14930  
CPT14940  
CPT14950  
CPT14960  
CPT14970  
CPT14980  
CPT14990  
CPT15000  
CPT15010  
CPT15020  
CPT15030  
CPT15040  
CPT15050  
CPT15060  
CPT15070  
CPT15080  
CPT15090  
CPT15100  
CPT15110  
CPT15120  
CPT15130  
CPT15140  
CPT15150  
CPT15160  
CPT15170

```

DO 20 I=K,N
IJ=I+1
IF (DABS(BIGA)-DABS(A(IJ))) 10,20,20
IF (ABS(BIGA)-ABS(A(IJ))) 10,20,20
10 BIGA=A(IJ)
L(K)=I
M(K)=J
20 CONTINUE
-----INTERCHANGE ROWS-----
J=L(K)
IF (J-K) 50,50,30
KI=K-N
DO 40 I=1,N
KI=KI+N
HOLD=-A(KI)
JI=KI-K+J
A(KI)=A(JI)
A(JI)=HOLD
40 CONTINUE
-----INTERCHANGE COLUMNS-----
I=M(K)
IF (I-K) 80,80,60
JP=N*(I-1)
DO 70 J=1,N
JK=NK+J
JI=JP+J
HOLD=-A(JK)
A(JK)=A(JI)
A(JI)=HOLD
70 CONTINUE
-----DIVIDE COLUMN BY MINUS PIVOT-----
----- (VALUE OF PIVOT ELEMENT IS CONTAINED IN BIGA) -----
IF (BIGA) 100,90,100
D=0.0D0
D=C.0EC
RETURN
100 DU 120 I=1,N
IF (I-K) 110,120,110
IK=NK+I
A(IK)=A(IK)/(-BIGA)
120 CONTINUE
-----REDUCE MATRIX-----
DO 150 I=1,N
IN=NK+I
HOLD=A(IK)
IJ=I-N
DO 150 J=1,N
IJ=IJ+N
IF (I-K) 130,150,130
IF (J-K) 140,150,140
130

```



```

140      KJ=IJ-I+K
150      A(IJ)=HCLD*A(KJ)+A(IJ)
160      CONTINUE
170      KJ=K-N
180      DU 170 J=1,N
190      KJ=KJ+N
200      IF (J-K) 160,170,160
210      A(KJ)=A(KJ)/BIGA
220      CONTINUE
230      D=D*BIGA
240      A(KK)=(1.0EC)/BIGA
250      CONTINUE
260      K=N
270      K=(K-1) 260,260,200
280      IF (K) 260,260,200
290      I=L(K)
300      IF (I-K) 230,230,210
310      JU=N*(K-1)
320      JP=N*(I-1)
330      DO 220 J=1,N
340      JK=JQ+J
350      HOLD=A(JK)
360      JI=JR+J
370      A(JK)=-A(JI)
380      A(JI)=HCLD
390      J=M(K)
400      IF (J-K) 190,190,240
410      KI=K-N
420      DO 250 I=1,N
430      KI=KI+N
440      HOLD=A(KI)
450      JI=KI-K+J
460      A(KI)=-A(JI)
470      A(JI)=HCLD
480      GU TO 150
490      K=Q
500      RETURN
510      END
520      SUBROUTINE EREXIT (N,A,IERR)
530      EREXIT RETURNS THE NUMBER OF THE EIGENVALUE WHERE HQR2
540      FAILS, THEN STOPS THE PROGRAM.
550      IF (IERR) THEN
560      PRINT *, 'HQR2 FAILED AT EIGENVALUE', N
570      STOP
580      END

```

```

INTEGER IERR
DOUBLE PRECISION A
DIMENSION A(N,N)
WRITE (5,10) IERR
CALL RAPRINT (N,N,N,S,A,4,'(9(1X,1PD13.0))')
RETURN
FORMAT (35H FAILURE IN HQR2 ON EIGENVALUE NO. ,I3)
END
10
=====
C SUBROUTINE MATPRT -- DISPLAYS A TWO-DIMENSIONAL ARRAY (16 COLS. MAX) =
C IN VARIABLE SCREEN FORMAT FOR USER EASE IN ROW IDENTIFICATION. =
C =====
C SUBROUTINE MATPRT (PRIT,NRGW,NCCL)
C =====
C IMPLICIT REAL*4 (A-H,O-Z)
C DIMENSION PRIT(NRGW,NCCL)
C -----
IF (NCCL.EQ.0) NCCL=1
IF (NCCL.EQ.1) WRITE(5,10)
IF (NCCL.EQ.2) WRITE(5,20)
IF (NCCL.EQ.3) WRITE(5,30)
IF (NCCL.EQ.4) WRITE(5,40)
IF (NCCL.EQ.5) WRITE(5,50)
IF (NCCL.EQ.6) WRITE(5,60)
IF (NCCL.EQ.7) WRITE(5,70)
IF (NCCL.EQ.8) WRITE(5,80)
IF (NCCL.EQ.9) WRITE(5,90)
IF (NCCL.EQ.10) WRITE(5,100)
IF (NCCL.EQ.11) WRITE(5,110)
IF (NCCL.EQ.12) WRITE(5,120)
IF (NCCL.EQ.13) WRITE(5,130)
IF (NCCL.EQ.14) WRITE(5,140)
IF (NCCL.EQ.15) WRITE(5,150)
IF (NCCL.EQ.16) WRITE(5,160)
RETURN
C -----
10 FORMAT (F12.5)
20 FORMAT (2F12.5)
30 FORMAT (3F12.5)
40 FORMAT (4F12.5)
50 FORMAT (5F12.5)
60 FORMAT (6F12.5)
70 FORMAT (6F12.5,/,F12.5,/)
80 FORMAT (6F12.5,/,2F12.5,/)
90 FORMAT (6F12.5,/,3F12.5,/)
100 FORMAT (6F12.5,/,4F12.5,/)
110 FORMAT (6F12.5,/,5F12.5,/)
120 FORMAT (6F12.5,/,6F12.5,/)
CPT3C900
CPT3C910
CPT3C920
CPT3C930
CPT3C940
CPT3C950
CPT3C960
CPT3C970
CPT3C980
CPT3C990
CPT31C00
CPT31C10
CPT31C20
CPT31C30
CPT31C40
CPT31C50
CPT31C60
CPT31C70
CPT31C80
CPT31C90
CPT31100
CPT31110
CPT31120
CPT31130
CPT31140
CPT31150
CPT31160
CPT31170
CPT31180
CPT31190
CPT31200
CPT31210
CPT31220
CPT31230
CPT31240
CPT31250
CPT31260
CPT31270
CPT31280
CPT31290
CPT31300
CPT31310
CPT31320
CPT31330
CPT31340
CPT31350
CPT31360

```

```

130 FORMAT (6F12.5,/,6F12.5,/,F12.5,/,/)
140 FORMAT (6F12.5,/,6F12.5,/,2F12.5,/,/)
150 FORMAT (6F12.5,/,6F12.5,/,3F12.5,/,/)
160 FORMAT (6F12.5,/,6F12.5,/,4F12.5,/,/)
END
C=====
C SUBROUTINE MODE (WNORM,G,GNORM,NS,N1,N2,ICON)
C
C   WNORM TRANSFORMATION MATRIX U OR U-INV
C   NS NO. OF STATE
C   NC NO. OF INPUTS OR OUTPUTS
C   ICON CONTROL FLAG TO INDICATE WHICH TRANSFORMATION
C      0 = MODAL G
C      1 = MODAL GAMMA
C      2 = MODAL H
C      3 = MODAL C
C      4 = MODAL K
C      5 = CONTROL EIGENVECTOR MATRIX
C      6 = MEASUREMENT EIGENVECTOR MATRIX
C=====
C IMPLICIT REAL*4(A-H,G-Z)
C DIMENSION WNORM(NS,NS),G(N1,N2),GNORM(N1,N2)
C DO 10 I=1,N1
C DO 10 J=1,N2
C   GNORM(I,J)=C.
C   IPCINT=IPCINT+1
C GO TO (20,20,90,90,20,90,90), IPCINT
C DO 30 J=1,N2
C DO 30 I=1,NS
C   K=1,NS
C   GNORM(I,J)=GNORM(I,J)+WNORM(I,K)*G(K,J)
C GO TO (40,70,90,90,80), IPCINT
C WRITE (6,170)
C DO 60 I=1,NS
C   WRITE (6,230) (GNORM(I,J),J=1,N2)
C RETURN
C WRITE (6,180)
C GO TO 50
C WRITE (6,240)
C GO TO 50
C DO 100 J=1,NS
C DO 100 I=1,N1
C DO 100 K=1,NS
C   GNORM(I,J)=GNORM(I,J)+G(I,K)*WNORM(K,J)
C GO TO (110,110,120,120,130,140), IPCINT
C WRITE (6,190)
C GO TO 150
C WRITE (6,200)
CPT131370
CPT131380
CPT131390
CPT131400
CPT131410
CPT16800
CPT16810
CPT16820
CPT16830
CPT16840
CPT16850
CPT16860
CPT16870
CPT16880
CPT16890
CPT16900
CPT16910
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CPT16970
CPT16980
CPT16990
CPT17000
CPT17010
CPT17020
CPT17030
CPT17040
CPT17050
CPT17060
CPT17070
CPT17080
CPT17090
CPT17100
CPT17110
CPT17120
CPT17130
CPT17140
CPT17150
CPT17160
CPT17170
CPT17180
CPT17190
CPT17200
CPT17210
CPT17220

```

```

130 GO TO 150
140 WRITE (6,210)
150 GO TO 150
160 WRITE (6,220)
170 DO 160 I=1,N1
180 WK ITE (6,230) (GNORM(I,J),J=1,NS)
190 RETURN
C-----
170 FORMAT (//,5X,45HMODAL CONTROL DISTRIBUTION MATRIX.....TI*G.,//)
180 FORMAT (//,5X,50HMODAL PROCESS NOISE DISTRIBUTION MATRIX.....TI*GAM.,
190 1.,//)
190 FURMAT (//,5X,45HMODAL MEASUREMENT SCALING MATRIX...H(BAR)*T.,//)
200 FURMAT (//,5X,45HMODAL MODAL CONTROL GAINS.....C#T.,//)
210 FURMAT (//,5X,45HMODAL EIGENVECTOR MATRIX.....C#M.,//)
220 FURMAT (//,5X,45HMODAL MEASUREMENT EIGENVECTOR MATRIX.....H(BAR)*M.,//)
230 FURMAT (1X,(2X,1P,6E14.6))
240 FURMAT (//,5X,45HMODAL FILTER STEADY STATE GAINS.....TI*K.,//)
C-----
C=====
SUBROUTINE CNORM (WZ,WY,VEC,NS,IWRITE,NSQ,DCG,D1,D2,WNORM,WNORMI,HC
10,CM,N1,N2)
C=====
      WZ(I)      REAL PART OF I-TH EIGENVALUE
      WY(I)      COMPLEX PART OF I-TH EIGENVALUE
      VEC        MATRIX OF RIGHT EIGENVECTORS STORED IN REAL FORM
                FROM HQR2
      NS         NO. OF STATES
      IWRITE     FLAG TO CONTROL FORMATS FOR DIFFERENT EIGENSYSYSTEMS=
      WNORM      NORMALIZED MATRIX U OF RIGHT EIGENVECTORS STORED
                BY COLUMNS IN REAL FORM
      WNCRMI     U-INVERSE 2*CONJUGATE OF LEFT EIGENVECTORS
                STORED BY ROW IN REAL FORM
      NSQ,DDG,D1,D2 - ARGUMENTS PASSED TO MINV
C=====
      IMPLICIT REAL*4 (A-H,O-Z)
      CHARACTER #8 FIELD,CCMMA,SEMCOL,RIGHT,FMT,SEMEMD
      DIMENSION WZ(NS),WY(NS),VEC(NS,NS),WNORM(NS,NS),WNORMI(NS,NS),STOR
15(6),D1(NS),D2(NS),FMT(14),HC(N1,N2),CM(N1,N2)
      DATA FIELD,E12.5,/,CCMMA/,/,SEMCOL/,/,SEMEMD/,/,RIGHT/,/
16FMT/,(1X,1P,13#.,/,SEMEMD/),/,SEMEMD/
C-----
      KK=0
      LR=0
      LC=0

```



```

C
10
20
30
40
50
C
60
70
80
90
100
110

DO 50 K=1,NS
IF (KK.EC.1) GO TO 40
IF (DABS(WY(K)).LT.1.D-10) GO TO 50
IF (ABS(WY(K)).LT.1.E-10) GO TO 50
LC=LC+1
EMAX=0.E0
DO 20 I=1,NS
CMCD=VEC(I,K)**2+VEC(I,K+1)**2
IF (CMCD-EMAX) 20,10,10
EMAX=CMCD
M=I
CONTINUE
VMR=VEC(M,K)
VM=VEC(M,K+1)
DO 30 I=1,NS
VR=VEC(I,K)
VI=VEC(I,K+1)
VECRN=(VR*VMR+VI*VMI)/EMAX
VEGIN=(-VR*VMI+VI*VMR)/EMAX
WIGRM(I,K)=VECRN
WIGRM(I,K+1)=VEGIN
CONTINUE
KK=1
GO TO 50
KK=0
CONTINUE
-----NORMALIZE REAL EIGENVECTORS BY THE TOTAL LENGTH-----
C
DO 80 K=1,NS
IF (DABS(WY(K)).GE.1.D-10) GO TO 80
IF (ABS(WY(K)).GE.1.E-10) GO TO 80
LR=LR+1
REMOD=C.E0
DO 60 I=1,NS
REMOD=VEC(I,K)**2+REMOD
RMCD=DSQRT(REMOD)
RMCD=SCRT(REMOD)
DO 70 I=1,NS
RVEC=VEC(I,K)/REMOD
WIGRM(I,K)=RVEC
CONTINUE
CONTINUE
GO TO (50,100,110,120,130), IWRITE
WRITE (6,320)
GO TO 140
WRITE (6,330)
GO TO 140
WRITE (6,340)
GO TO 140

```

```

CPT17710
CPT17720
CPT17730
CPT17730
CPT17740
CPT17750
CPT17760
CPT17770
CPT17780
CPT17790
CPT17800
CPT17810
CPT17820
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CPT18050
CPT18060
CPT18070
CPT18080
CPT18090
CPT18100
CPT18110
CPT18120
CPT18130
CPT18140
CPT18150

```







WURZCC12  
 WURZCC13  
 WURZCC14  
 WURZCC15  
 WURZCC16  
 WURZCC17  
 WURZCC18  
 WURZCC19  
 WURZCC20  
 WURZCC21  
 WURZCC22  
 WURZCC23  
 WURZCC24  
 WURZCC25  
 WURZCC26  
 WURZCC27  
 WURZCC28  
 WURZCC29  
 WURZCC30  
 WURZCC31  
 WURZCC32  
 WURZCC33  
 WURZCC34  
 WURZCC35  
 WURZCC36  
 WURZCC37  
 WURZCC38  
 WURZCC39  
 WURZCC40  
 WURZCC41  
 WURZCC42  
 WURZCC43  
 WURZCC44  
 WURZCC45  
 WURZCC46  
 WURZCC47  
 WURZCC48  
 WURZCC49  
 WURZCC50  
 WURZCC51  
 WURZCC52  
 WURZCC53  
 WURZCC54  
 WURZCC55  
 WURZCC56  
 WURZCC57  
 WURZCC58  
 WURZCC59

CALL WURZEL(A,B,N,THETA,EPS,NC)

DESCRIPTION OF PARAMETERS

A - SYMMETRIC, POSITIVE-DEFINITE, INPUT SQUARE MATRIX.  
 B - SYMMETRIC, CONTAINS SQUARE ROOT OF A, AFTER EXIT FROM WURZEL.  
 N - ORDER OF A AND B.  
 THETA - CONSTANT (SEE METHOD AND REMARKS). IF EIGENVALUES OF A ARE UNKNOWN, CHOOSE THETA CLOSE TO UNITY.  
 EPS - CONSTANT SPECIFYING DESIRED ACCURACY (SEE METHOD). FOR SIX PLACE ACCURACY CHOOSE EPS = 1.E-6  
 NC - ORDER OF A AND B.

REMARKS

PARAMETERS A,B,THETA, AND EPS ABOVE ARE ALL REAL\*8

THE CONVERSION PROCESS IS VERY SLOW IF THE LARGEST AND SMALLEST EIGENVALUES OF A DIFFER BY SEVERAL ORDERS OF MAGNITUDE.

SUBROUTINES AND FUNCTION SUBPROGRAM REQUIRED

NCNE

METHOD

IF X IS THE VECTOR ASSOCIATED WITH MATRIX A, THEN MATRIX A IS POSITIVE-DEFINITE IF  $X^*AX$  IS GREATER THAN ZERO. NCN THE SEQUENCE:

$B(K+1) = B(K) + C*(A-B(K)**2)$  ..1..

CONVERGES TO THE SQUARE ROOT OF A.

IN EXPRESSION ..1..  $C = \text{THETA}/2 * \text{SQRT}(\text{NORM}(A))$ , WHERE:

THETA IS A CONSTANT GREATER THAN ZERO AND LESS THAN THE

SQUARE ROOT OF ALPHA.

ALPHA IS THE QUOTIENT OF  $\text{NORM}(A)$ , DIVIDED BY THE MAXIMUM

EIGENVALUES OF A, AND IT IS GREATER OR EQUAL TO ONE.

$\text{NORM}(A)$  IS THE MAXIMUM VALUE OBTAINED BY ADDING EACH ROW

OF A ALL THE WAY ACROSS.

THE FIRST APPROXIMATION OF B, THE SQUARE ROOT MATRIX, IS

OBTAINED AS FOLLOWS;  $B(0) = 2.C * C \# A$

THE RATE OF CONVERGENCE OF ..1.. TO THE SQUARE ROOT OF A

IS GIVEN BY THE RATE OF CONVERGENCE TO ZERO OF THE

SEQUENCE:

$X(K) = (1 - \text{THETA}(\text{SQRT}(\text{LAMDAMIN}/\text{LAMDAMAX})))**K$   
 WHERE LAMDAMIN AND LAMDAMAX ARE THE MINIMUM AND MAXIMUM  
 EIGENVALUES OF A, RESPECTIVELY.

TC ACCELERATE CONVERGENCE THETA SHOULD BE CHOSEN CLOSE TO  
 THE SQUARE ROOT OF ALPHA





WURZC107  
 WURZC108  
 WURZC109  
 WURZC110  
 WURZC111  
 WURZC112  
 WURZC113  
 WURZC114  
 WURZC115  
 WURZC116  
 WURZC117  
 WURZC118  
 WURZC119  
 WURZC120  
 WURZC121  
 WURZC122  
 WURZC123  
 WURZC124  
 WURZC125  
 WURZC126  
 WURZC127  
 WURZC128  
 WURZC129

C COMPUTE MAXIMUM VALUE AS SHOWN IN PREVIOUS COMMENT.  
 C

DO 75 J=I,N  
 S=ABS(E(I,J)-BB(J))  
 IF (S-DELTA) 75,75,74  
 DELTA=S  
 74 WRITE(6,1000)DELTA  
 75 B(I,J)=BB(J)  
 80 CONTINUE

C SET SYMMETRIC TERMS IN MATRIX B.  
 C

NN=N-1  
 DO 90 I=1,NN  
 NJ=I+1  
 DO 90 J=NJ,N  
 B(J,I)=B(I,J)  
 90 B(I,I)=E(I,I)  
 WURZC124  
 IF (DELTA-EPS) 95,95,94  
 94 GO TO 95  
 95 RETURN  
 END

C \*\*\*\*\*  
 C \*\*\*\*\* THE END \*\*\*\*\*  
 C \*\*\*\*\*  
 C \*\*\*\*\*



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